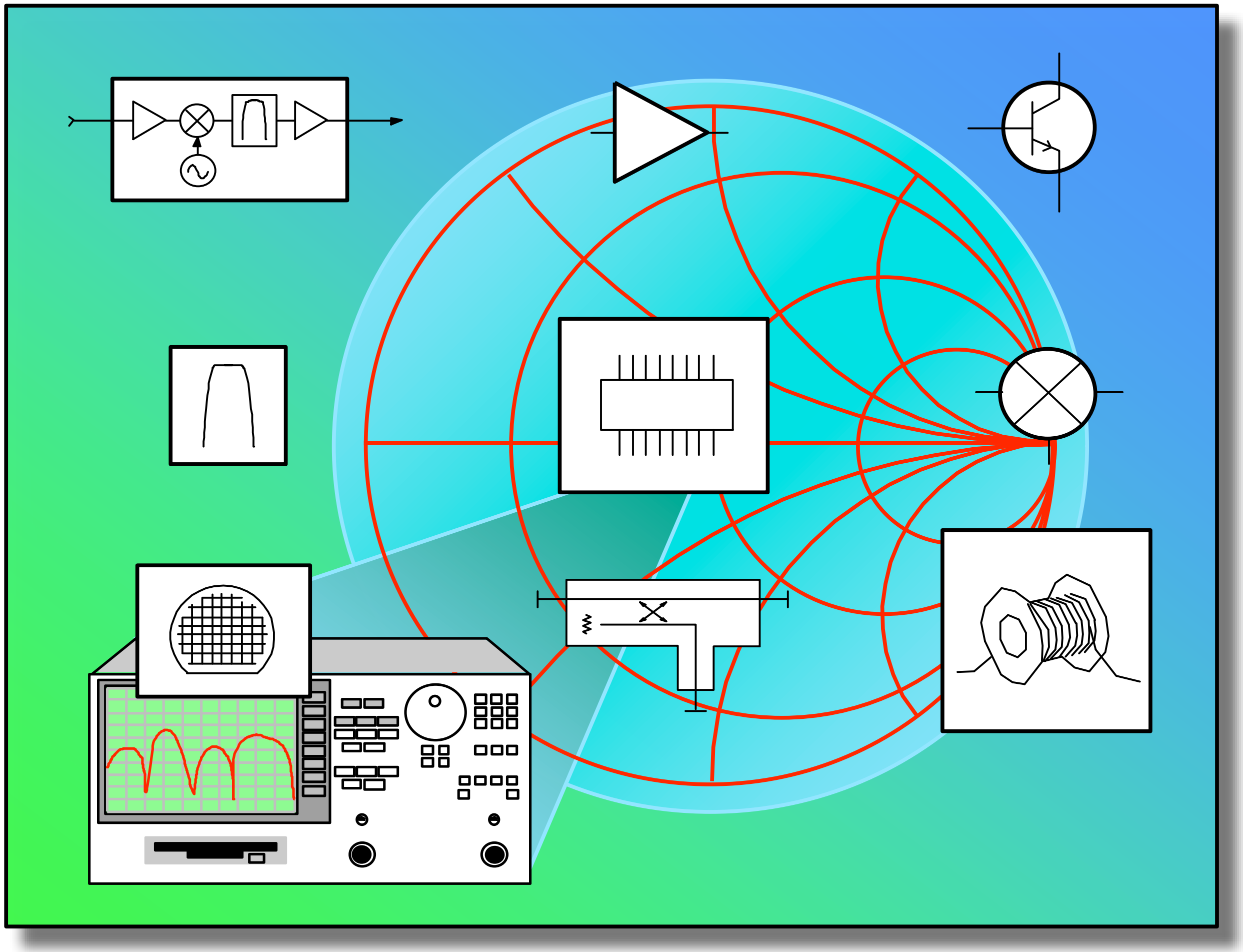
Network Analyzer Basics



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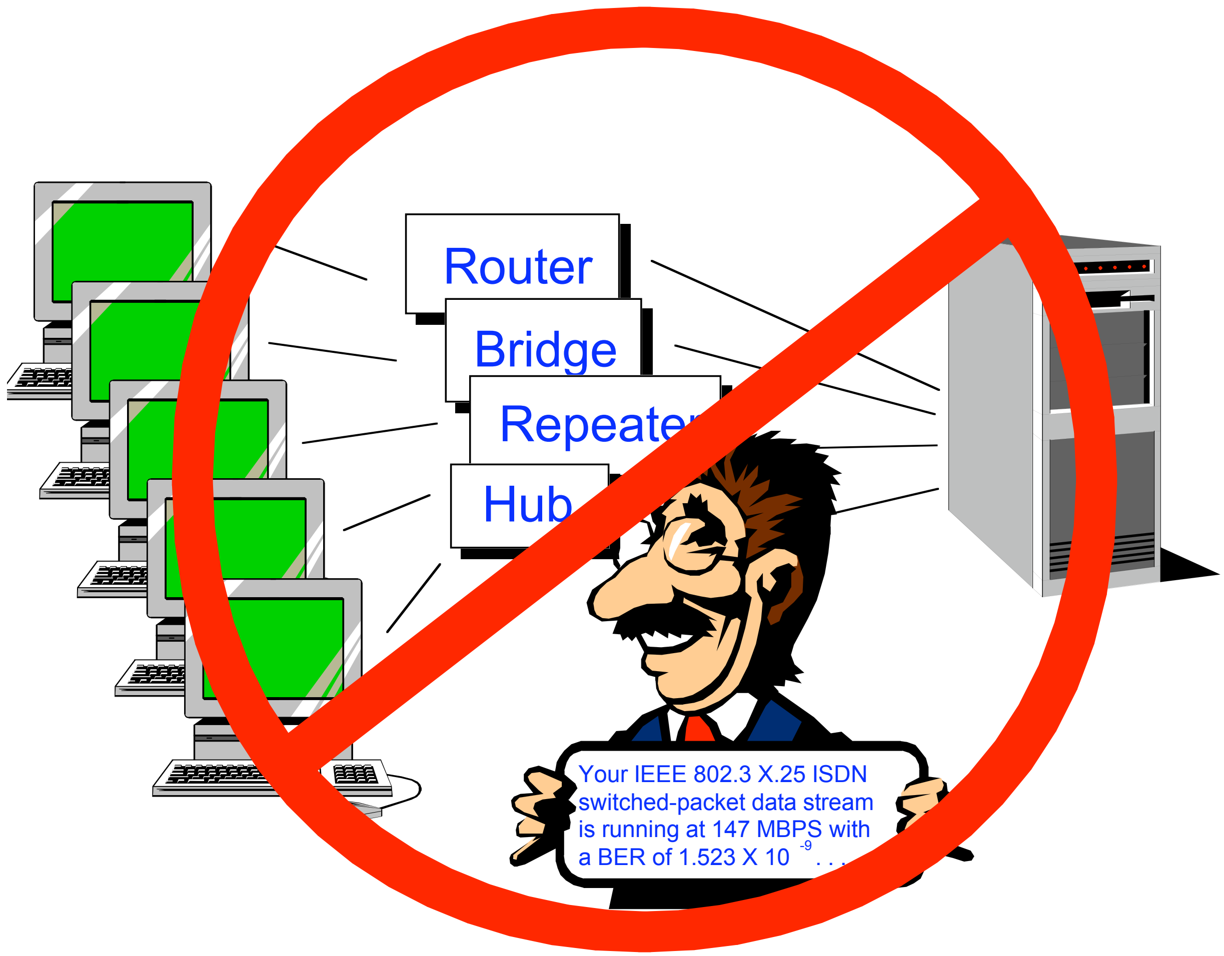
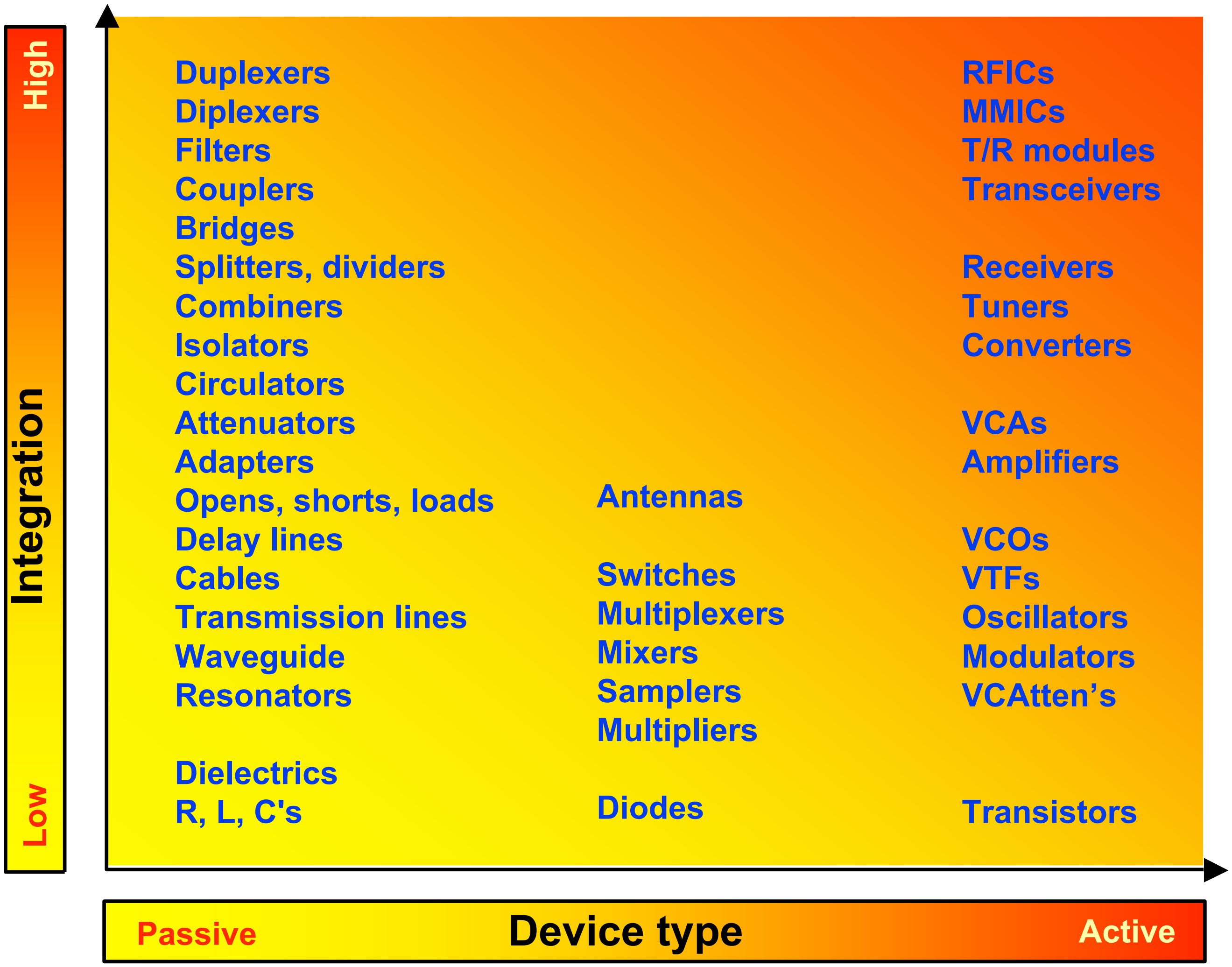
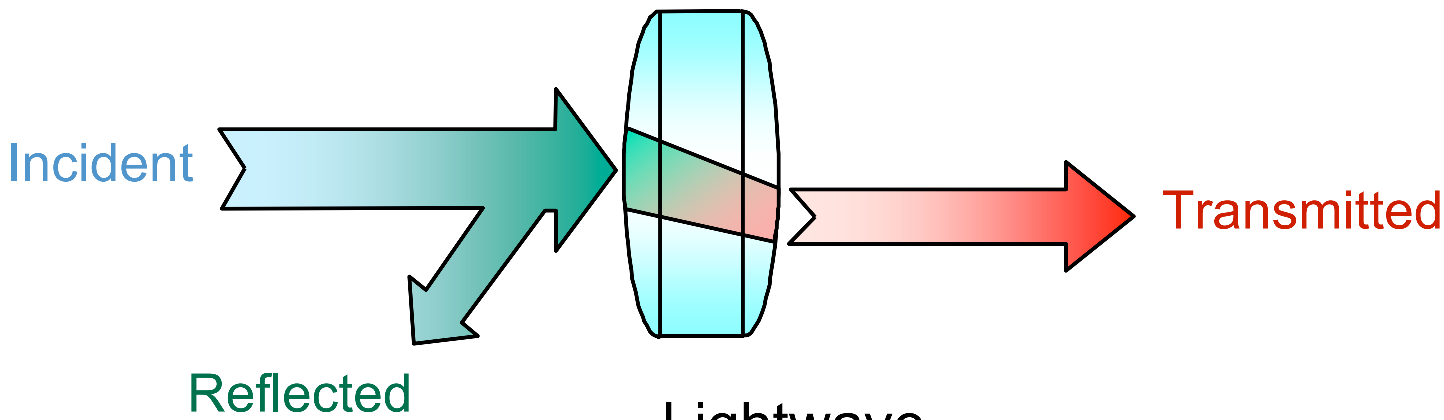
Network Analysis is NOT....



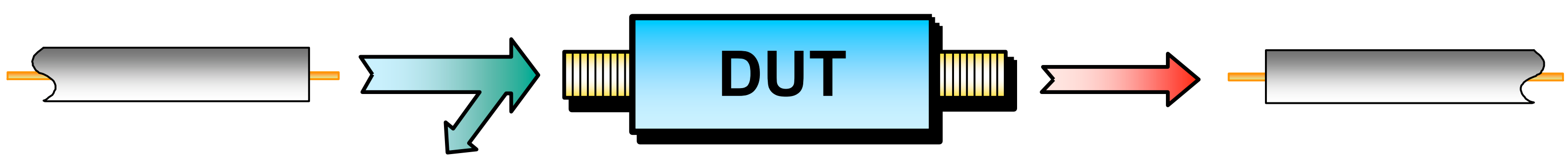
What Types of Devices are Tested?



Lightwave Analogy to RF Energy



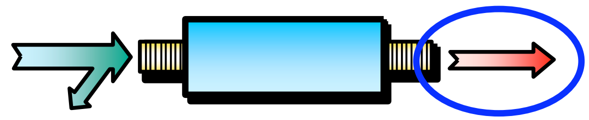
Lightwave



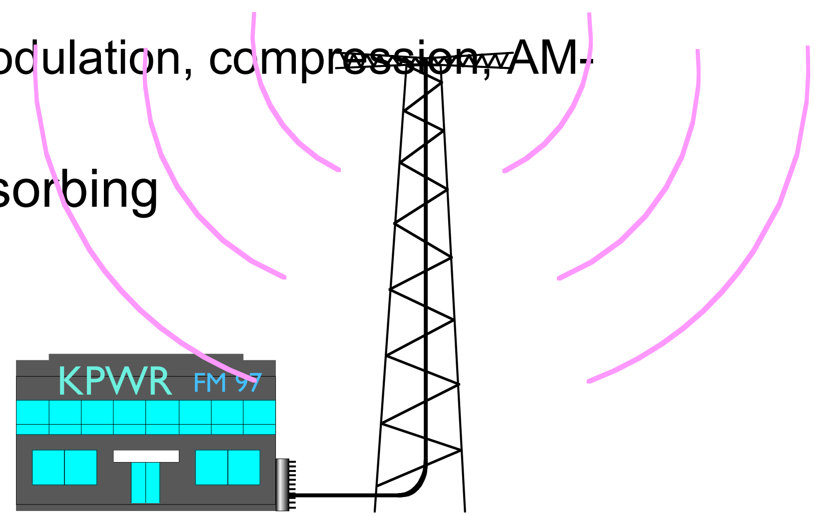
RF

Why Do We Need to Test Components?

- Verify specifications of “building blocks” for more complex RF systems

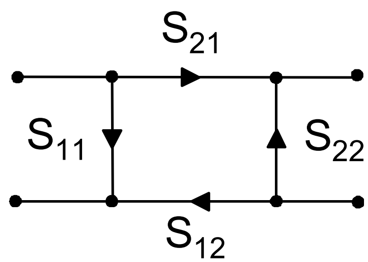


- Ensure distortionless transmission of communications signals
  - linear: constant amplitude, linear phase / constant group delay
  - nonlinear: harmonics, intermodulation, compression, AM-to-PM conversion
- Ensure good match when absorbing power (e.g., an antenna)

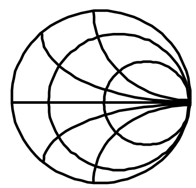


The Need for Both Magnitude and Phase

1. Complete characterization of linear networks

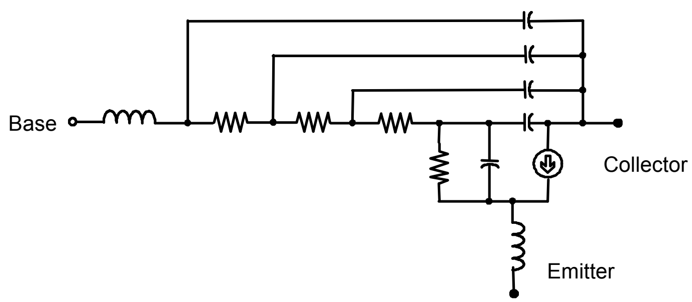


2. Complex impedance needed to design matching circuits

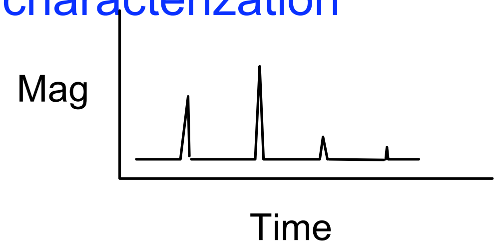


3. Complex values needed for device modeling

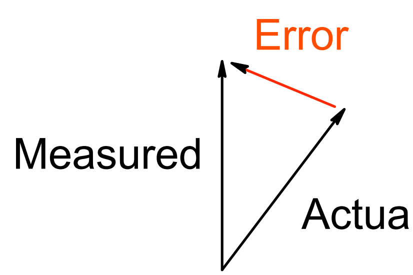
High-frequency transistor model



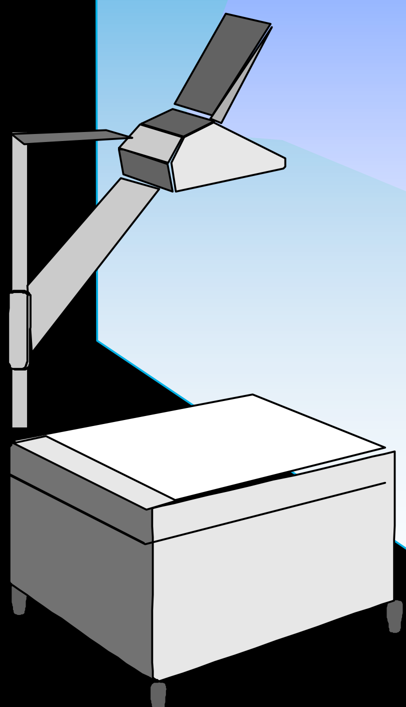
4. Time-domain characterization



5. Vector-error correction



Agenda

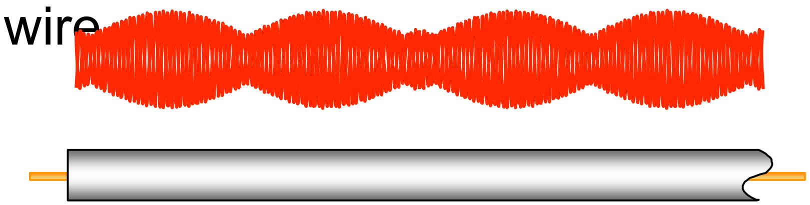


- **What measurements do we make?**
  - Transmission-line basics
  - Reflection and transmission parameters
  - S-parameter definition
- **Network analyzer hardware**
  - Signal separation devices
  - Detection types
  - Dynamic range
  - T/R versus S-parameter test sets
- **Error models and calibration**
  - Types of measurement error
  - One- and two-port models
  - Error-correction choices
  - Basic uncertainty calculations
- **Example measurements**
- **Appendix**

Transmission Line Basics

Low frequencies

- wavelengths >> wire length
- current (I) travels down wires easily for efficient power transmission
- measured voltage and current not dependent on position along wire

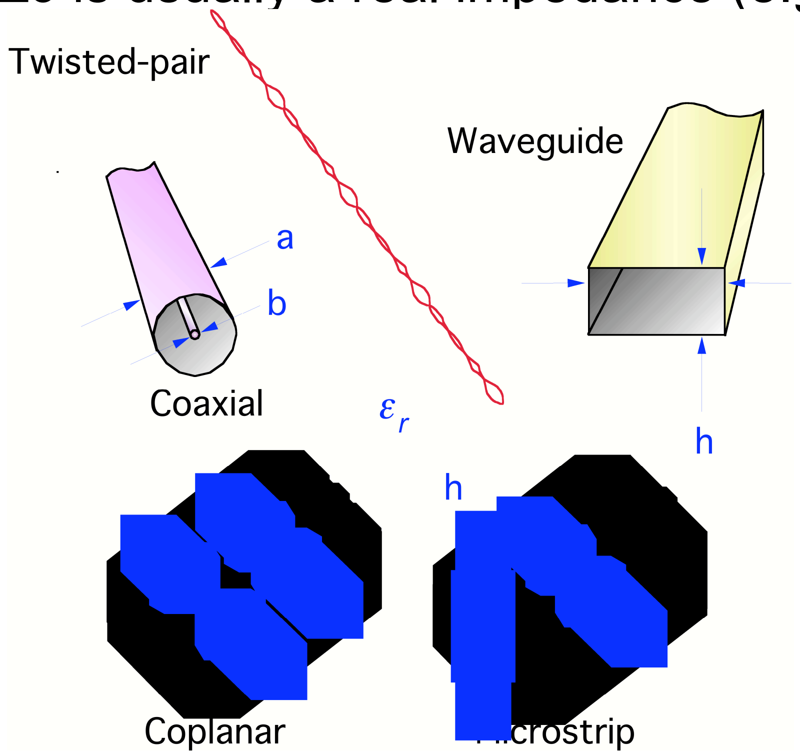


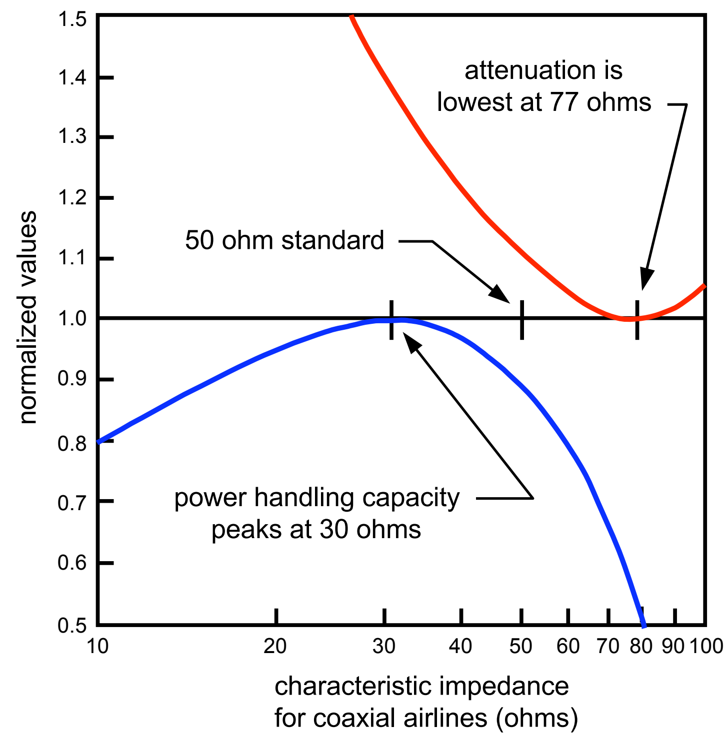
High frequencies

- wavelength ≈ or << length of transmission medium
- need transmission lines for efficient power transmission
- matching to characteristic impedance (Zo) is very important for low reflection and maximum power transfer
- measured envelope voltage dependent on

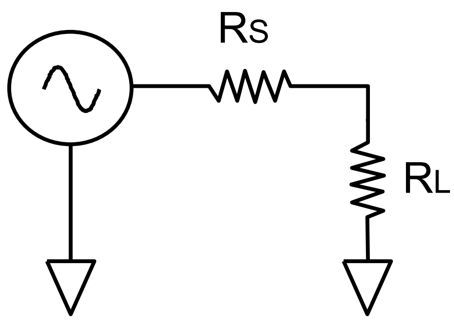
Transmission line Zo

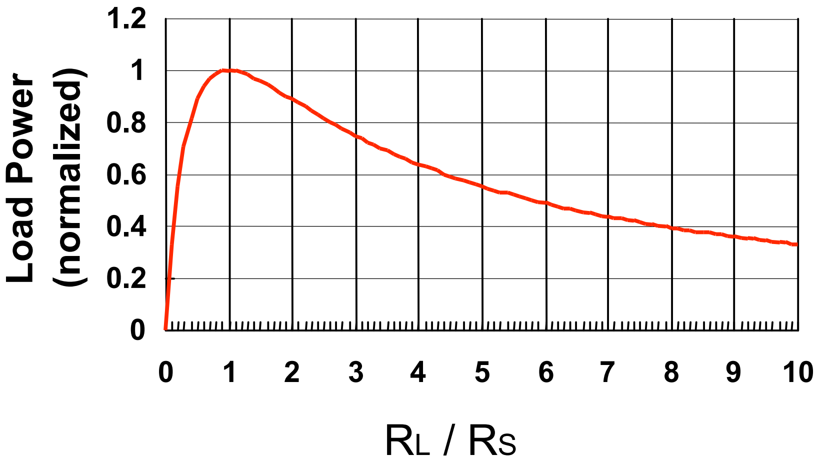
- Zo determines relationship between voltage and current waves
- Zo is a function of physical dimensions and ε_r
- Zo is usually a real impedance (e.g. 50 or 75 ohms)



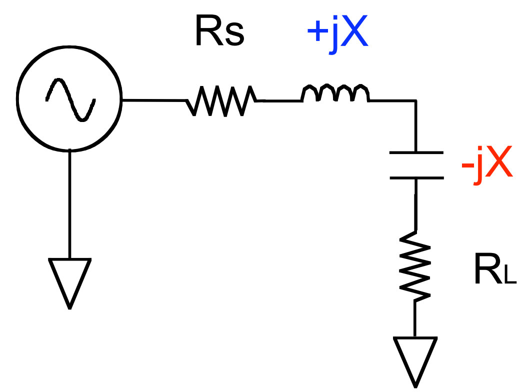


Power Transfer Efficiency





For complex impedances, maximum power transfer occurs when $Z_L = Z_S^*$ (conjugate match)



Maximum power is transferred when $R_L = R_S$

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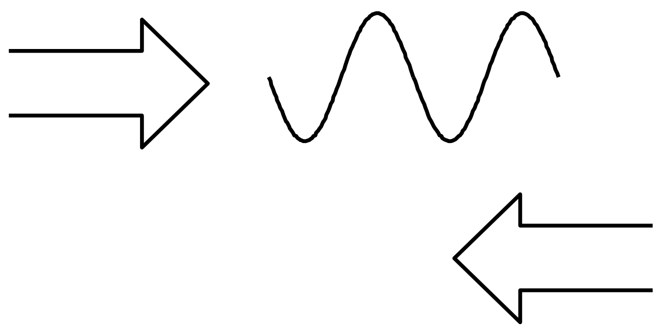
Transmission Line Terminated with Zo



For reflection, a transmission line terminated in Zo behaves like an infinitely long transmission line

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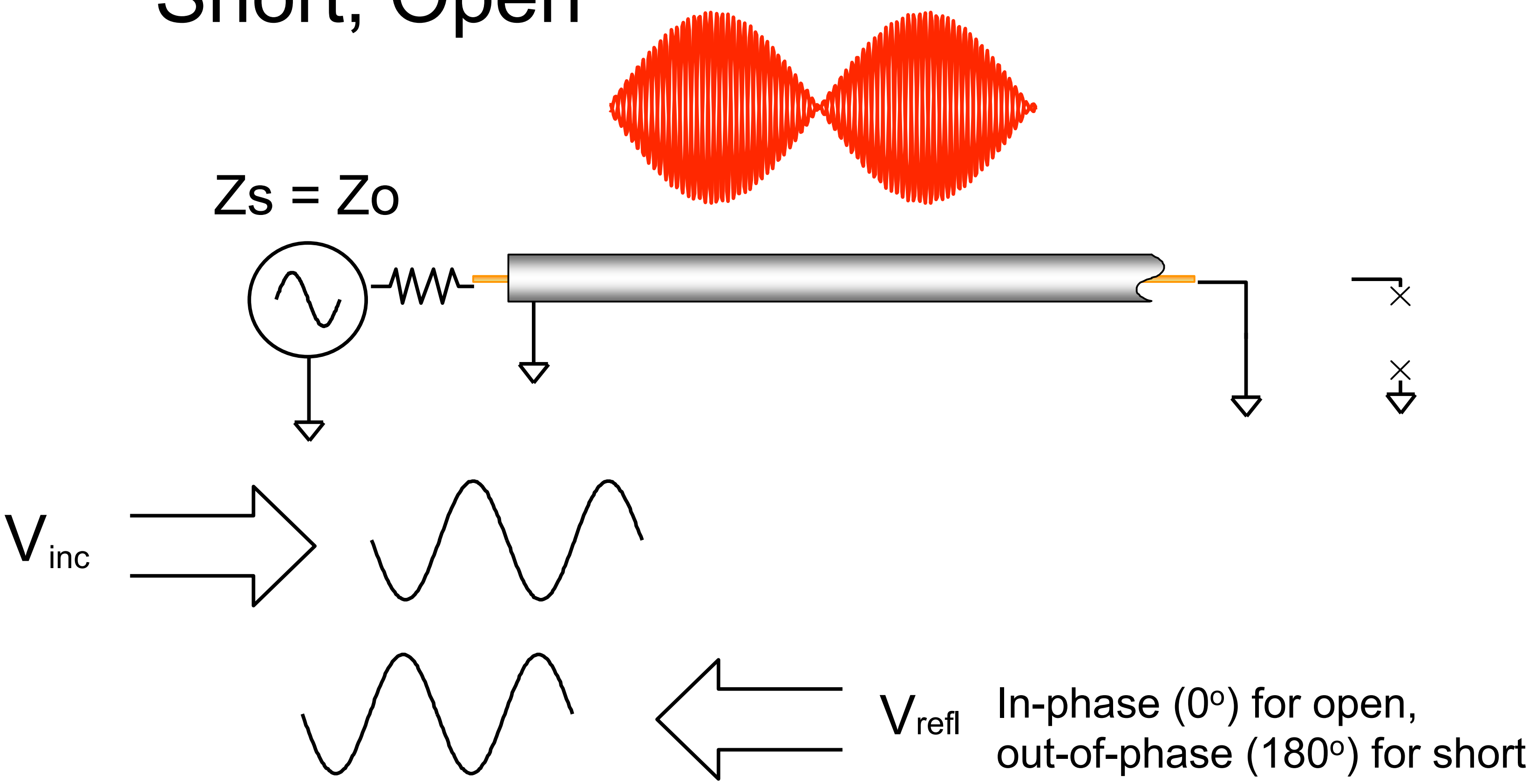
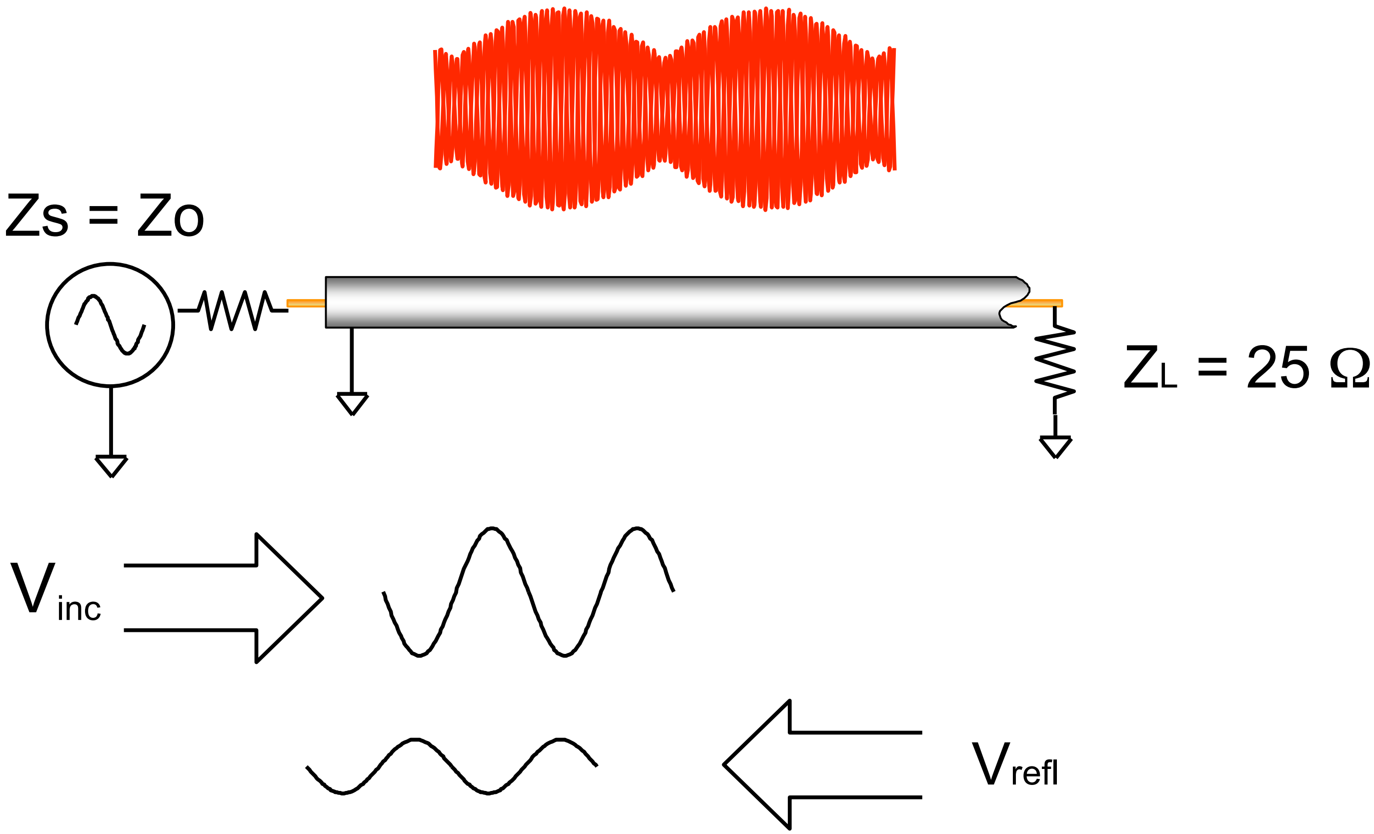
Transmission Line Terminated with Short, Open



In-phase (0°) for open, out-of-phase (180°) for short

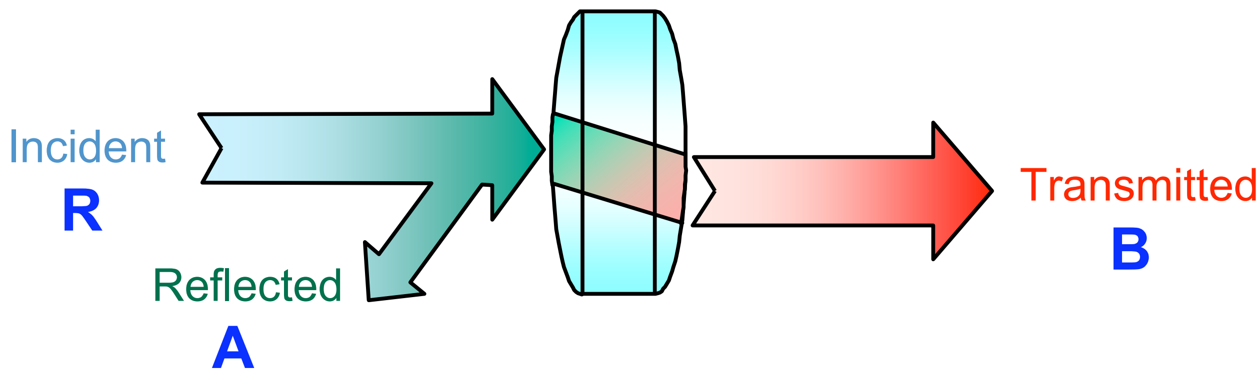
For reflection, a transmission line terminated in a short or open reflects all power back to source

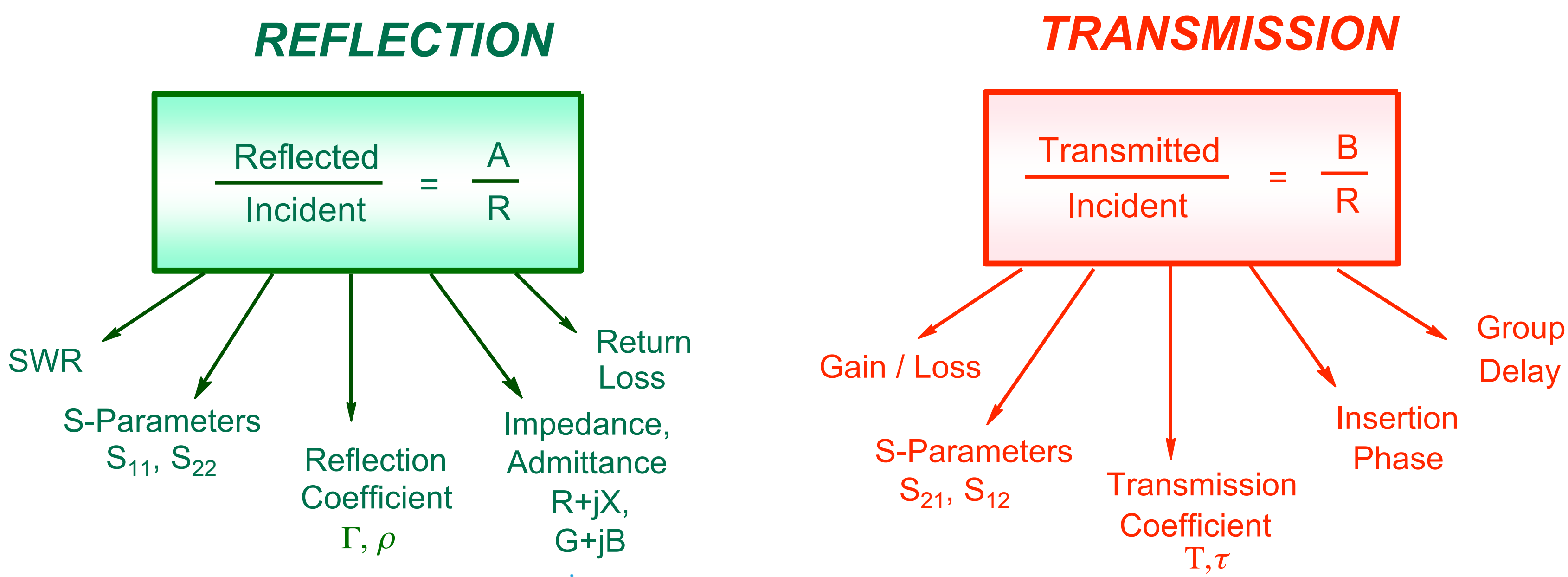
Transmission Line Terminated with 25 Ω



Standing wave pattern does not go to zero as with short or open

High-Frequency Device Characterization

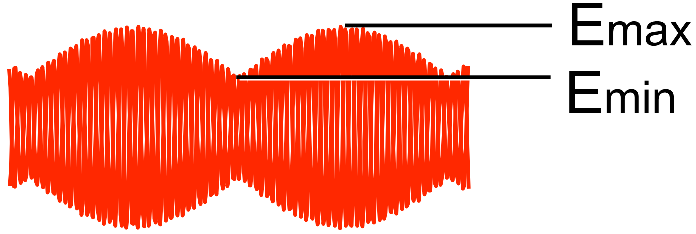




Reflection Parameters

Reflection Coefficient $\Gamma = \dfrac{V_{reflected}}{V_{incident}} = \rho \angle \Phi = \dfrac{Z_L - Z_O}{Z_L + Z_O}$

Return loss $= -20 \log(\rho), \quad \rho = |\Gamma|$

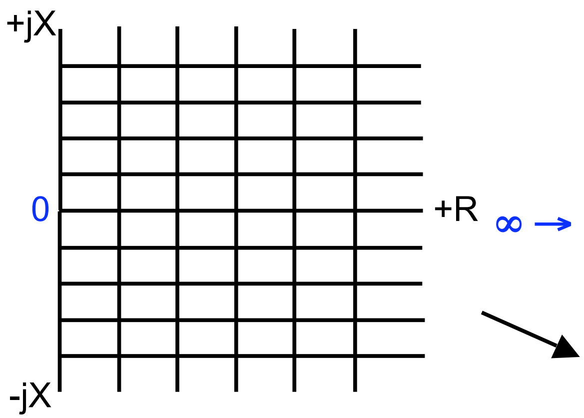


Voltage Standing Wave Ratio

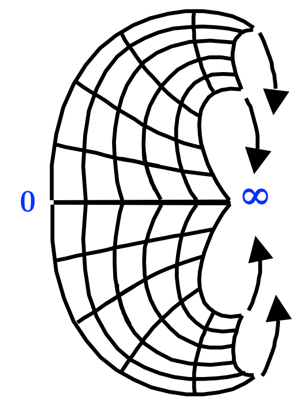
VSWR $= \dfrac{E_{max}}{E_{min}} = \dfrac{1 + \rho}{1 - \rho}$

No reflection ***($Z_L = Zo$)***		***Full reflection*** ***(Z_L = open, short)***
0	ρ	1
∞ dB	**RL**	0 dB
1	**VSWR**	∞

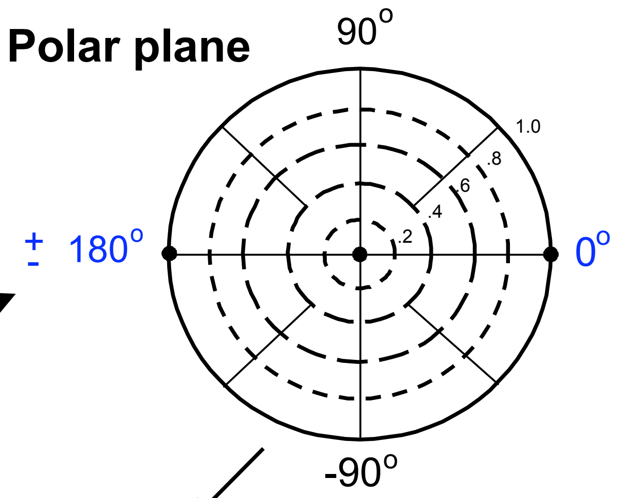
Smith Chart Review

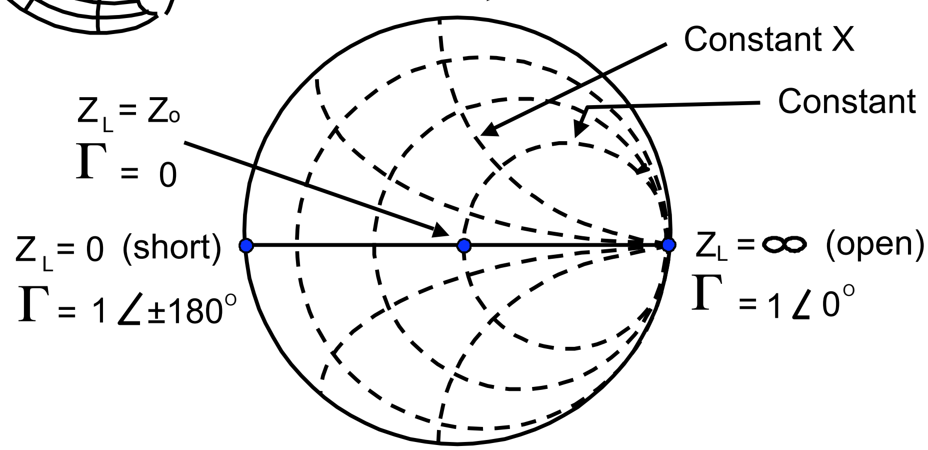


Rectilinear impedance plane



Polar plane





Smith chart

Smith Chart maps rectilinear impedance plane onto polar plane

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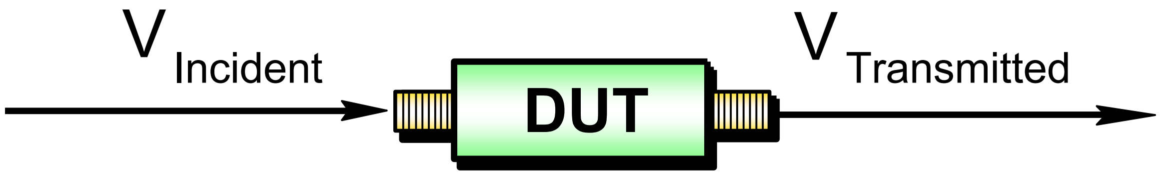
Transmission Parameters

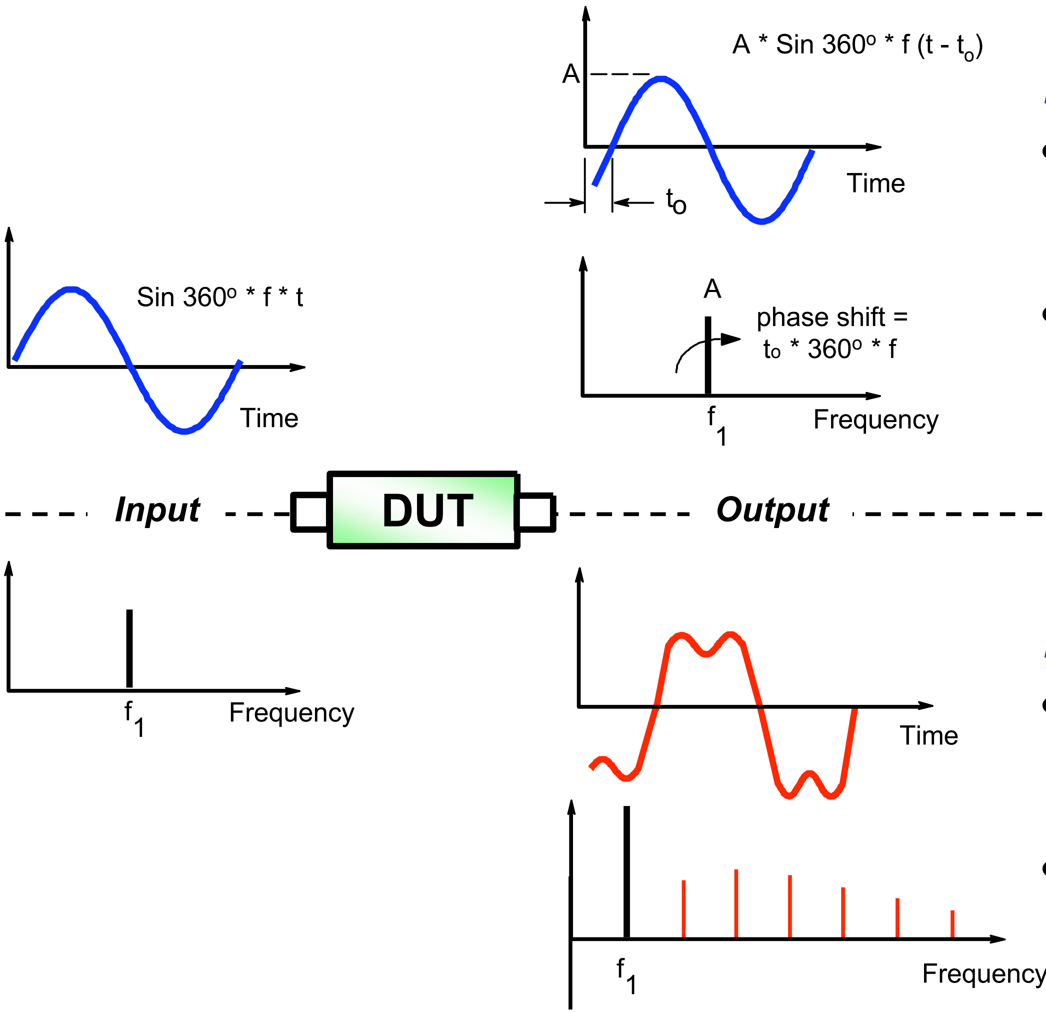


Transmission Coefficient $= T = \dfrac{V_{Transmitted}}{V_{Incident}} = \tau\angle\phi$

Insertion Loss (dB) $= -20 \text{ Log} \left| \dfrac{V_{Trans}}{V_{Inc}} \right| = -20 \log \tau$

Gain (dB) $= 20 \text{ Log} \left| \dfrac{V_{Trans}}{V_{Inc}} \right| = 20 \log \tau$

Linear Versus Nonlinear Behavior



Linear behavior:

- input and output frequencies are the same (no additional frequencies created)
- output frequency only undergoes magnitude and phase change

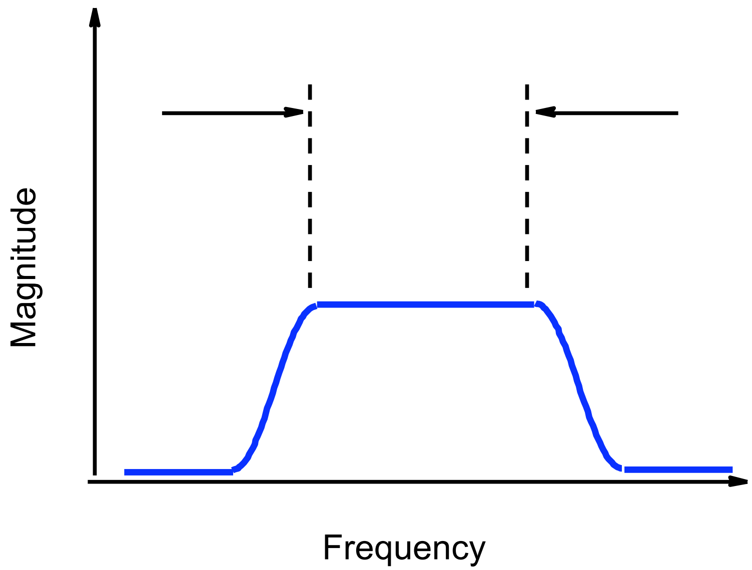
Nonlinear behavior:

- output frequency may undergo frequency shift (e.g. with mixers)
- additional frequencies created (harmonics, intermodulation)

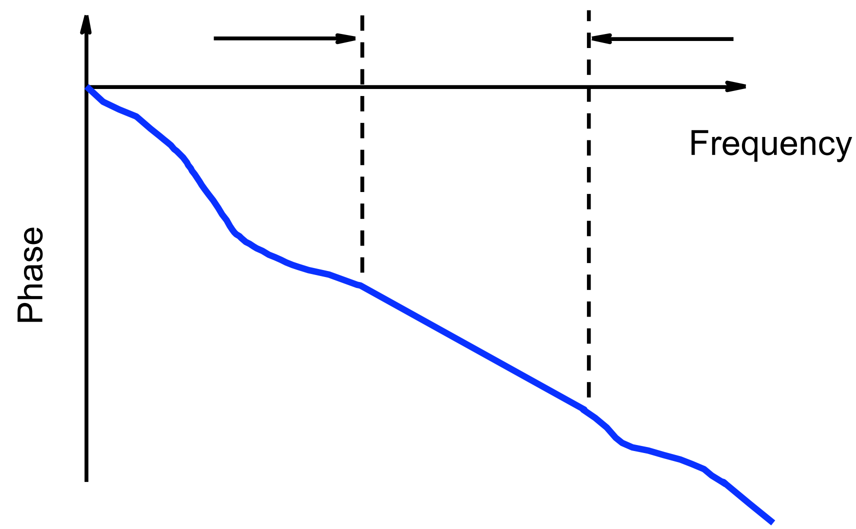
Criteria for Distortionless Transmission

Linear Networks

Constant amplitude over bandwidth of interest



Linear phase over bandwidth of interest



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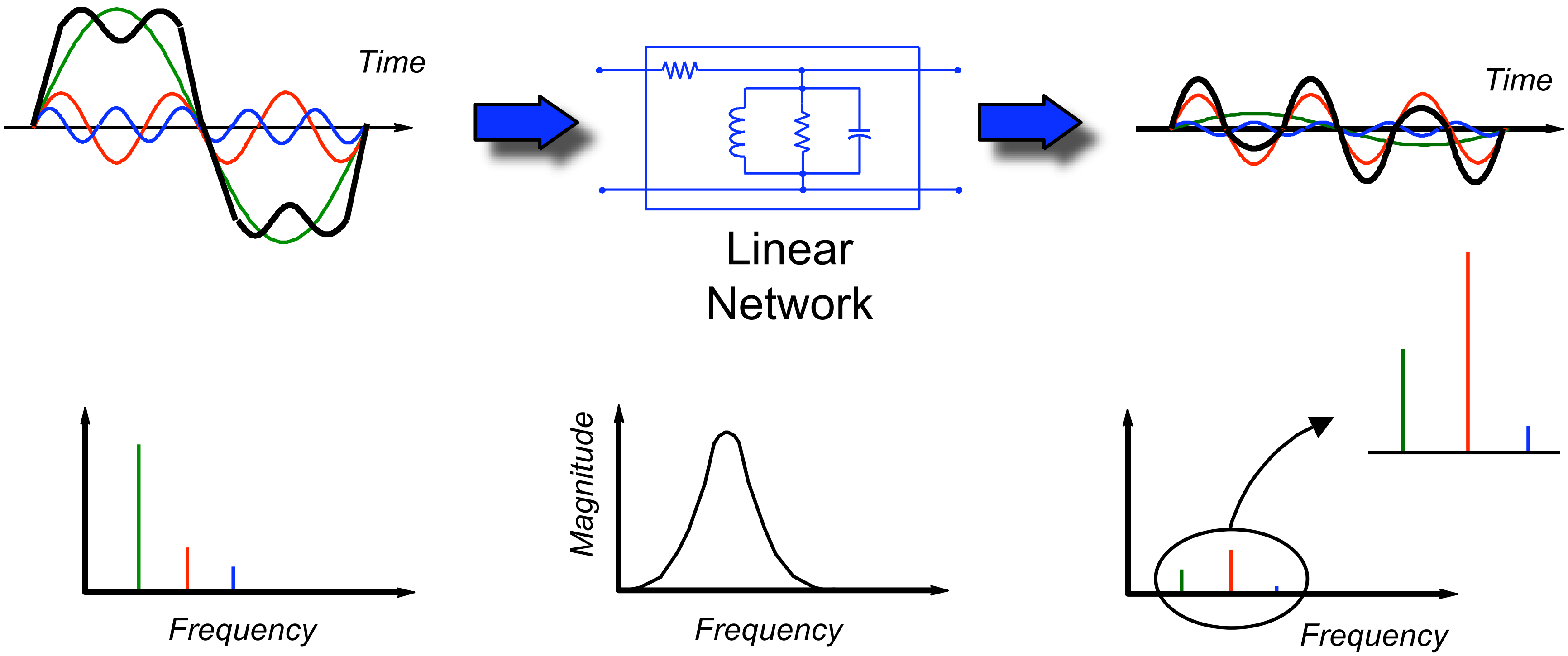
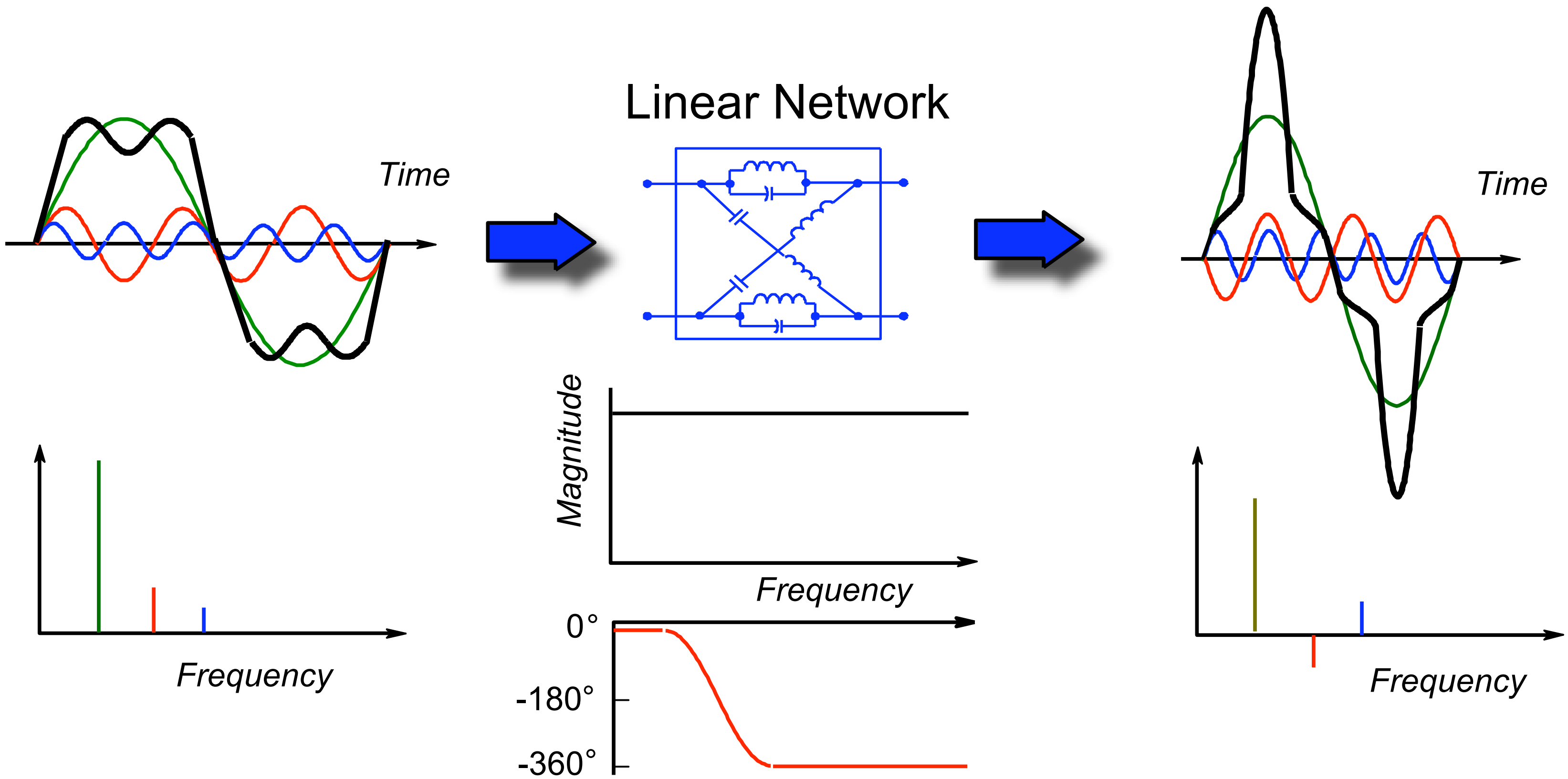
Magnitude Variation with Frequency

$$F(t) = \sin wt + \frac{1}{3} \sin 3wt + \frac{1}{5} \sin 5wt$$



Phase Variation with Frequency

$$F(t) = \sin wt + 1/3 \sin 3wt + 1/5 \sin 5wt$$



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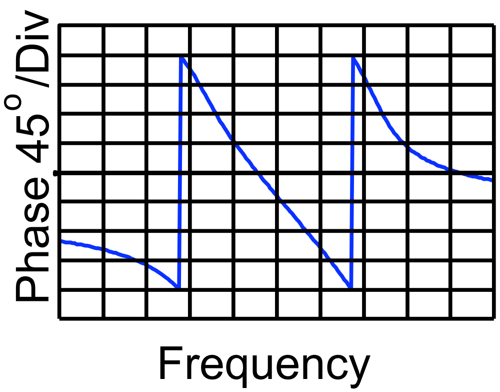
Deviation from Linear Phase

Use electrical delay to remove linear portion of phase response

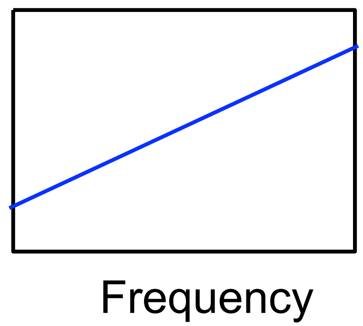
RF filter response



+

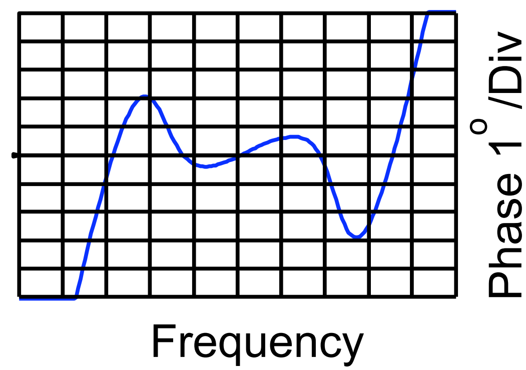
Linear electrical length added

(Electrical delay function)



yields

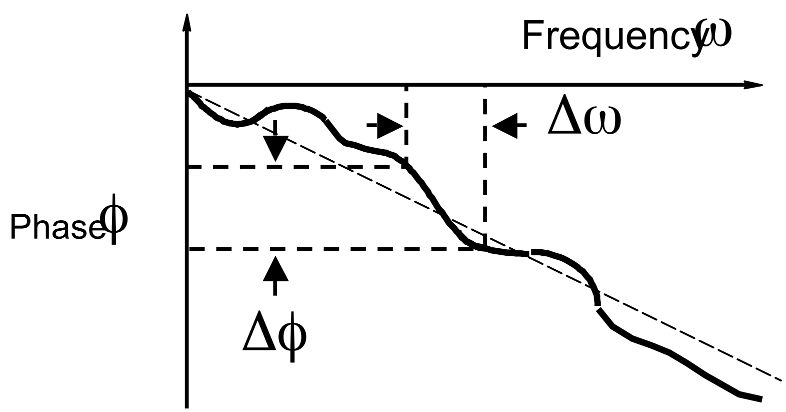
Deviation from linear phase

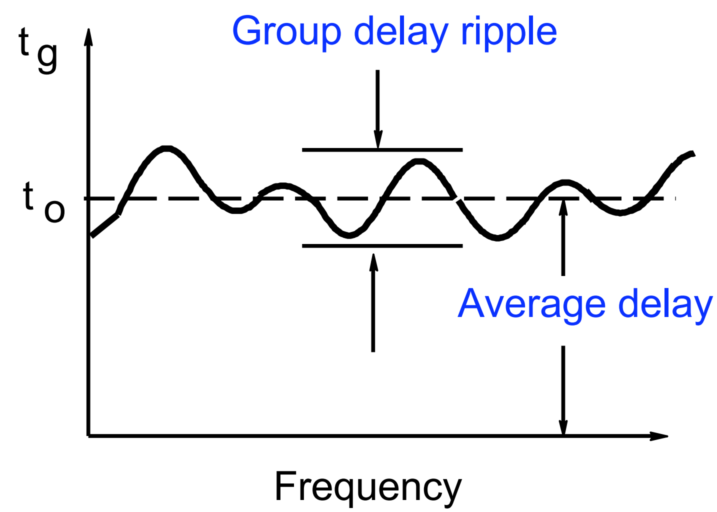


Low resolution

High resolution

Group Delay





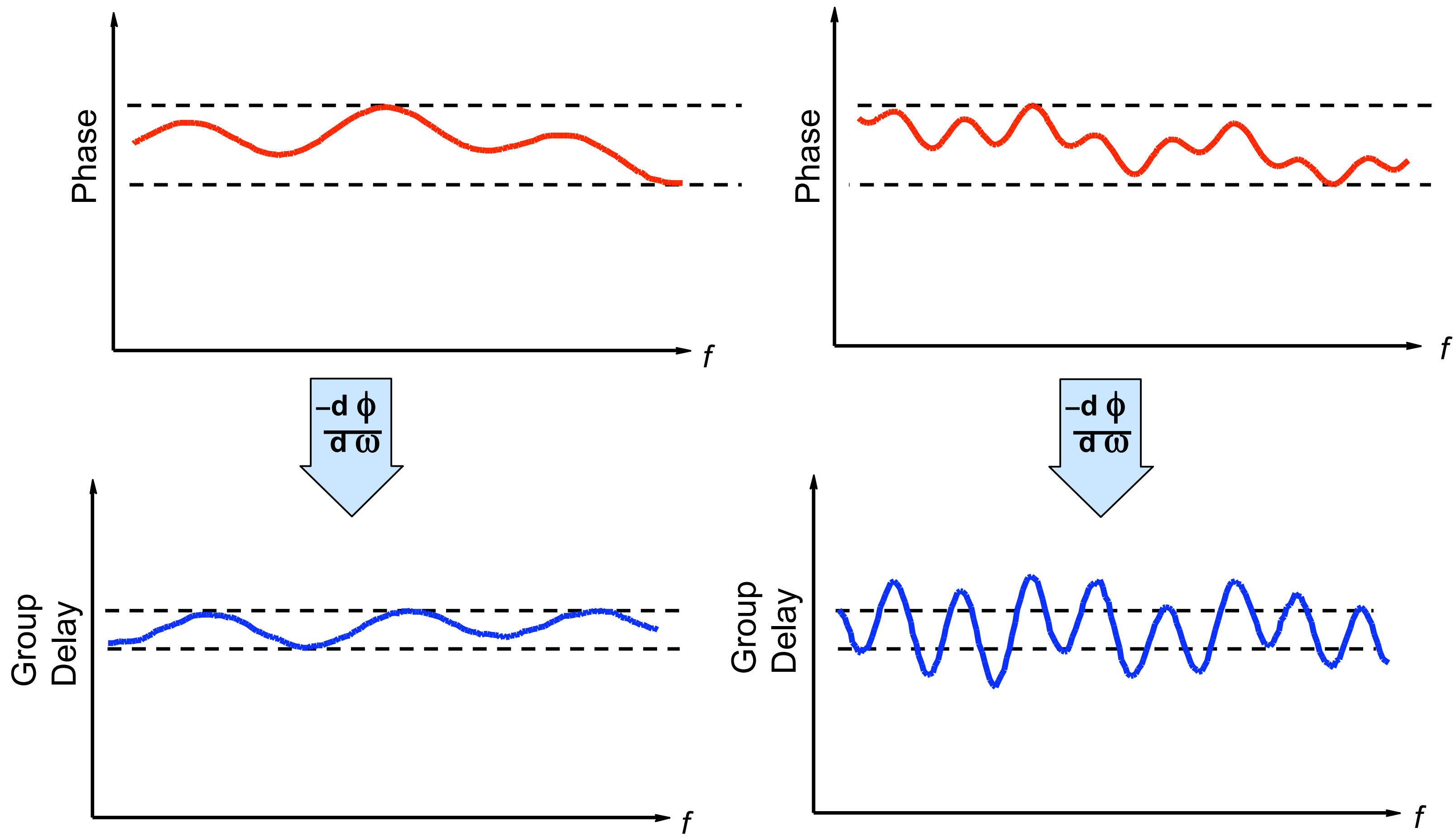
Group Delay (t_g) =

$$\frac{-d\,\phi}{d\,\omega} = \frac{-1}{360^{o}} * \frac{d\,\phi}{d\,f}$$

- ϕ in radians
- ω in radians/sec
- ϕ in degrees
- f in Hertz ($\omega = 2\pi f$)

- group-delay ripple indicates phase distortion
- average delay indicates electrical length of DUT
- aperture of measurement is very important

Why Measure Group Delay?



Same p-p phase ripple can result in different group delay

Characterizing Unknown Devices

Using parameters (H, Y, Z, S) to characterize devices:

- gives linear behavioral model of our device
- measure parameters (e.g. voltage and current) versus frequency under various source and load conditions (e.g. short and open circuits)
- compute device parameters from measured data
- predict circuit performance under any source and load conditions

H-parameters

$V_1 = h_{11}I_1 + h_{12}V_2$

$I_2 = h_{21}I_1 + h_{22}V_2$

Y-parameters

$I_1 = y_{11}V_1 + y_{12}V_2$

$I_2 = y_{21}V_1 + y_{22}V_2$

Z-parameters

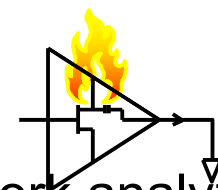
$V_1 = z_{11}I_1 + z_{12}I_2$

$V_2 = z_{21}I_1 + z_{22}I_2$

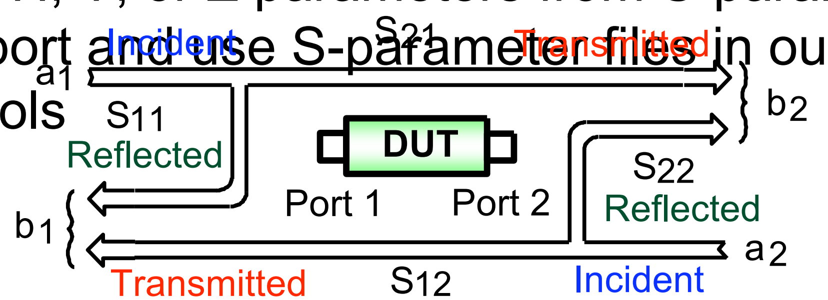
$$h_{11} = \left.\frac{V_1}{I_1}\right|_{V_2=0}$$ *(requires **short circuit**)*

$$h_{12} = \left.\frac{V_1}{V_2}\right|_{I_1=0}$$ *(requires **open circuit**)*

Why Use S-Parameters?



- relatively easy to **obtain** at high frequencies
  - measure voltage traveling waves with a vector network analyzer
  - don't need shorts/opens which can cause active devices to oscillate or self-destruct
- relate to **familiar** measurements (gain, loss, reflection coefficient ...)
- can **cascade** S-parameters of multiple devices to predict system performance
- can **compute** H, Y, or Z parameters from S-parameters if desired
- can easily import and use S-parameter files in our **electronic-simulation** tools

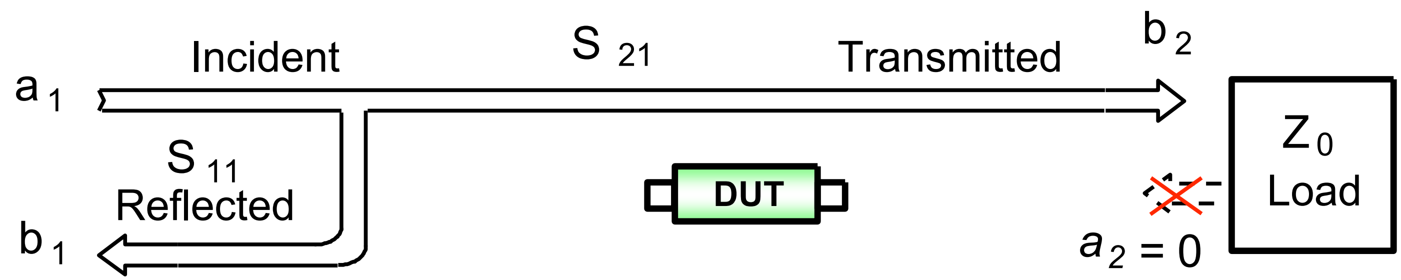


$$b_1 = S_{11} a_1 + S_{12} a_2$$

$$b_2 = S_{21} a_1 + S_{22} a_2$$

Measuring S-Parameters

Forward



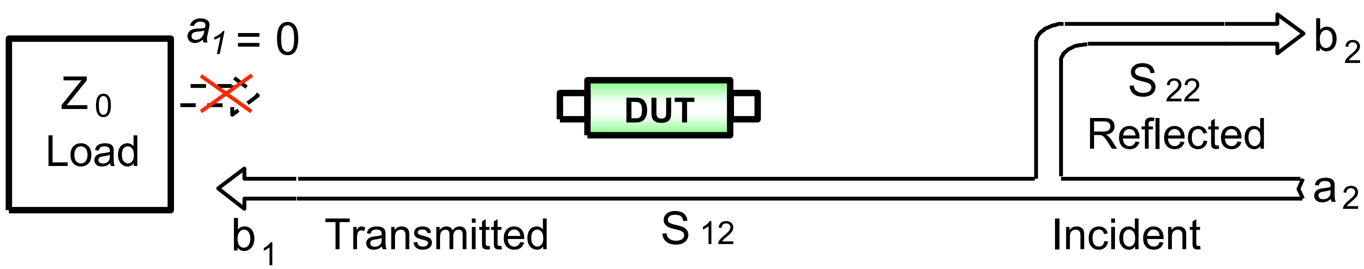
$$S_{11} = \frac{\text{Reflected}}{\text{Incident}} = \left.\frac{b_1}{a_1}\right|_{a_2 = 0}$$

$$S_{21} = \frac{\text{Transmitted}}{\text{Incident}} = \left.\frac{b_2}{a_1}\right|_{a_2 = 0}$$

$$S_{22} = \frac{\text{Reflected}}{\text{Incident}} = \left.\frac{b_2}{a_2}\right|_{a_1 = 0}$$

$$S_{12} = \frac{\text{Transmitted}}{\text{Incident}} = \left.\frac{b_1}{a_2}\right|_{a_1 = 0}$$

Reverse



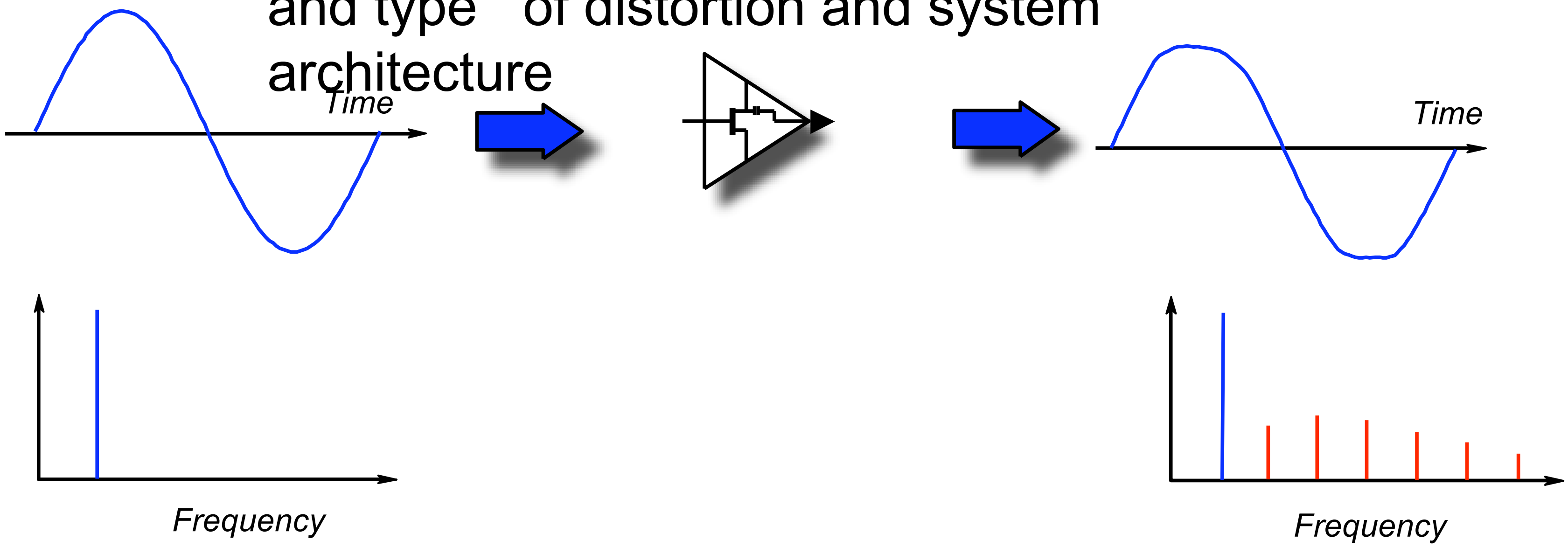
Equating S-Parameters with Common Measurement Terms

S11 = forward reflection coefficient ***(input match)***
S22 = reverse reflection coefficient ***(output match)***
S21 = forward transmission coefficient ***(gain or loss)***
S12 = reverse transmission coefficient ***(isolation)***

Remember, S-parameters are inherently complex, linear quantities -- however, we often express them in a log-magnitude format

Criteria for Distortionless Transmission
Nonlinear Networks

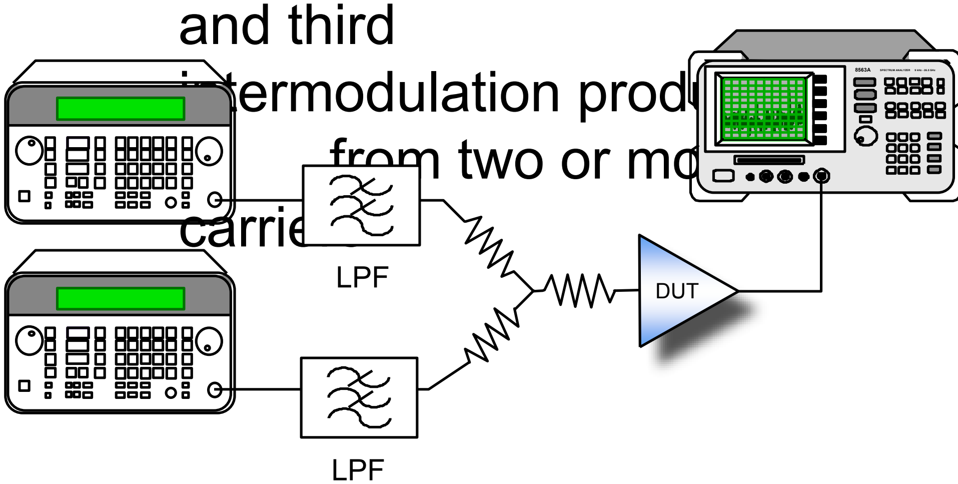
- Saturation, crossover, intermodulation, and other nonlinear effects can cause signal distortion
- Effect on system depends on amount and type of distortion and system architecture

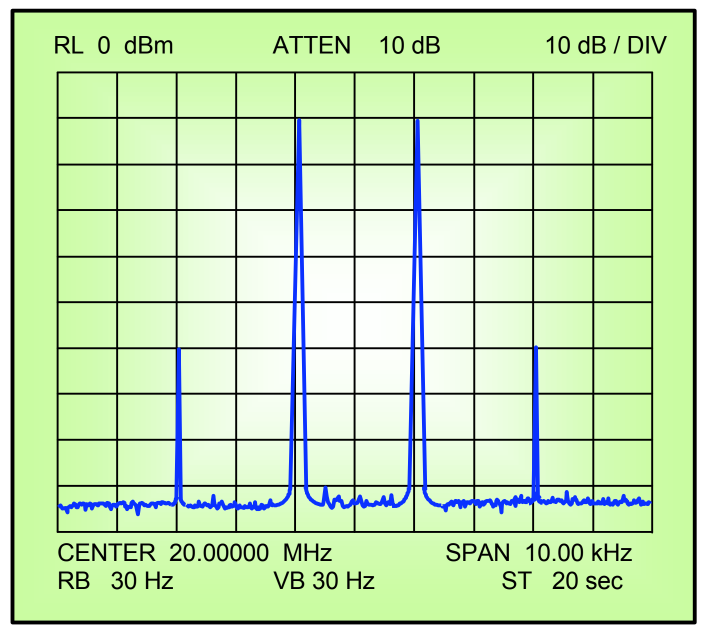


Measuring Nonlinear Behavior

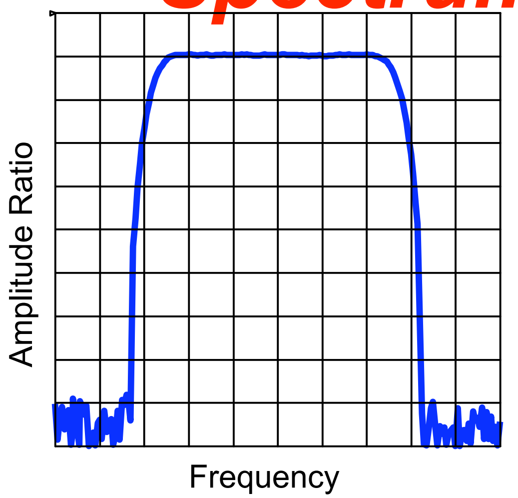
Most common measurements:

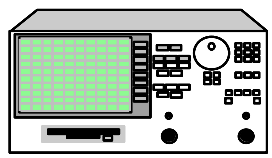
- using a ***network analyzer*** and power sweeps
  - gain compression
  - AM to PM conversion
- using a ***spectrum analyzer*** + source(s)
  - harmonics, particularly second and third
  - intermodulation products resulting from two or more carriers



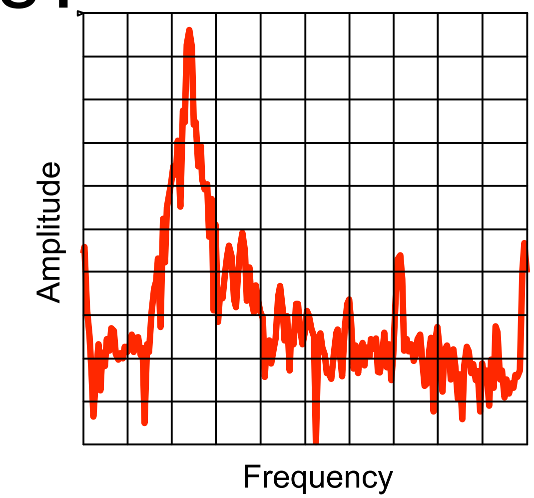


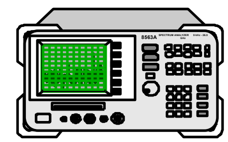
What is the Difference Between ***Network*** and ***Spectrum*** Analyzers?





Measures known signal





Measures unknown signals

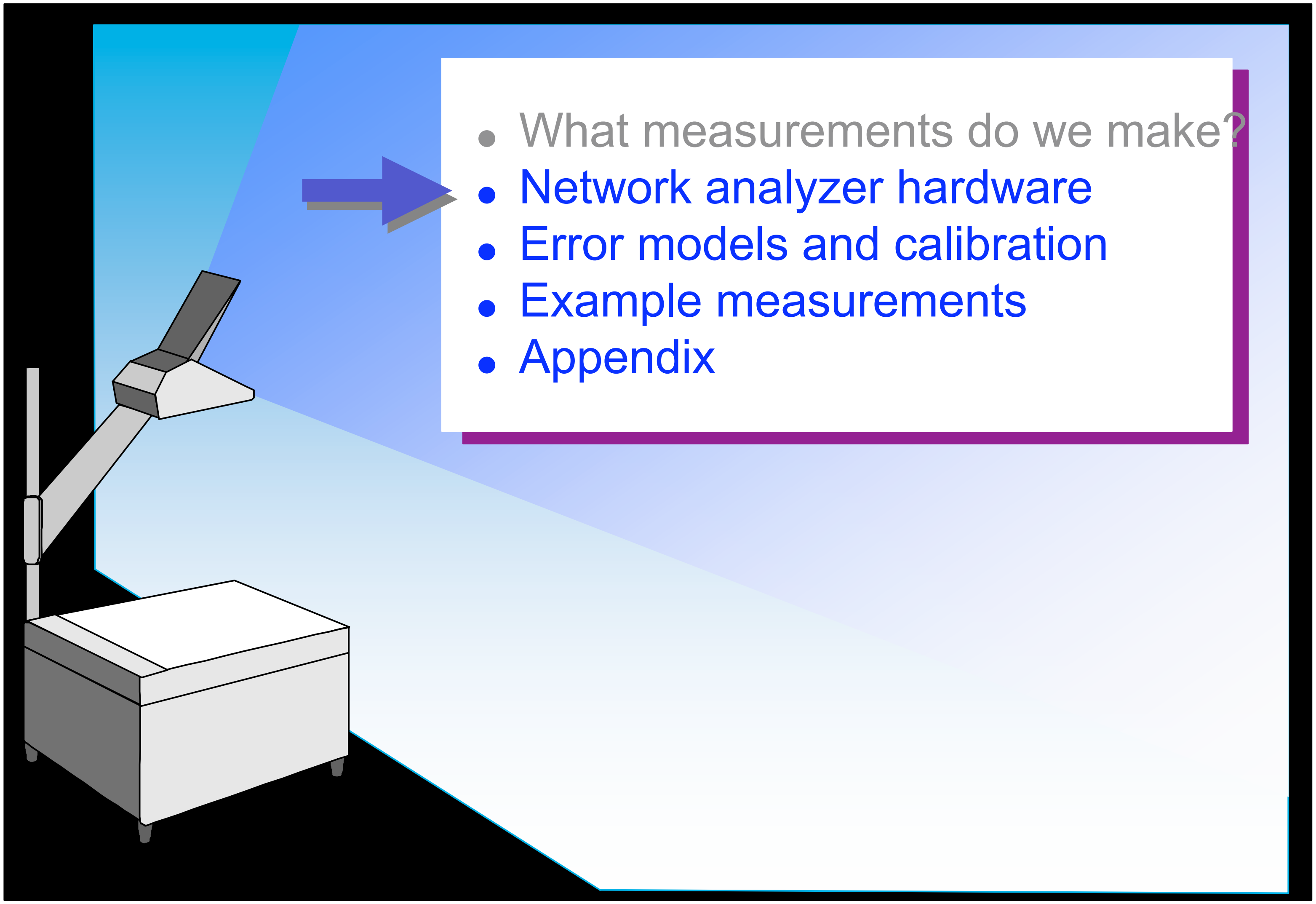
Network analyzers:

- measure components, devices,
  circuits, sub-assemblies
- contain source and receiver
- display ratioed amplitude and phase
  (frequency or power sweeps)
- offer advanced error correction

Spectrum analyzers:

- measure signal amplitude characteristics
  carrier level, sidebands, harmonics...)
- can demodulate (& measure) complex signals
- are receivers only (single channel)
- can be used for scalar component test (*no* phase) with tracking gen. or ext.

Agenda



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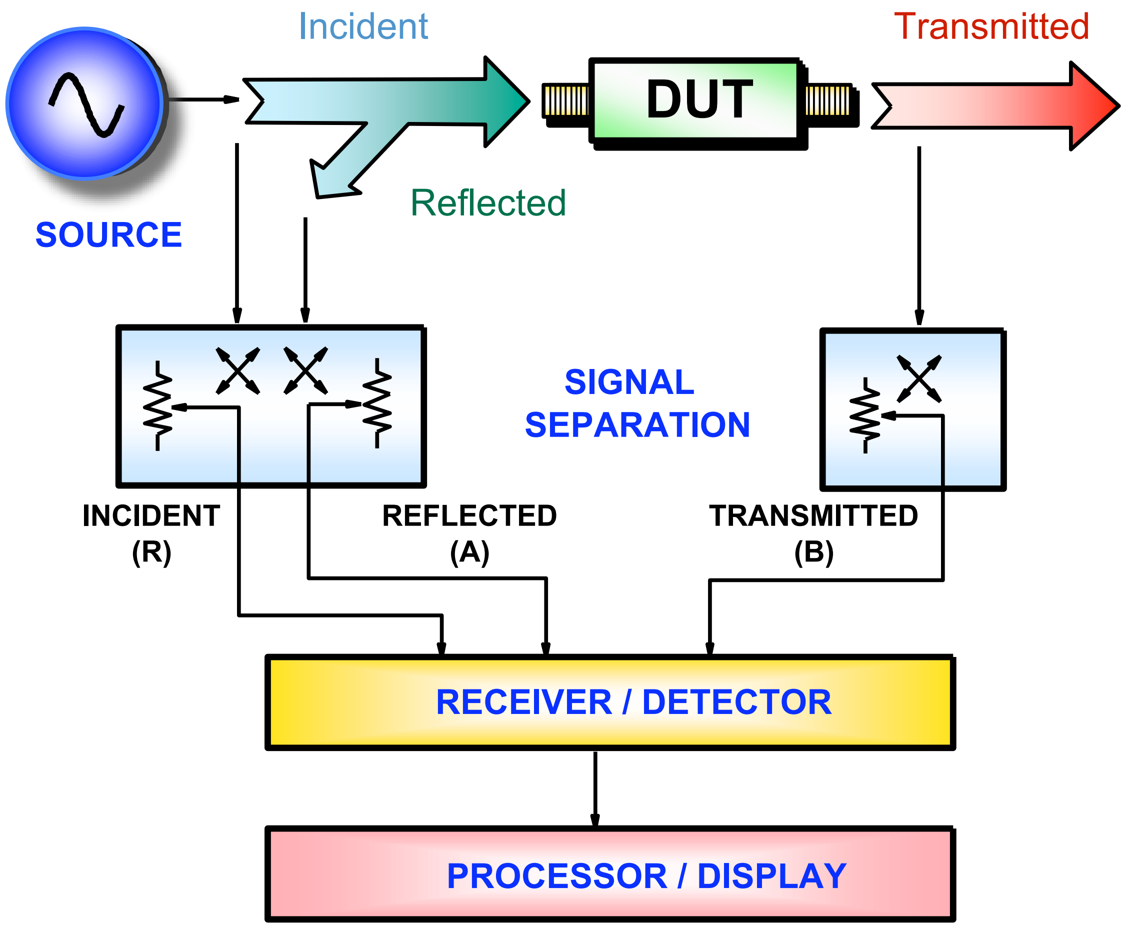
Generalized Network Analyzer Block Diagram



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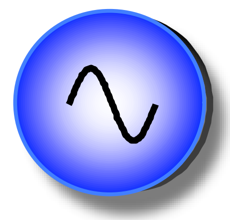
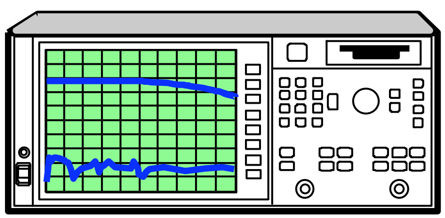
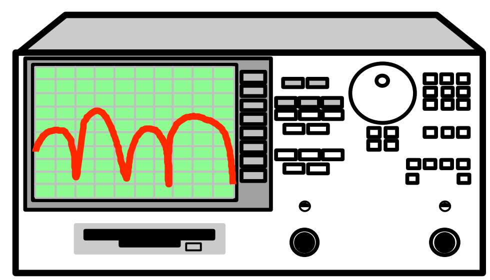
Source

- Supplies stimulus for system
- Swept frequency or power
- Traditionally NAs used separate source
- Most Agilent analyzers sold today have ***integrated, synthesized*** sources







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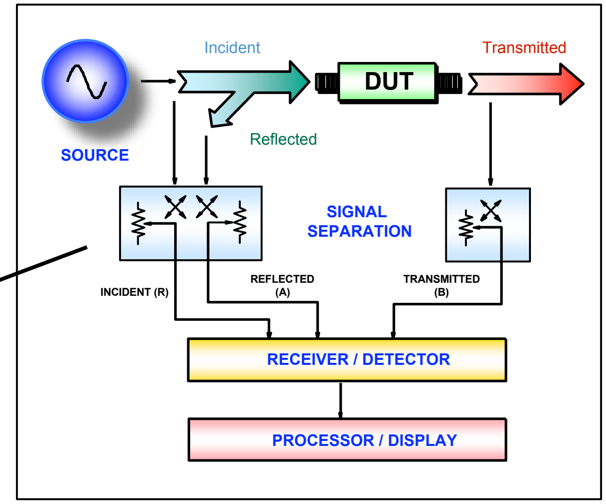
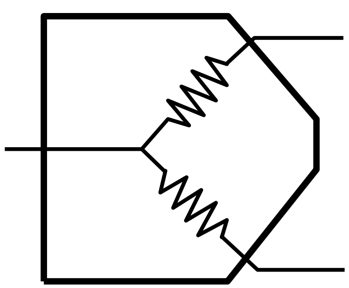
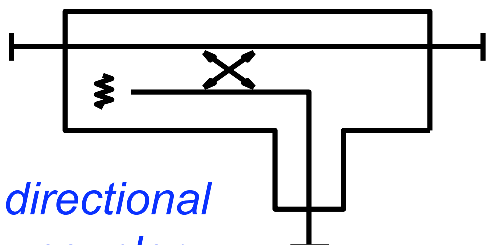
Signal Separation



- measure incident signal for reference
- separate incident and reflected signals

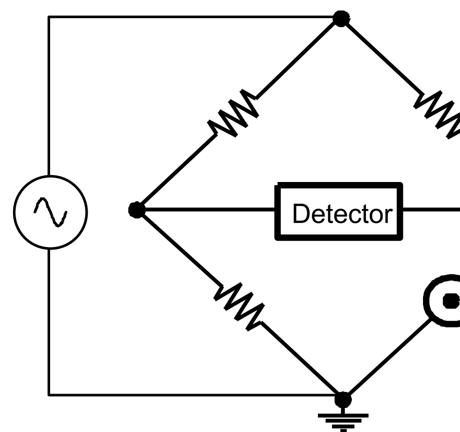
splitter





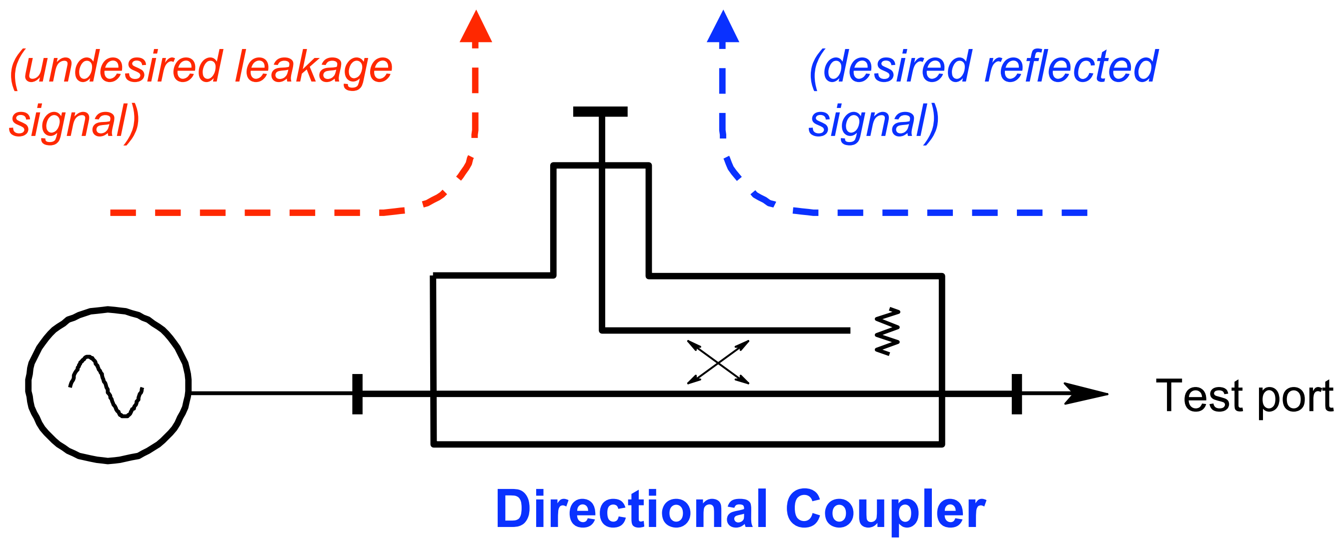
directional coupler

bridge

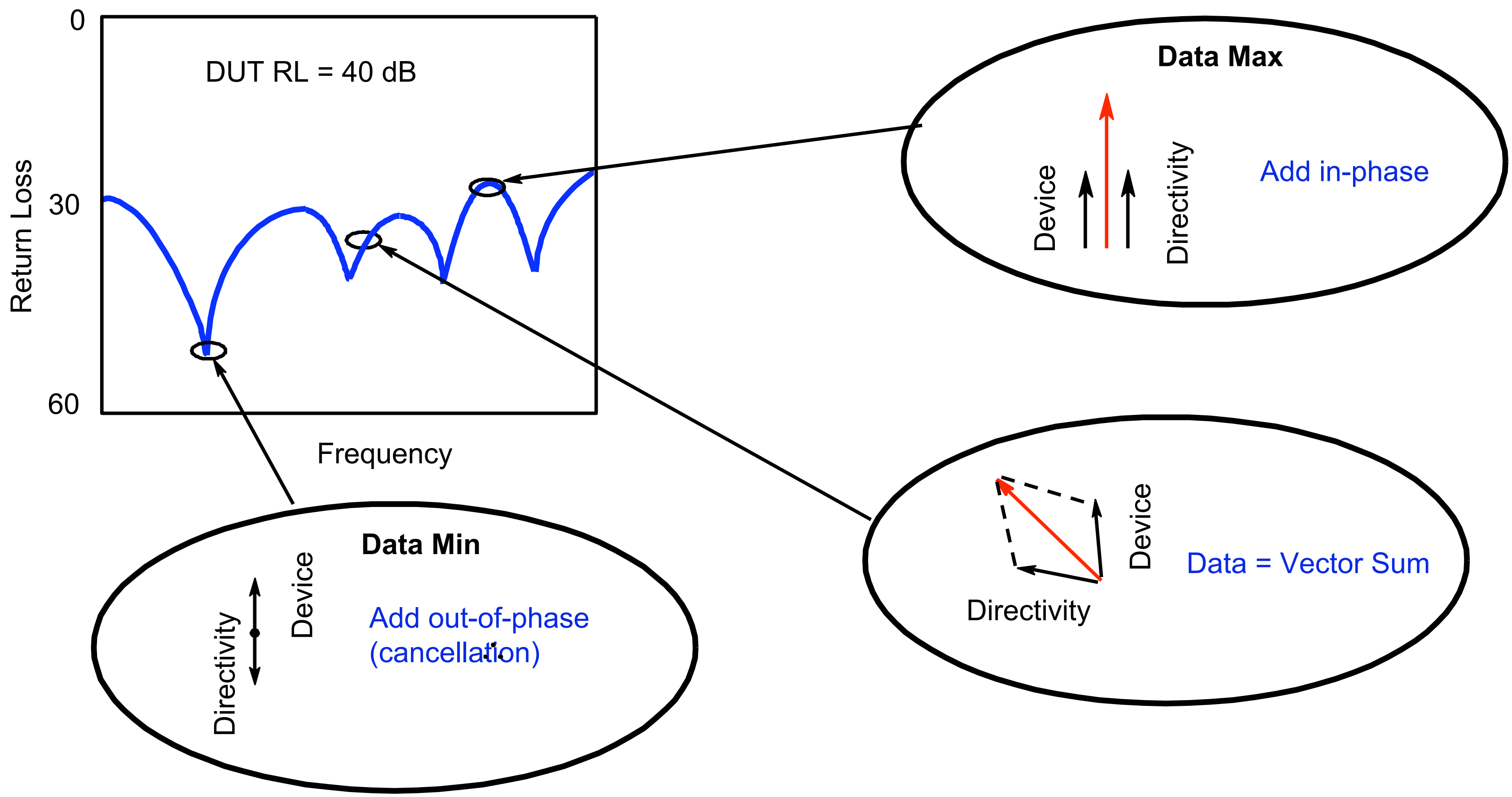


Directivity

Directivity is a measure of how well a coupler can separate signals moving in opposite directions



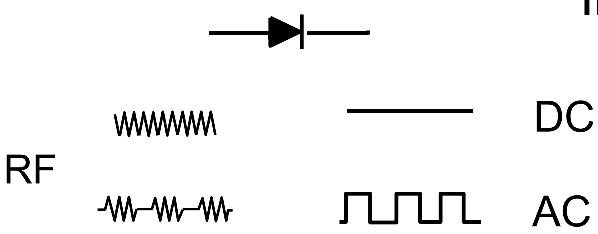
Interaction of Directivity with the DUT (Without Error Correction)

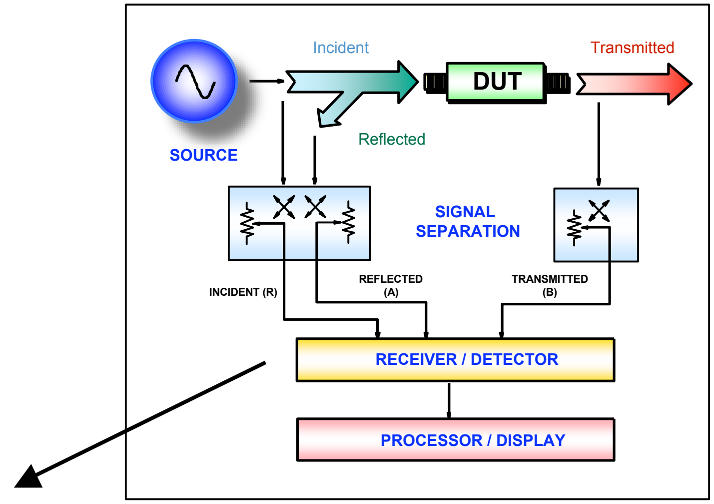


Detector Types

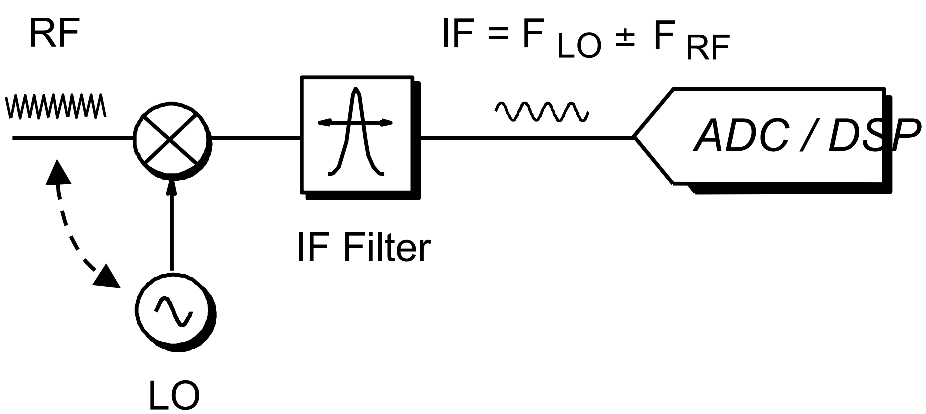
Scalar **broadband**
(no phase
information)

Diode



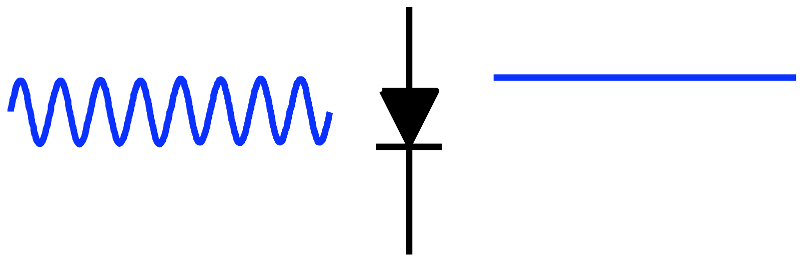


Tuned Receiver

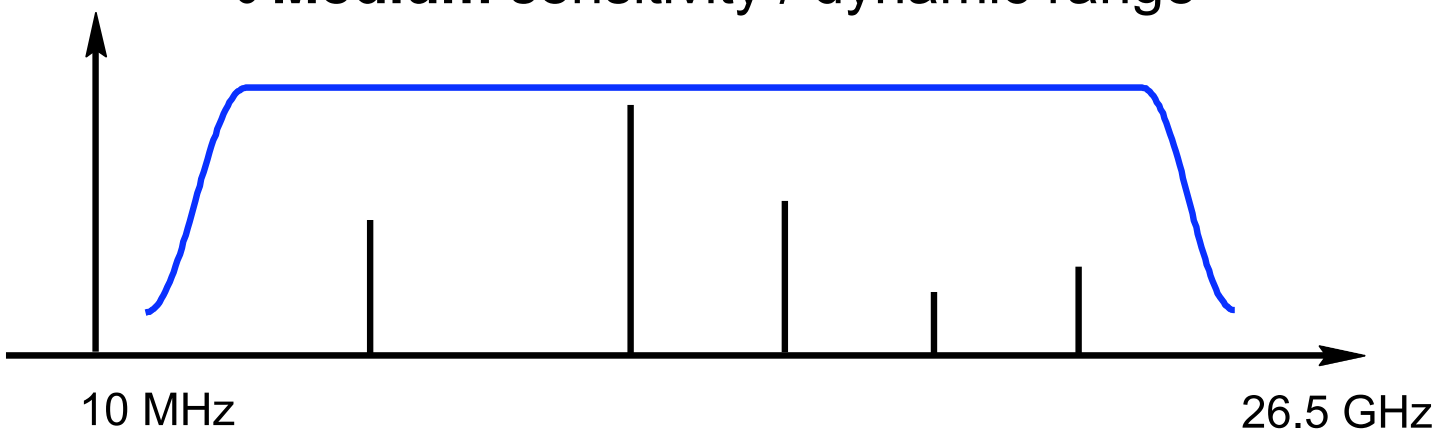


Vector
(magnitude and
phase)

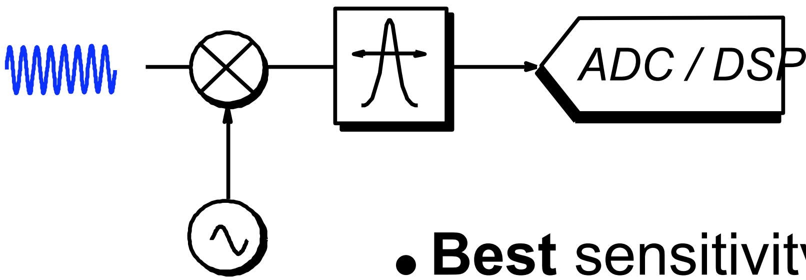
Broadband Diode Detection



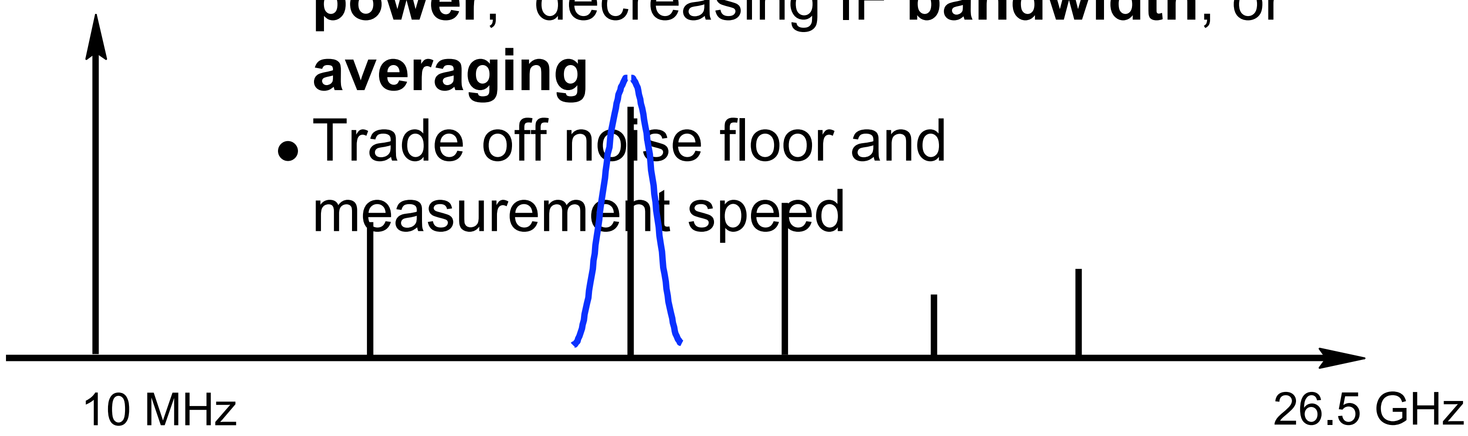
- Easy to make **broadband**
- **Inexpensive** compared to tuned receiver
- Good for measuring frequency-translating devices
- Improve dynamic range by increasing power
- **Medium** sensitivity / dynamic range



Narrowband Detection - Tuned Receiver



- **Best** sensitivity / dynamic range
- Provides harmonic / spurious signal **rejection**
- Improve dynamic range by increasing **power**, decreasing IF **bandwidth**, or **averaging**
- Trade off noise floor and measurement speed



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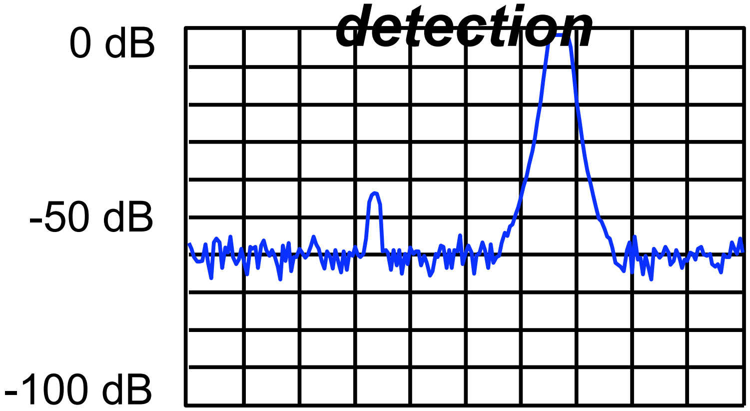
Comparison of Receiver Techniques

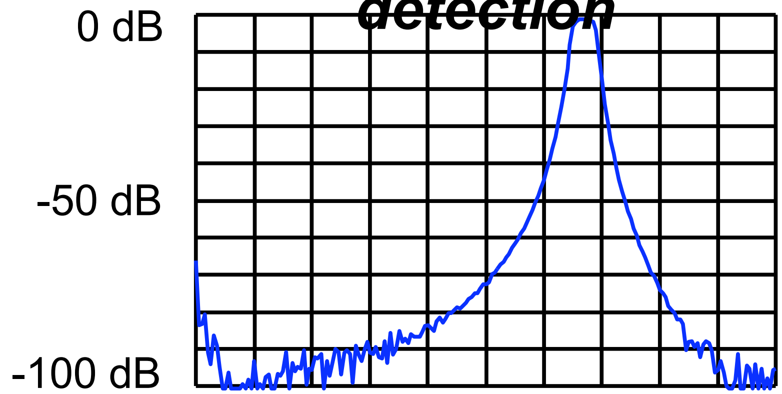
Broadband (diode) detection



-60 dBm Sensitivity

- higher noise floor
- false responses

Narrowband (tuned-receiver) detection

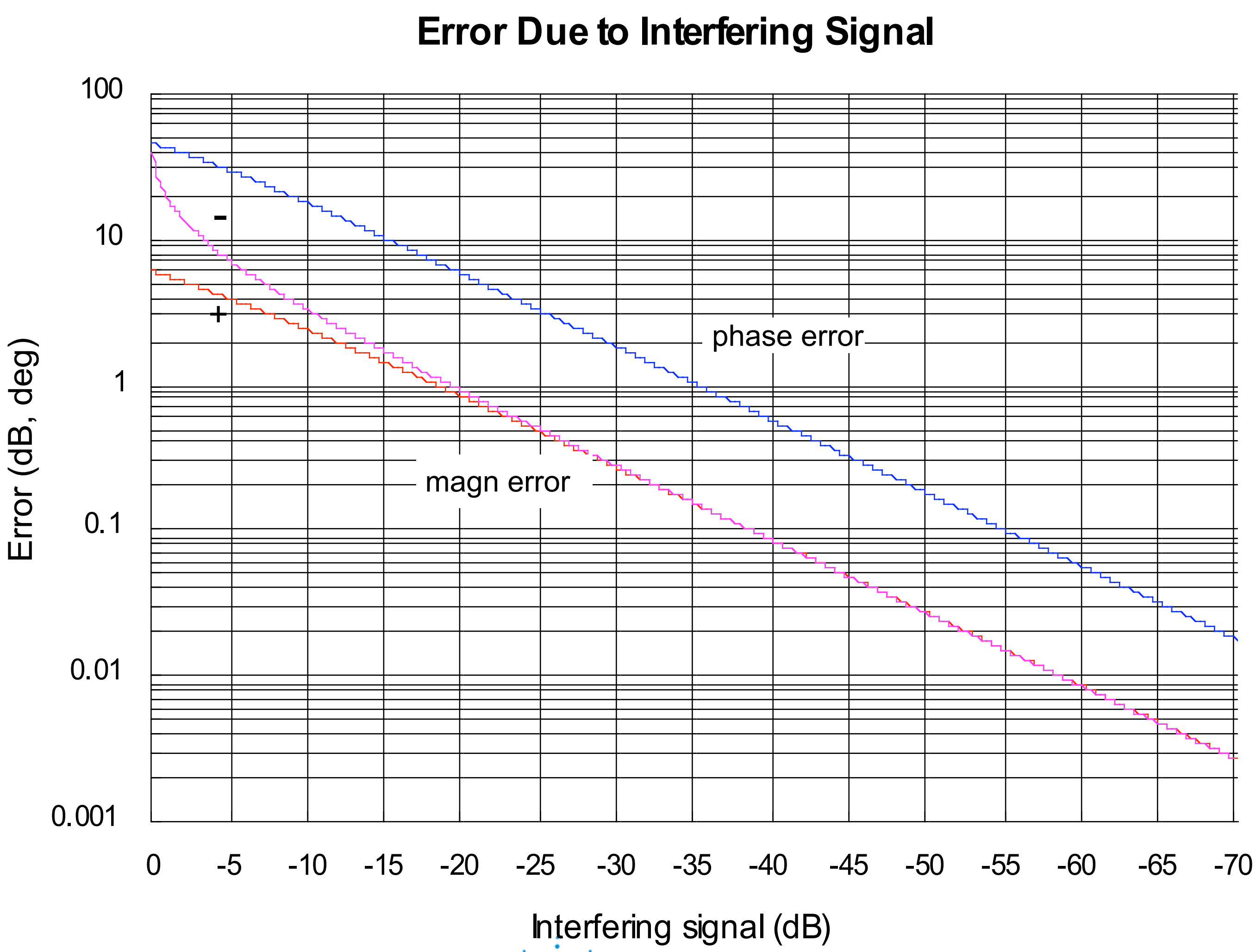


< -100 dBm Sensitivity

- high dynamic range
- harmonic immunity

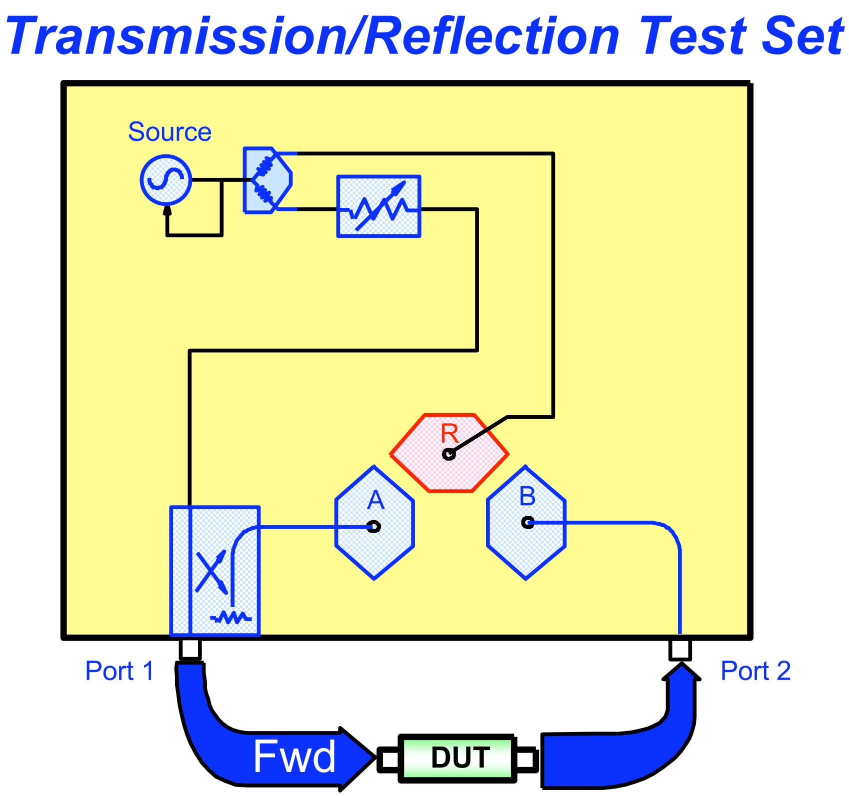
Dynamic range = maximum receiver power - receiver noise floor

Dynamic Range and Accuracy

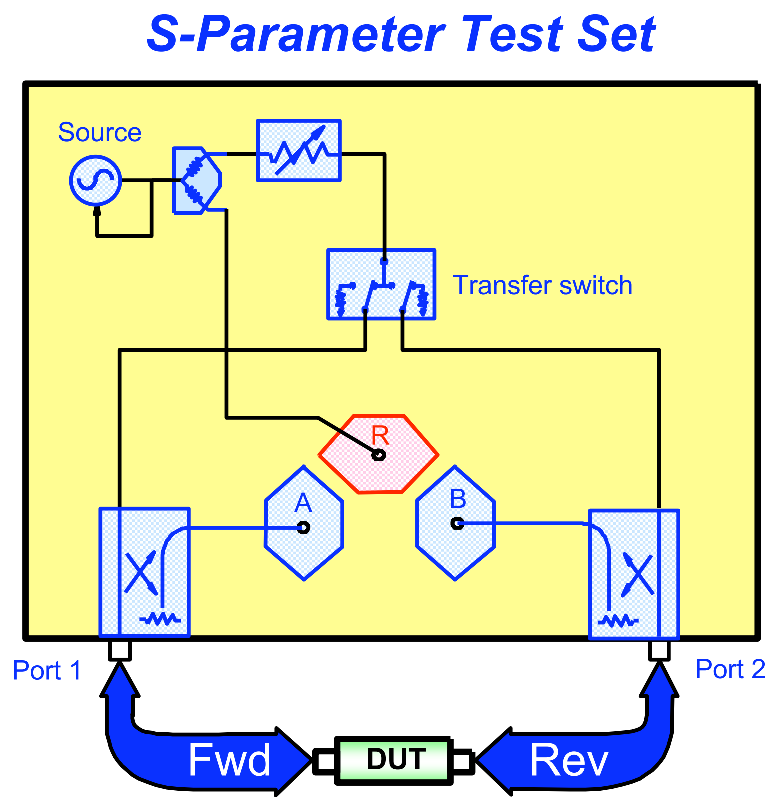


Dynamic range is very important for measurement accuracy!

T/R Versus S-Parameter Test Sets

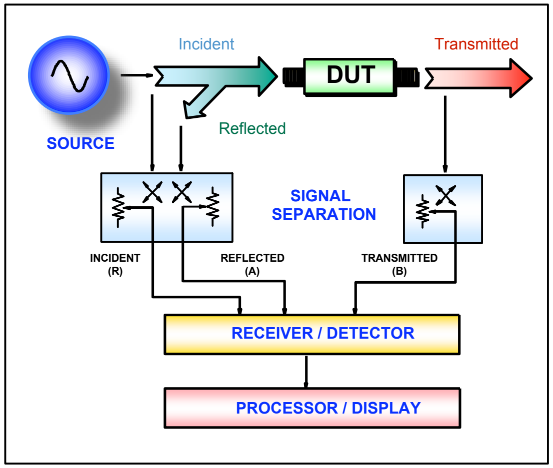


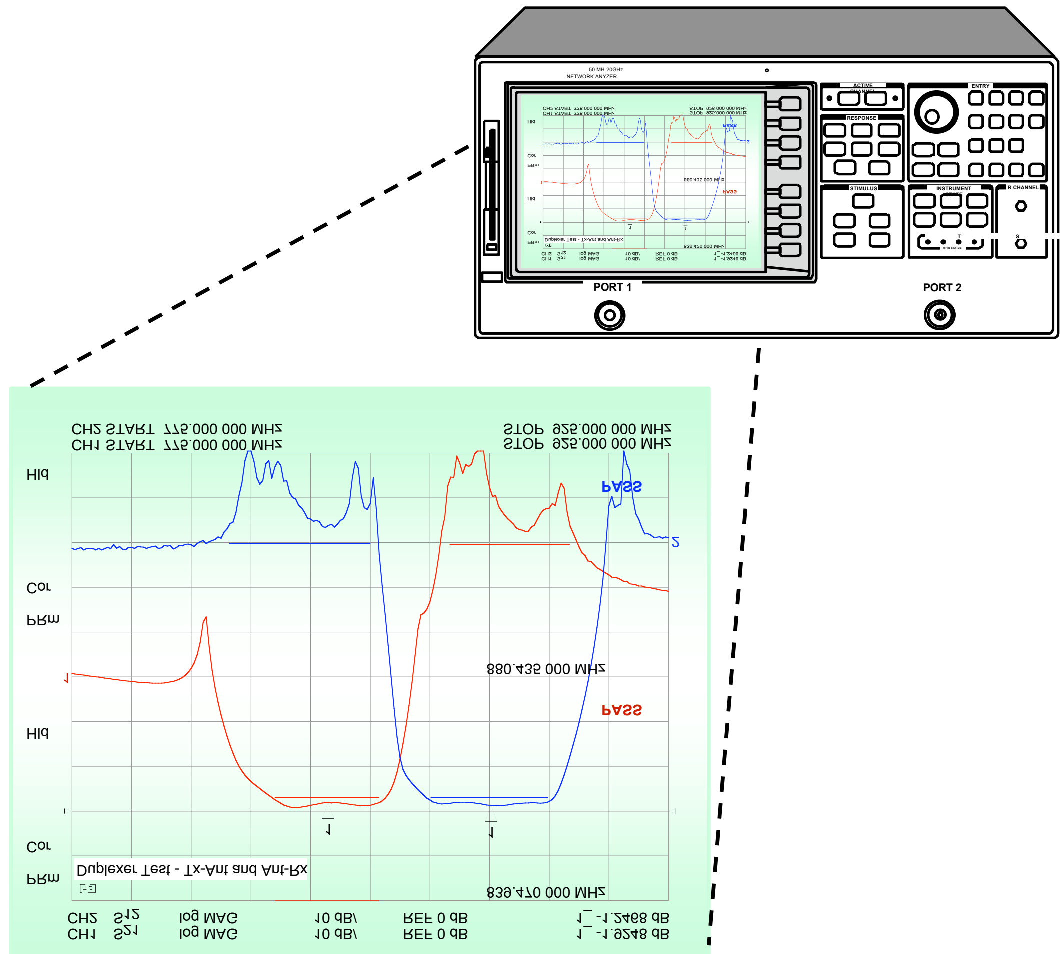
- RF always comes out port 1
- port 2 is always receiver
- **response**, **one-port** cal available



- RF comes out port 1 or port 2
- forward and reverse measurements
- **two-port** calibration possible

Processor / Display





- markers
- limit lines
- pass/fail indicators
- linear/log formats
- grid/polar/Smith charts

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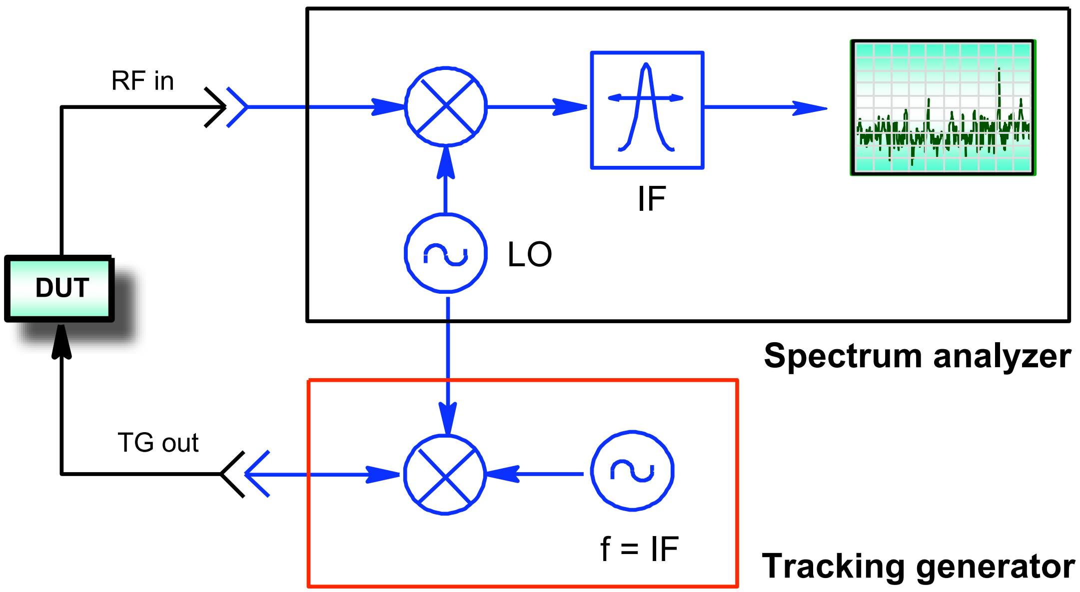
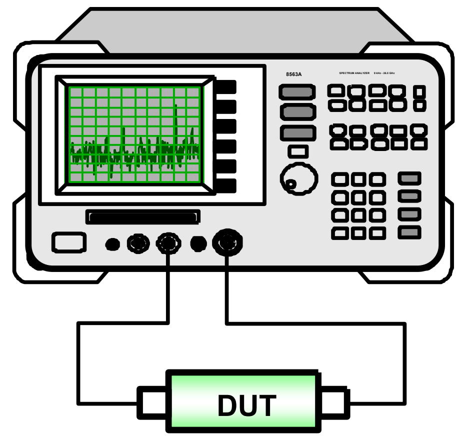
Spectrum Analyzer / Tracking Generator

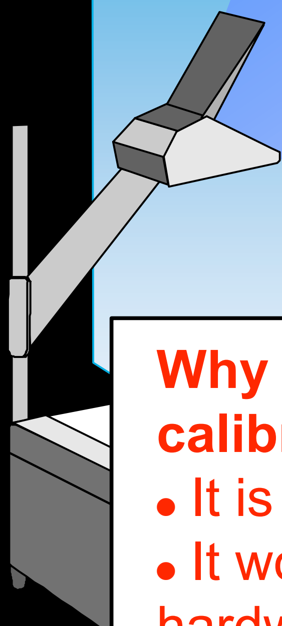




Key differences from network analyzer:

- **one channel** -- no ratioed or phase measurements
- More **expensive** than scalar NA (but better dynamic range)
- Only error correction available is **normalization** (and possibly open-short averaging)
- Poorer **accuracy**
- Small **incremental cost** if SA is required for other measurements

Agenda

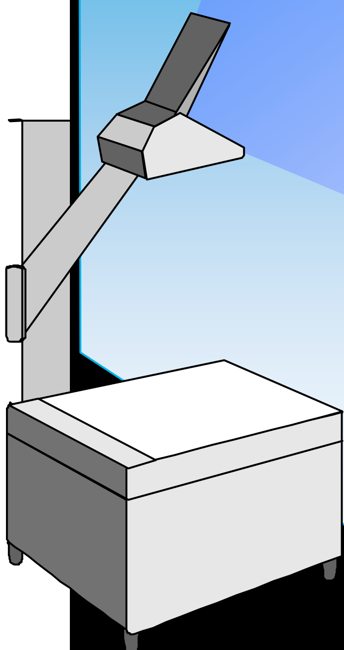


- What measurements do we make?
- Network analyzer hardware
- Error models and calibration
- Example measurements
- Appendix

Why do we even need error-correction and calibration?

- It is impossible to make perfect hardware
- It would be extremely expensive to make hardware good enough to eliminate the need for error correction

Calibration Topics



- What measurements do we make?
- Network analyzer hardware
- Error models and calibration
  - measurement errors
  - what is vector error correction?
  - calibration types
  - accuracy examples
  - calibration considerations
- Example measurements
- Appendix

Measurement Error Modeling

Systematic errors

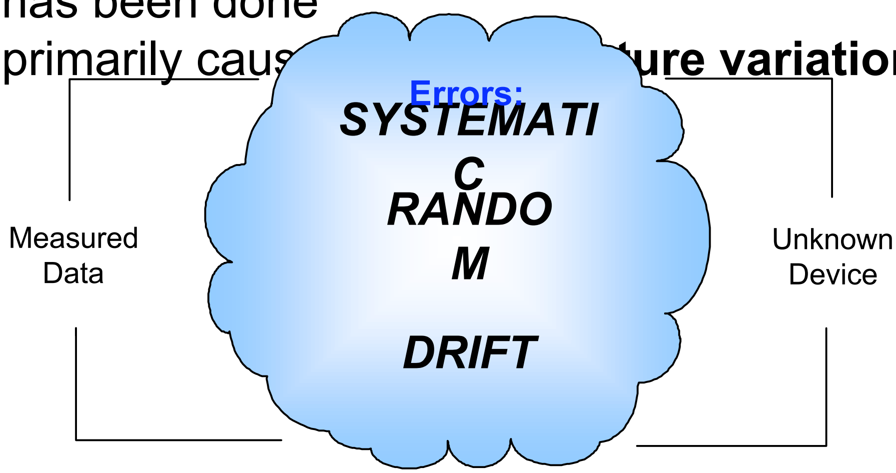
- due to **imperfections** in the analyzer and test setup
- assumed to be **time invariant** (predictable)

Random errors

- **vary** with time in random fashion (unpredictable)
- main contributors: instrument **noise,** switch and connector **repeatability**

Drift errors

- due to system performance changing ***after*** a calibration has been done
- primarily caus ... **ure variation**



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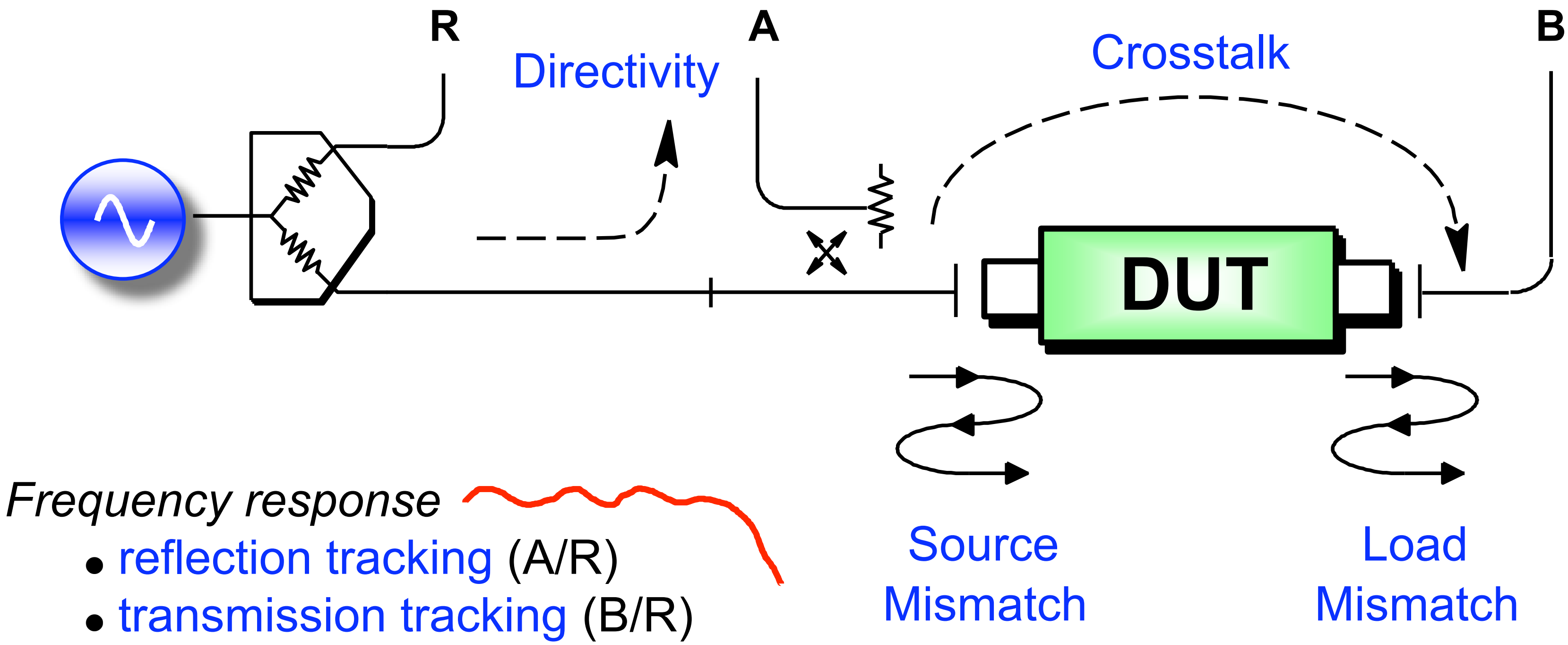
Systematic Measurement Errors

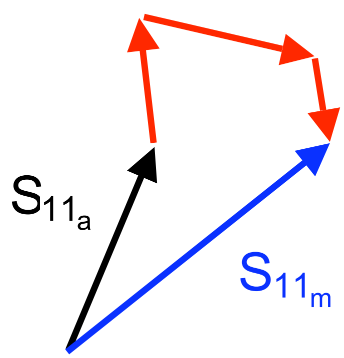


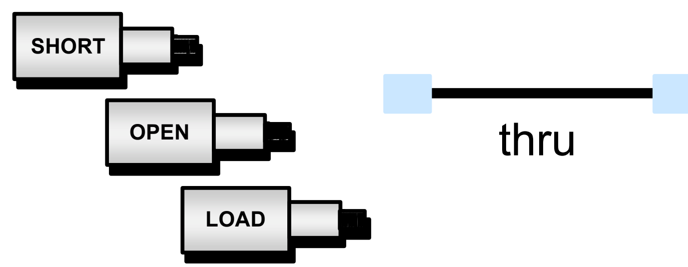
Six forward and six reverse error terms yields 12 error terms for two-port devices

Types of Error Correction

- **response (normalization)**
  - simple to perform
  - only corrects for tracking errors
  - stores reference trace in memory, then does data divided by memory

- **vector**
  - requires more standards
  - requires an analyzer that can measure phase
  - accounts for all major sources of systematic error

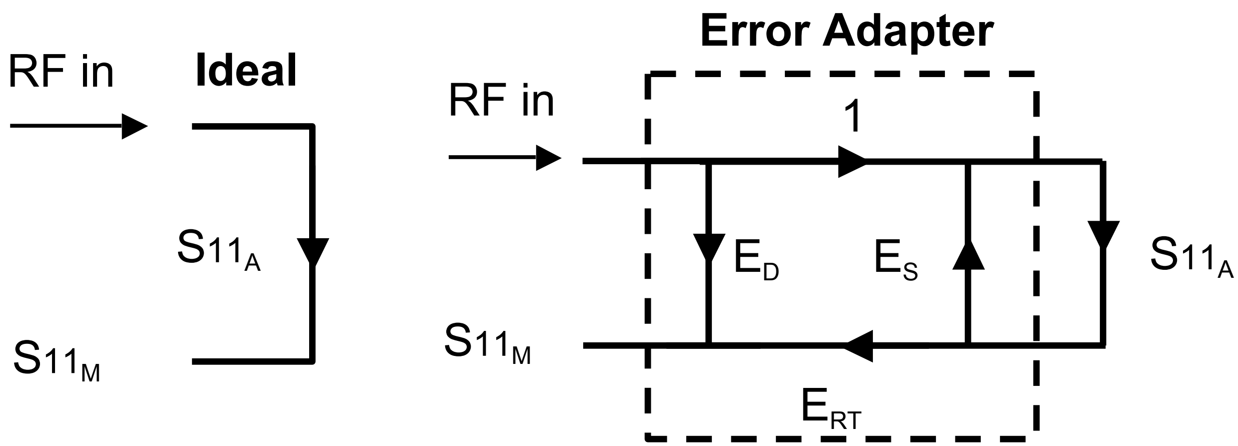




What is Vector-Error Correction?

- Process of characterizing systematic error terms
  - measure **known standards**
  - remove effects from subsequent measurements
- **1-port calibration** *(reflection measurements)*
  - only 3 systematic error terms measured
  - directivity, source match, and reflection tracking
- **Full 2-port calibration** *(reflection and transmission measurements)*
  - 12 systematic error terms measured
  - usually requires 12 measurements on four known standards (SOLT)
- Standards defined in **cal kit definition** file
  - network analyzer contains standard cal kit definitions
  - **CAL KIT DEFINITION MUST MATCH ACTUAL CAL KIT USED!**
  - User-built standards must be characterized and entered into user cal-kit

Reflection: One-Port Model



E_D = Directivity

E_{RT} = Reflection tracking

E_S = Source Match

$S11_M$ = Measured

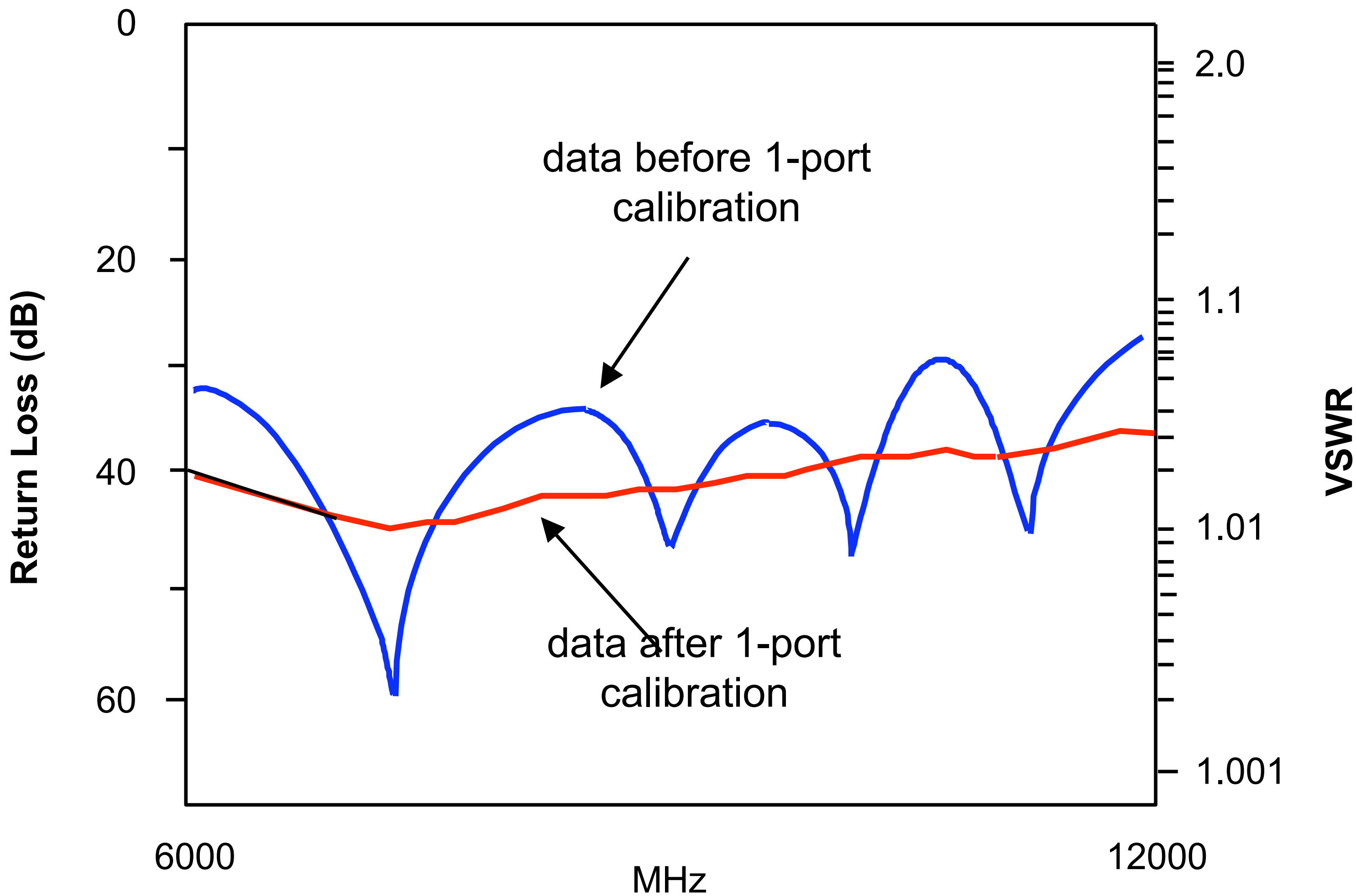
$S11_A$ = Actual

To solve for error terms, we measure 3 standards to generate 3 equations and 3 unknowns

$$S11_M = E_D + E_{RT} \left[\frac{S11_A}{1 - E_S \, S11_A} \right]$$

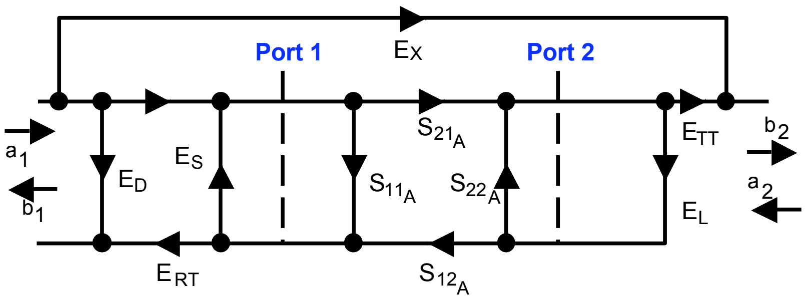
- Assumes good termination at port two if testing two-port devices
- If using port 2 of NA *and* DUT reverse isolation is low (e.g., filter passband):
  - assumption of good termination is not valid
  - two-port error correction yields better results

Before and After One-Port Calibration

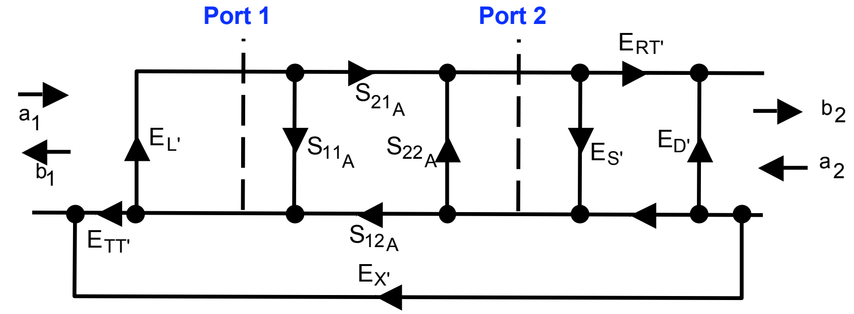


Two-Port Error Correction

Forward model



Reverse model



E_D = fwd directivity
E_S = fwd source match
E_{RT} = fwd reflection tracking
$E_{D'}$ = rev directivity
$E_{S'}$ = rev source match
$E_{RT'}$ = rev reflection tracking

E_L = fwd load match
E_{TT} = fwd transmission tracking
E_X = fwd isolation
$E_{L'}$ = rev load match
$E_{TT'}$ = rev transmission tracking
$E_{X'}$ = rev isolation

- Each actual S-parameter is a function of all four measured S-parameters
- Analyzer must make forward *and* reverse sweep to update any one S-parameter
- Luckily, you don't need to know these equations to ***use*** network analyzers!!!

$$S_{11a} = \frac{\left(\frac{S_{11m}-E_D}{E_{RT}}\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}E_{S'}\right)-E_L\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}{\left(1+\frac{S_{11m}-E_D}{E_{RT}}E_S\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}E_{S'}\right)-E_{L'}E_L\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}$$

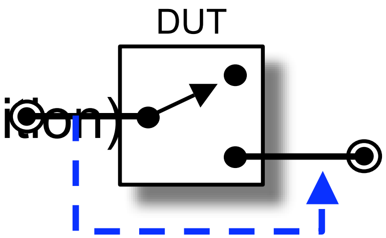
$$S_{21a} = \frac{\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}(E_{S'}-E_L)\right)}{\left(1+\frac{S_{11m}-E_D}{E_{RT}}E_S\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}E_{S'}\right)-E_{L'}E_L\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}$$

$$S_{12a} = \frac{\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)\left(1+\frac{S_{11m}-E_D}{E_{RT}}(E_S-E_{L'})\right)}{\left(1+\frac{S_{11m}-E_D}{E_{RT}}E_S\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}E_{S'}\right)-E_{L'}E_L\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}$$

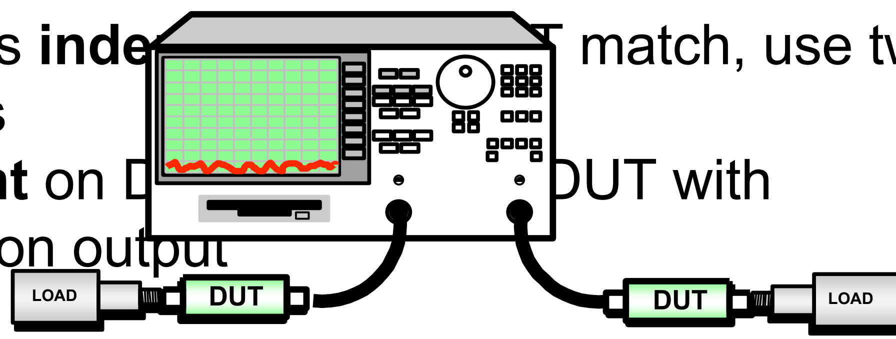
$$S_{22a} = \frac{\left(\frac{S_{22m}-E_{D'}}{E_{RT'}}\right)\left(1+\frac{S_{11m}-E_D}{E_{RT}}E_S\right)-E_{L'}\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}{\left(1+\frac{S_{11m}-E_D}{E_{RT}}E_S\right)\left(1+\frac{S_{22m}-E_{D'}}{E_{RT'}}E_{S'}\right)-E_{L'}E_L\left(\frac{S_{21m}-E_X}{E_{TT}}\right)\left(\frac{S_{12m}-E_{X'}}{E_{TT'}}\right)}$$

Crosstalk: Signal Leakage Between Test Ports During Transmission

- Can be a problem with:
  - high-isolation devices (e.g., switch in open position)
  - high-dynamic range devices (some filter stopbands)

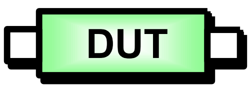


- Isolation calibration
  - adds noise to error model (measuring near noise floor of system)
  - only perform if really needed (use averaging if necessary)
  - if crosstalk is **inde**… T match, use two terminations
  - if **dependent** on D… DUT with termination on output



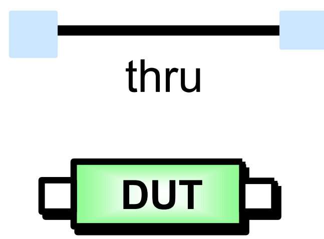
Errors and Calibration Standards

UNCORRECTED



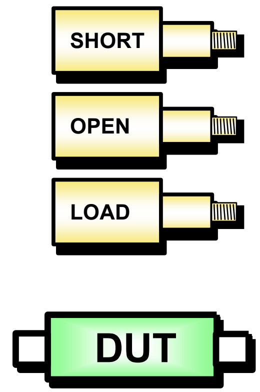
- Convenient
- Generally not accurate
- No errors removed

RESPONSE



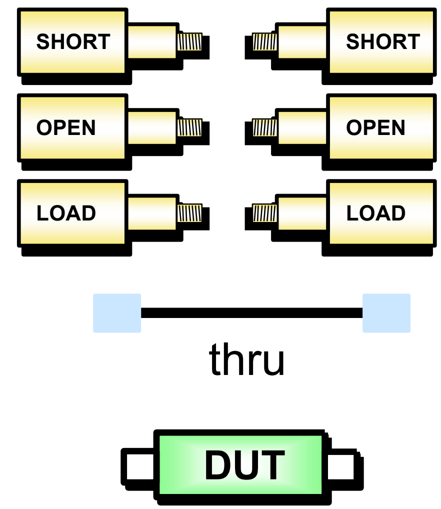
- Easy to perform
- Use when highest accuracy is not required
- Removes frequency response error

1-PORT



- For reflection measurements
- Need good termination for high accuracy with two-port devices
- Removes these errors:
  - Directivity
  - Source match
  - Reflection tracking

FULL 2-PORT

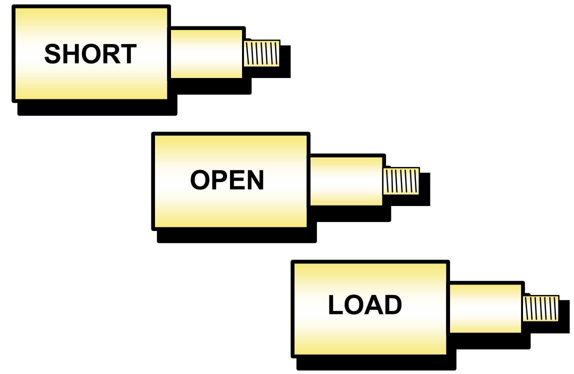


- Highest accuracy
- Removes these errors:
  - Directivity
  - Source, load match
  - Reflection tracking
  - Transmission tracking
  - Crosstalk

ENHANCED-RESPONSE

- Combines response and 1-port
- Corrects source match for transmission measurements

Calibration Summary



Reflection

Test Set (cal type)

	T/R (one-port)	S-parameter (two-port)
• Reflection tracking	✓	✓
• Directivity	✓	✓
• Source match	✓	
• Load match	✗	

Transmission

Test Set (cal type)

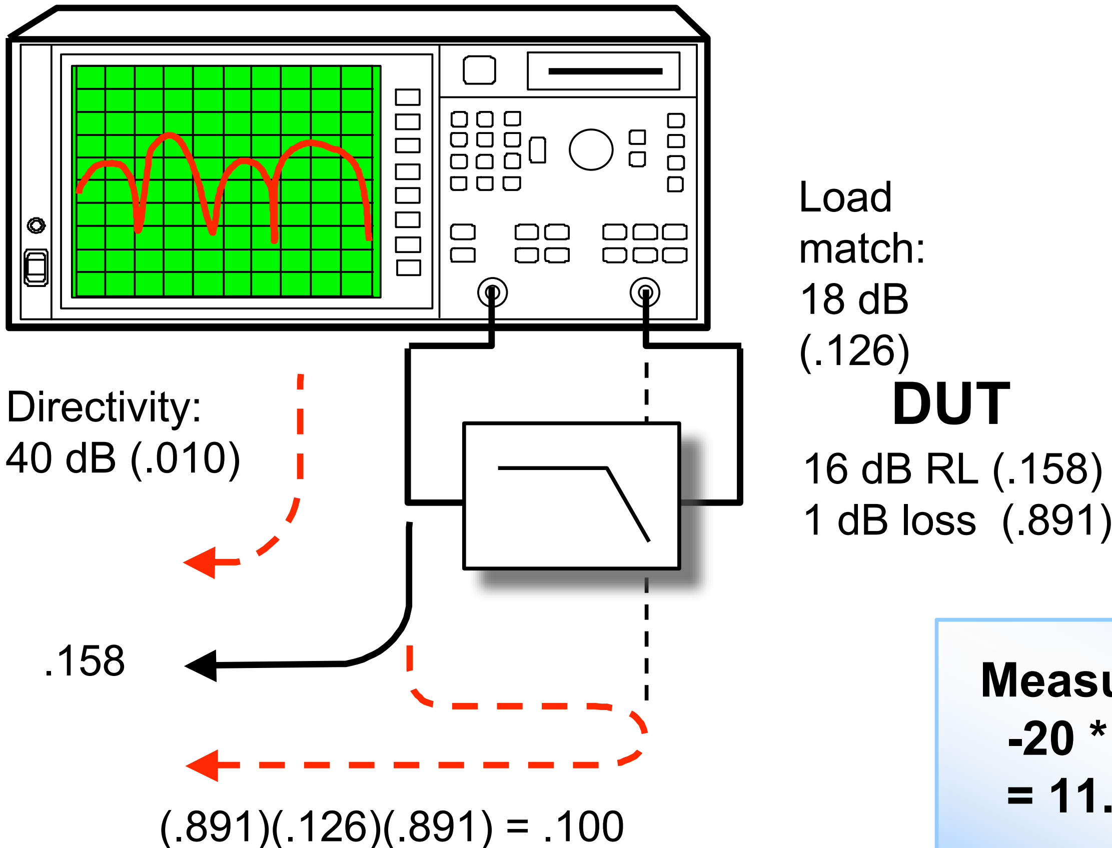
	T/R (response, isolation)	S-parameter (two-port)
• Transmission Tracking	✓	✓
• Crosstalk	✓	✓
• Source match (✓*)	✗	✓
• Load match	✗	✓

✓ ***error can be corrected***

✗ ***error cannot be corrected***

✓* *enhanced response cal* corrects for source match during transmission measurements

Reflection Example Using a One-Port Cal



Remember: convert all dB values to linear for uncertainty calculations!

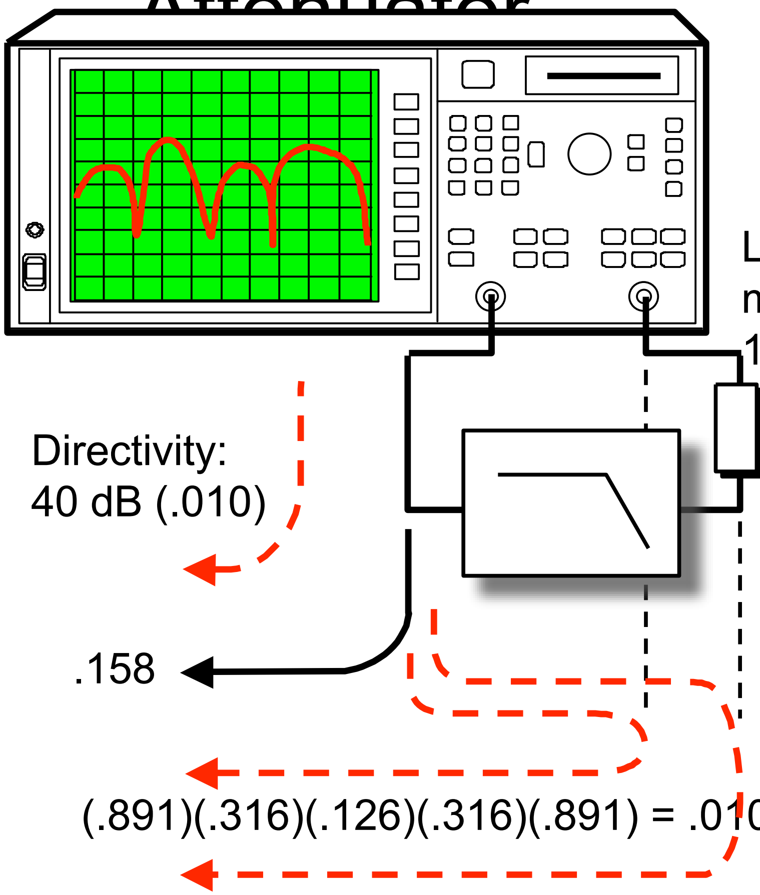
ρ or $\text{loss}_{(\text{linear})} = 10^{\left(\frac{-\text{dB}}{20}\right)}$

Measurement uncertainty:

-20 * log (.158 + .100 + .010)
= 11.4 dB (-4.6dB)

-20 * log (.158 - .100 - .010)
= 26.4 dB (+10.4 dB)

Using a One-Port Cal + Attenuator



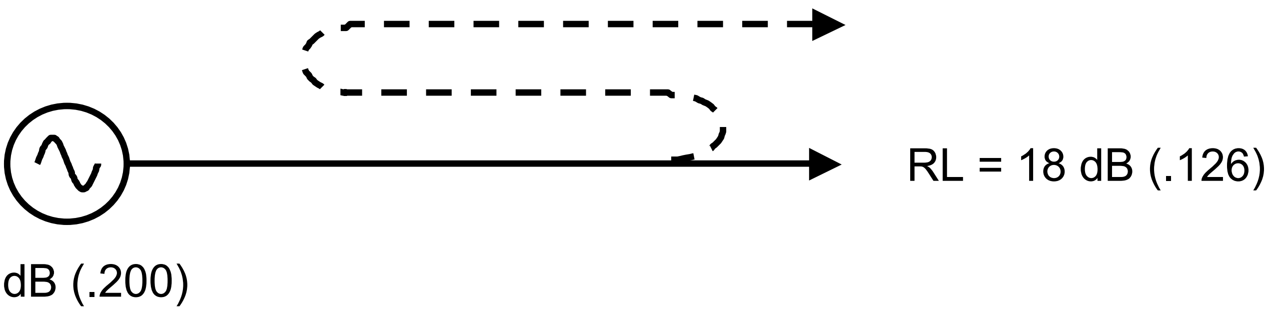
Worst-case error = .010 + .010 + .019 = .039

Measurement uncertainty:
-20 * log (.158 + .039)
= 14.1 dB (-1.9 dB)

-20 * log (.158 - .039)
= 18.5 dB (+2.5 dB)

Low-loss bi-directional devices generally require two-port calibration for low measurement uncertainty

Transmission Example Using Response Cal



Thru calibration (normalization) builds error into measurement due to source and load match interaction

Calibration Uncertainty

$$= (1 \pm \rho_S \, \rho_L)$$

$$= (1 \pm (.200)(.126)$$

$$= \pm 0.22 \text{ dB}$$

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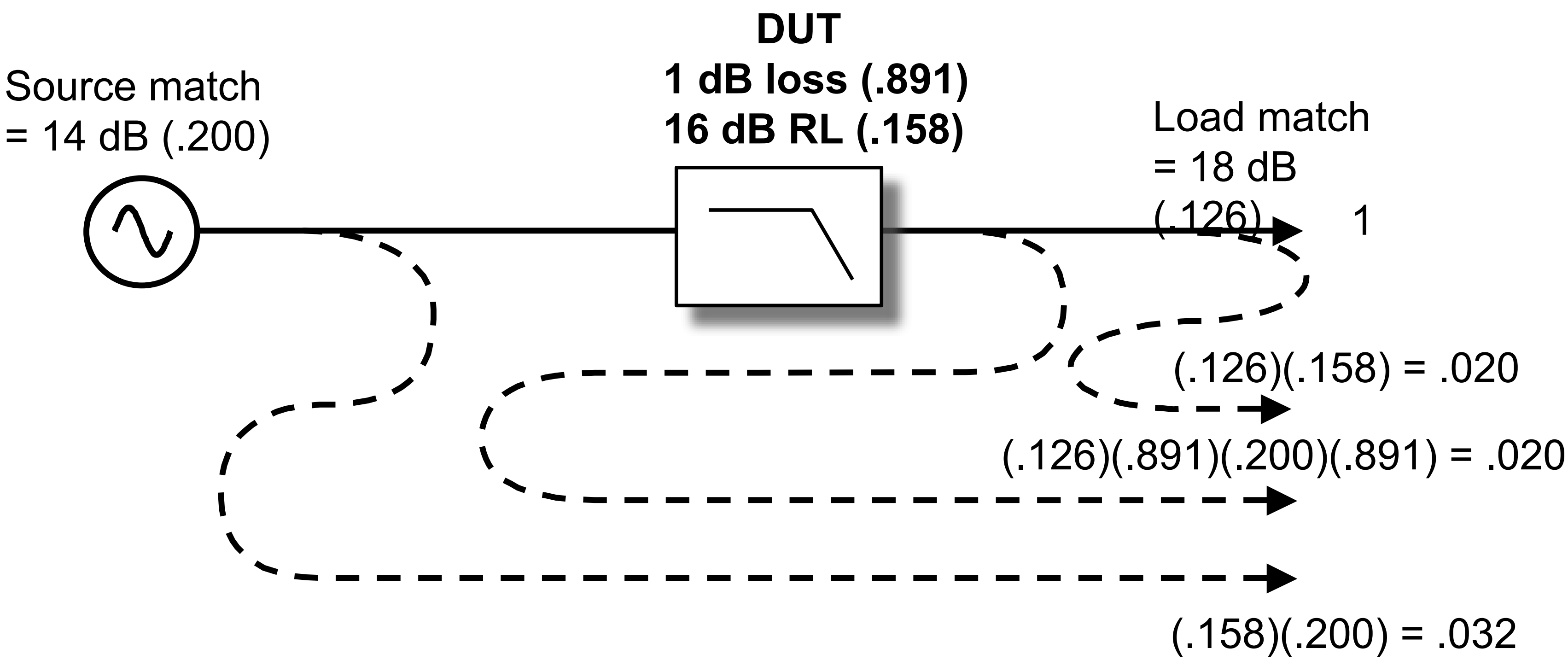
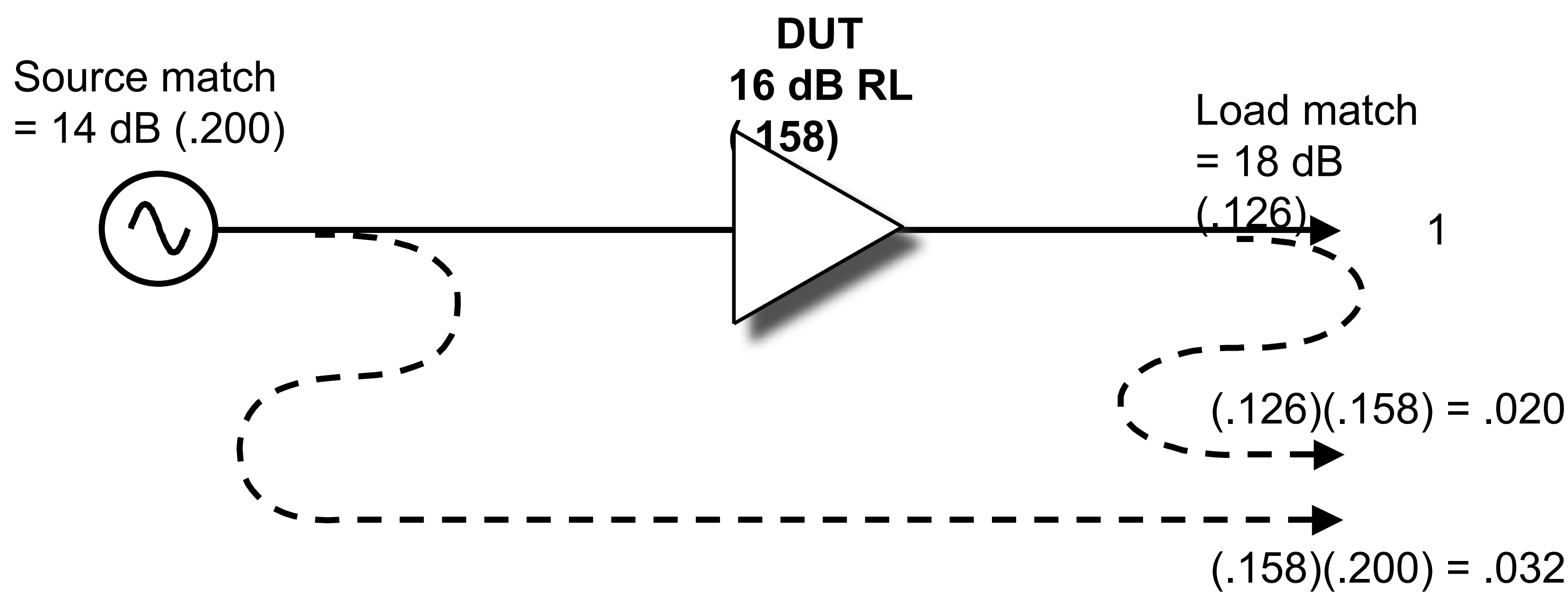
Filter Measurement with Response Cal



Total measurement uncertainty:
+0.60 + 0.22 = + 0.82 dB
-0.65 - 0.22 = - 0.87 dB

Measurement uncertainty
= 1 ± (.020+.020+.032)
= 1 ± .072
= + 0.60 dB
- 0.65 dB

Measuring Amplifiers with a Response Cal



Total measurement uncertainty:

+0.44 + 0.22 = + 0.66 dB

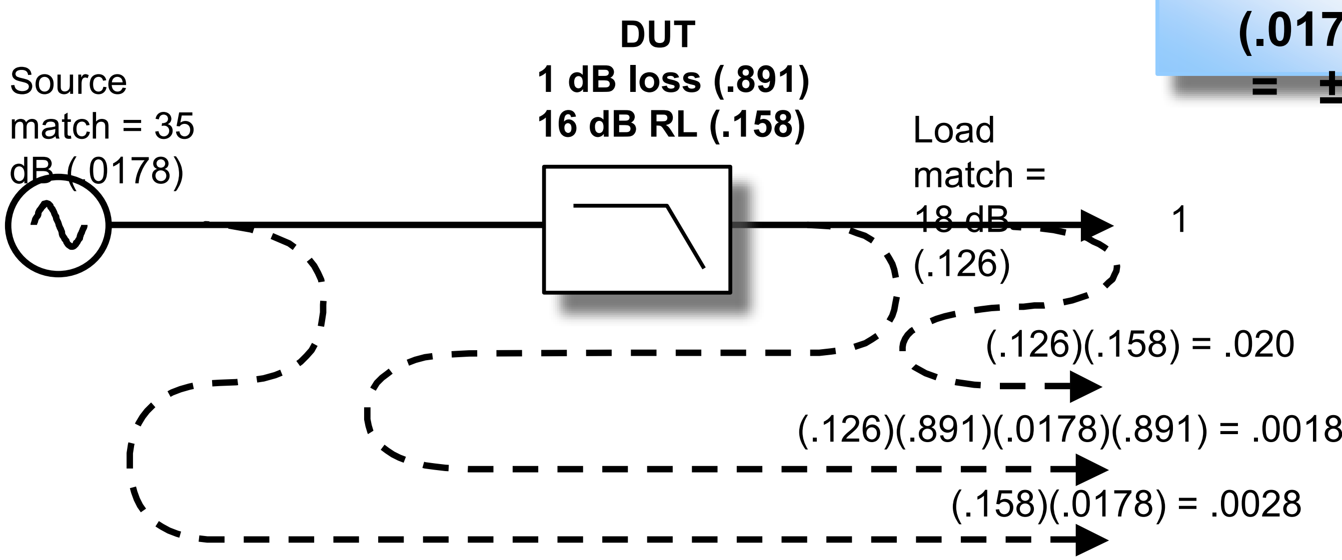
-0.46 - 0.22 = - 0.68 dB

Measurement uncertainty
= 1 ± (.020+.032)
= 1 ± .052
= + 0.44 dB
- 0.46 dB

Filter Measurements using the ***Enhanced Response*** Calibration

Effective source match = 35 dB!

Calibration Uncertainty
$=(1 \pm \rho_S \, \rho_L)$
$= (1 \pm (.0178)(.126)$
$= \pm .02$ dB



Measurement uncertainty
= 1 ± (.020+.0018+.0028)
= 1 ± .0246
= + 0.211 dB
- 0.216 dB

Total measurement uncertainty:
0.22 + .02 = ± 0.24 dB

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Using the ***Enhanced Response*** Calibration Plus an Attenuator

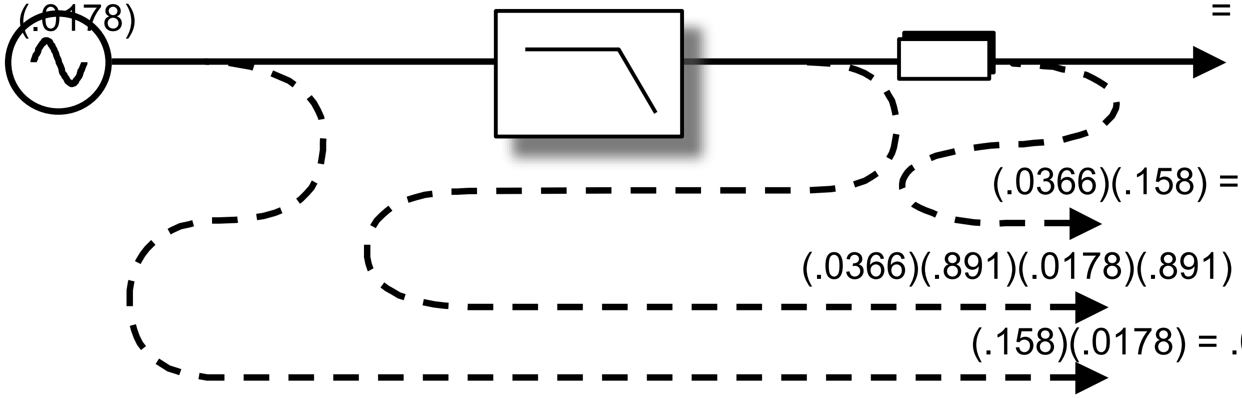
10 dB attenuator (.316)
SWR = 1.05 (.024 linear or 32.4 dB)
Analyzer load match =18 dB (.126)

Calibration Uncertainty
= $(1 \pm \rho_S \rho_L)$
= (1 ± (.0178)(.0366)
= ± .01 dB

Source match = 35 dB (.0178)

DUT
1 dB loss (.891)
16 dB RL (.158)

Effective load match = (.316)(.316)(.126) + .024
= .0366 (28.7dB)

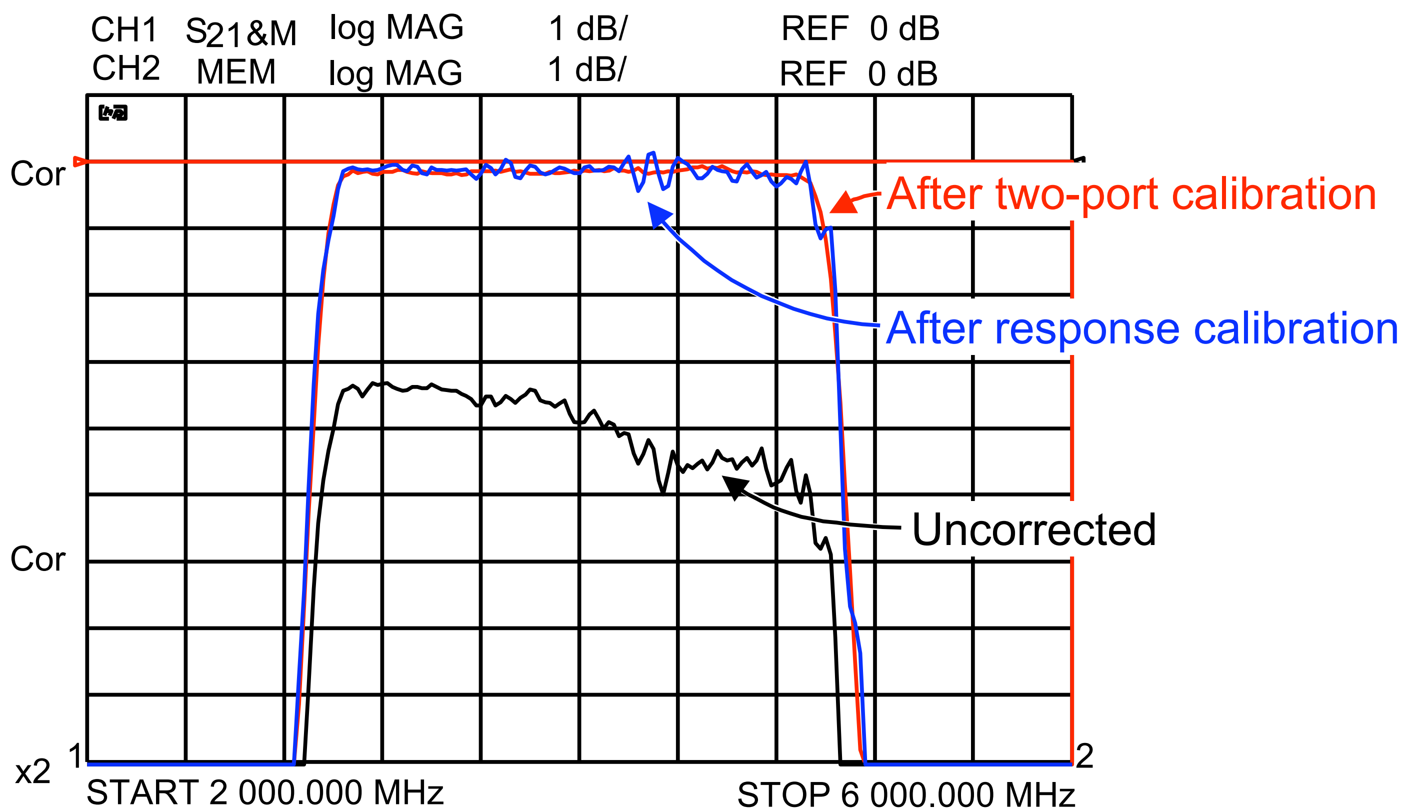


Measurement uncertainty
= 1 ± (.006+.0005+.0028)
= 1 ± .0093
= ± 0.08 dB

Total measurement uncertainty:
0.01 + .08 = ± 0.09 dB

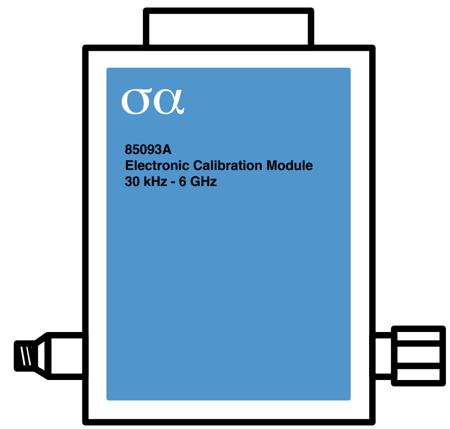
Response versus Two-Port Calibration

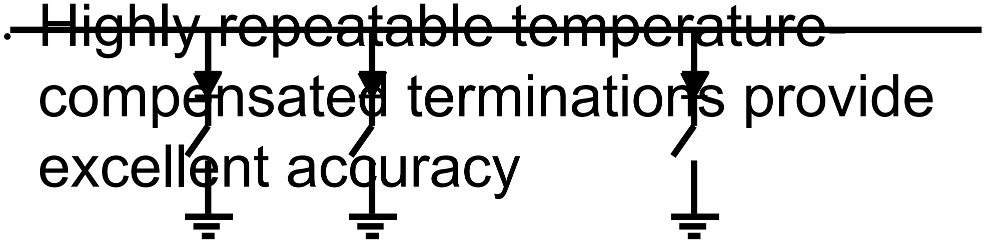
Measuring filter insertion loss



ECal: Electronic Calibration (85060/90 series)

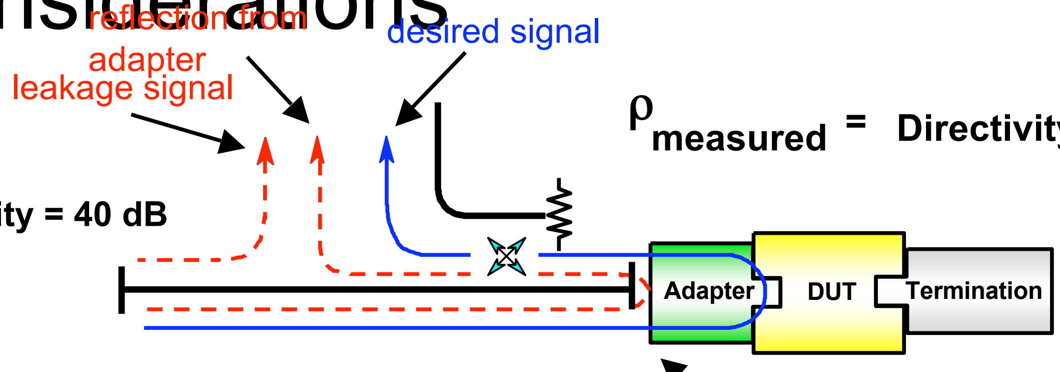
- Variety of modules cover 30 kHz to 26.5 GHz
- Six connector types available (50 Ω and 75 Ω)
- Single-connection
  - reduces calibration time
  - makes calibrations easy to perform
  - minimizes wear on cables and standards
  - eliminates operator errors
- Highly repeatable temperature compensated terminations provide excellent accuracy





Microwave modules use a transmission line shunted by PIN-diode switches in various combinations

Adapter Considerations



$\rho_{measured}$ = Directivity + $\rho_{adapter}$ + ρ_{DUT}

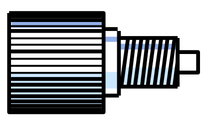
Coupler directivity = 40 dB

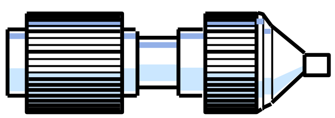
DUT has SMA (f) connectors

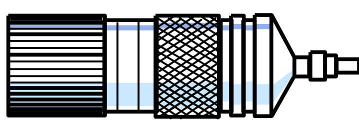
APC-7 calibration done here

Worst-case
System Directivity

Adapting from APC-7 to SMA (m)

28 dB  APC-7 to SMA (m)
SWR:1.06

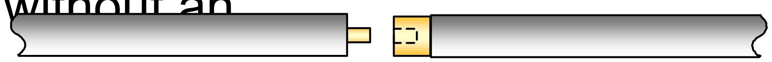
17 dB  APC-7 to N (f) + N (m) to SMA (m)
SWR:1.05 SWR:1.25

14 dB  APC-7 to N (m) + N (f) to SMA (f) + SMA (m) to (m)
SWR:1.05 SWR:1.25 SWR:1.15

Calibrating Non-Insertable Devices

When doing a through cal, normally test ports mate directly

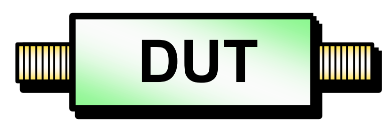
- cables can be connected directly without an adapter



- result is a zero-length through

What is an insertable device?

- has same type of connector, but different sex on each port
- has same type of sexless connector on each port (e.g. APC-7)

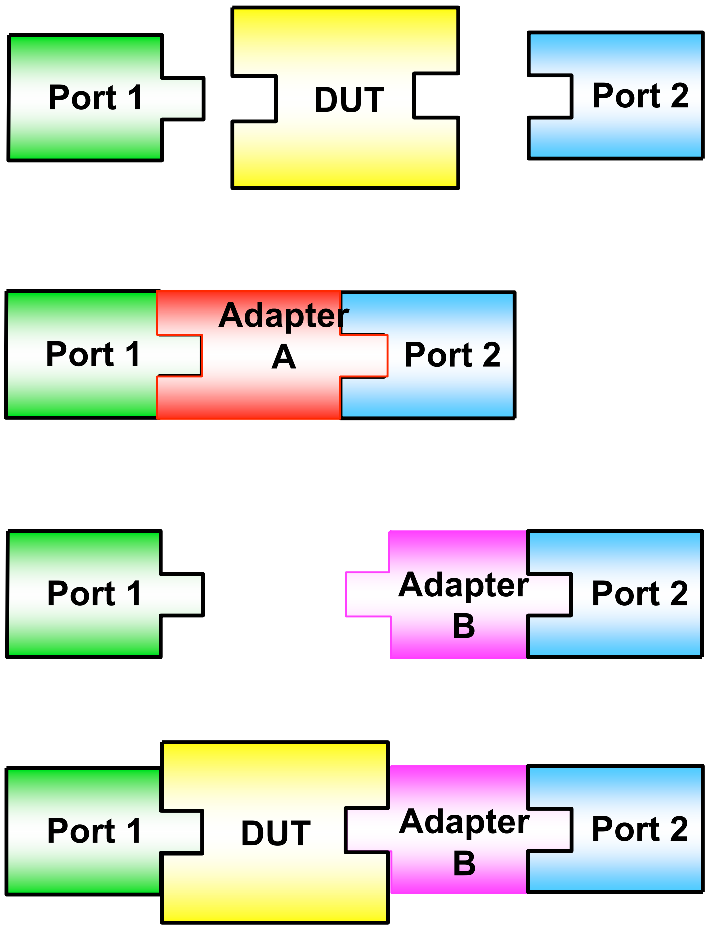


What is a non-insertable device?

- one that cannot be inserted in place of a zero-length through
- has same connectors on each port (type and sex)
- has different type of connector on each port (e.g., waveguide on one port, coaxial on the other)

What calibration choices do I have for non-

Swap Equal Adapters Method

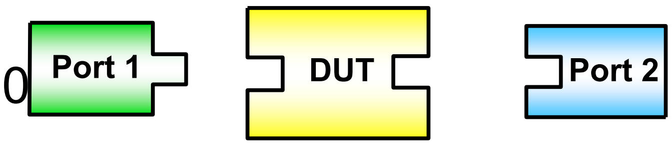


Accuracy depends on how well the adapters are matched - loss, electrical length, match and impedance should all be equal

1. Transmission cal using adapter A.
2. Reflection cal using adapter B.
3. Measure DUT using adapter B.

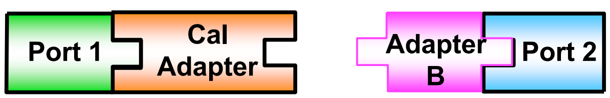
Adapter Removal Calibration

- Calibration is very accurate and traceable
- In firmware of 8753, 8720 and 8510 series
- Also accomplished with ECal modules (85060
- Uses adapter with same connectors as DUT
- Must specify electrical length of adapter to within 1/4 wavelength of highest frequency (to avoid phase ambiguity)



Cal Set 1

1. Perform 2-port cal with adapter on port 2. Save in cal set 1.

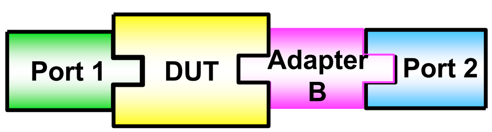


Cal Set 2

2. Perform 2-port cal with adapter on port 1. Save in cal set 2.

[CAL] [MORE] [MODIFY CAL SET]
[ADAPTER REMOVAL]

3. Use ADAPTER REMOVAL to generate new cal set.



4. Measure DUT without cal adapter.

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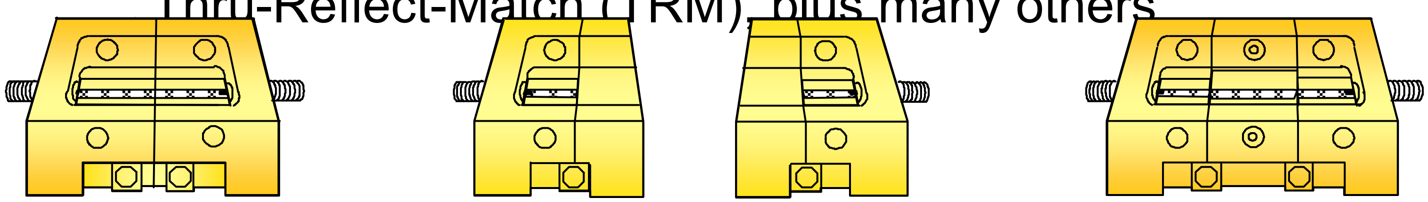
Thru-Reflect-Line (TRL) Calibration

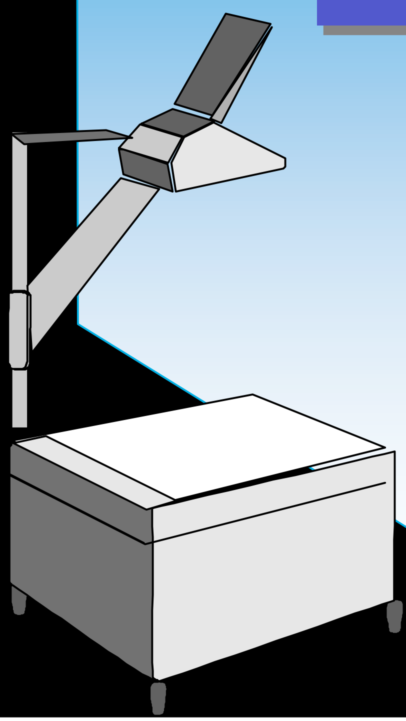
We know about Short-Open-Load-Thru (SOLT) calibration...
What is TRL?

- A two-port calibration technique
- Good for noncoaxial environments (waveguide, fixtures, wafer probing)
- Uses the same 12-term error model as the more common SOLT cal
- Uses practical calibration standards th are easily fabricated and chara
- Two variations: TRL (requires 4 receiv and TRL* (only three receivers needed)
- Other variations: Line-Reflect-Match (LRM), Thru-Reflect-Match (TRM), plus many others

*TRL was developed for **non-coaxial microwave** measurements*

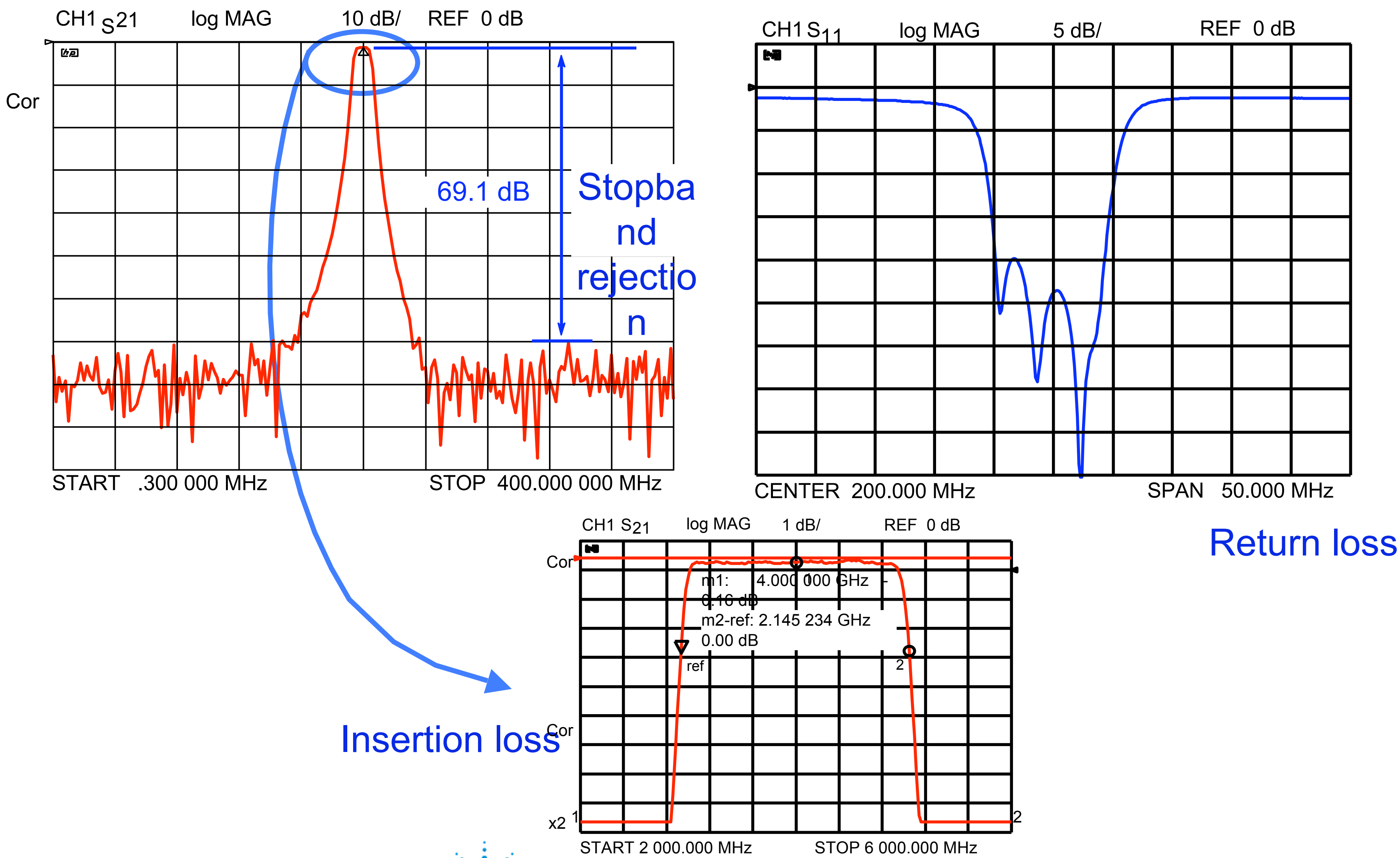


Agenda



- What measurements do we make?
- Network analyzer hardware
- Error models and calibration
- Example measurements
- Appendix

Frequency Sweep - Filter Test



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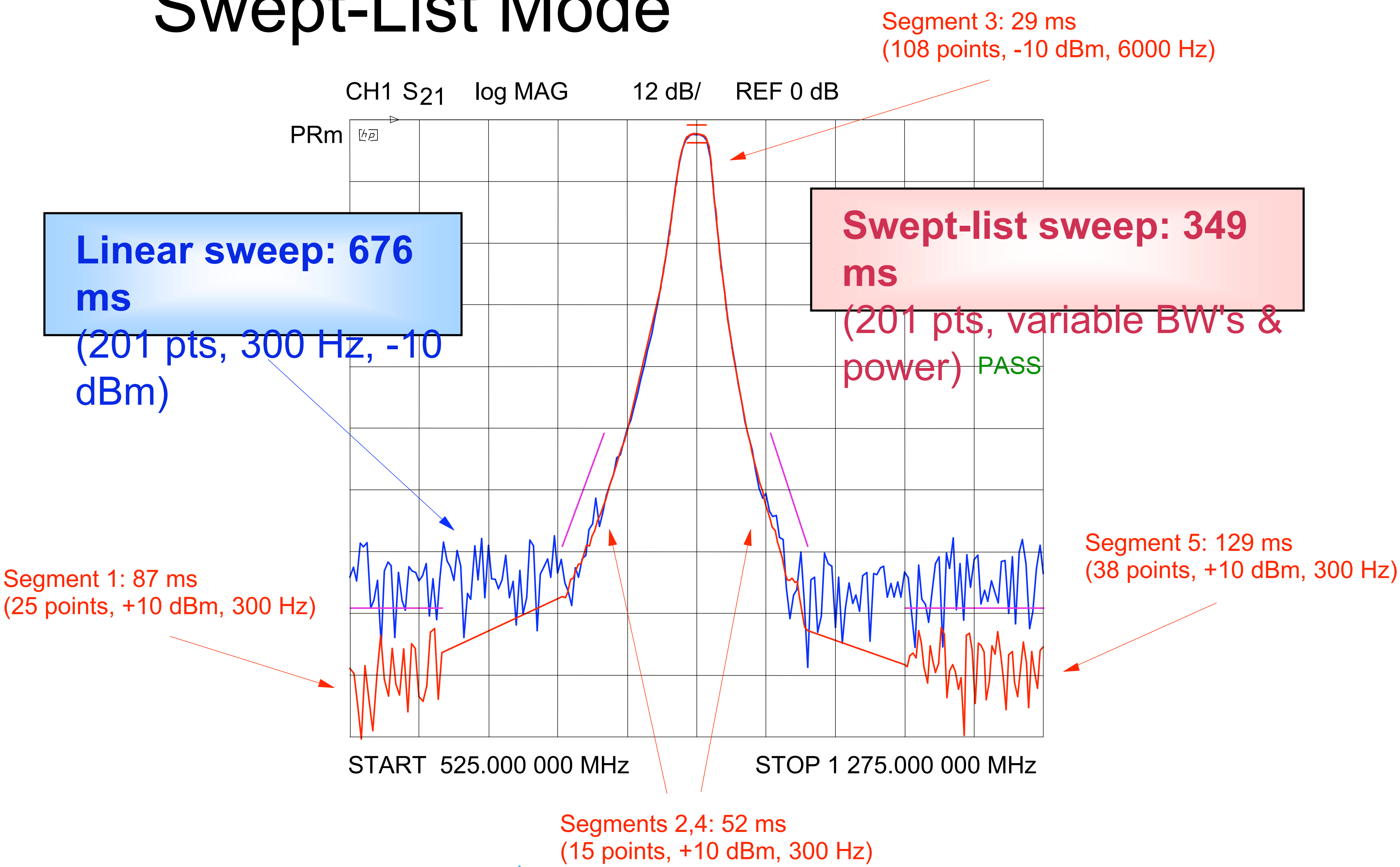
Optimize Filter Measurements with Swept-List Mode



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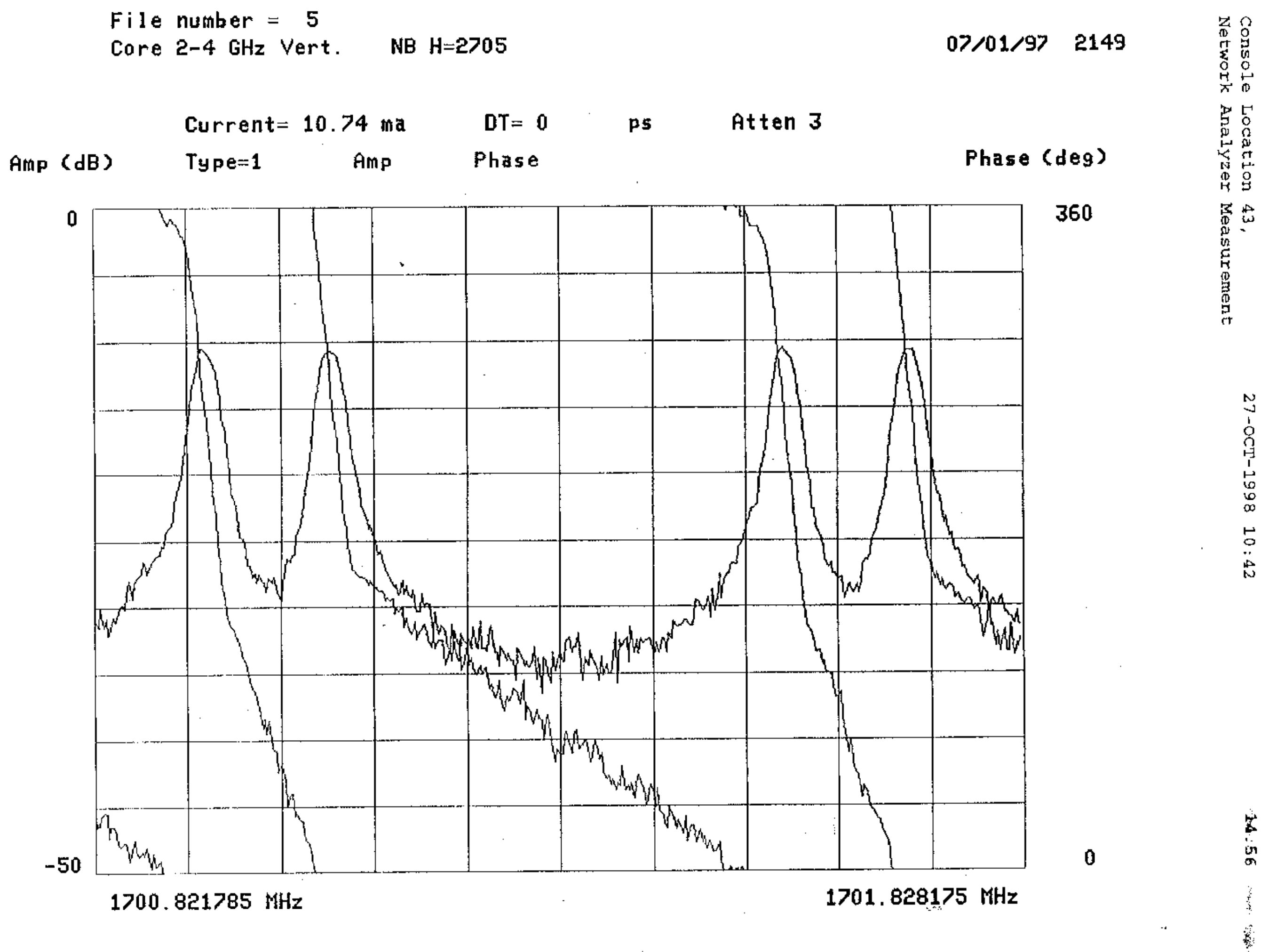
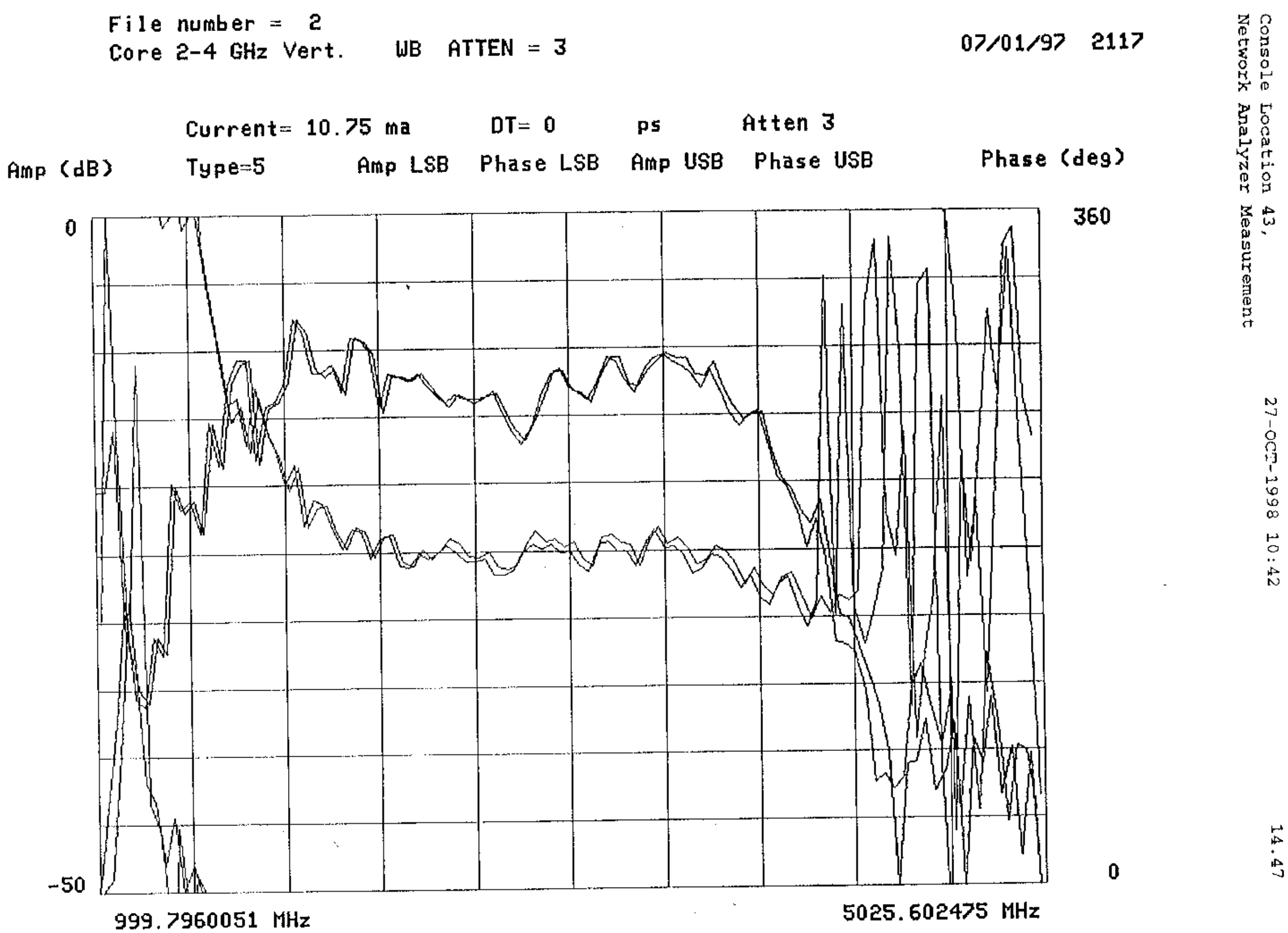
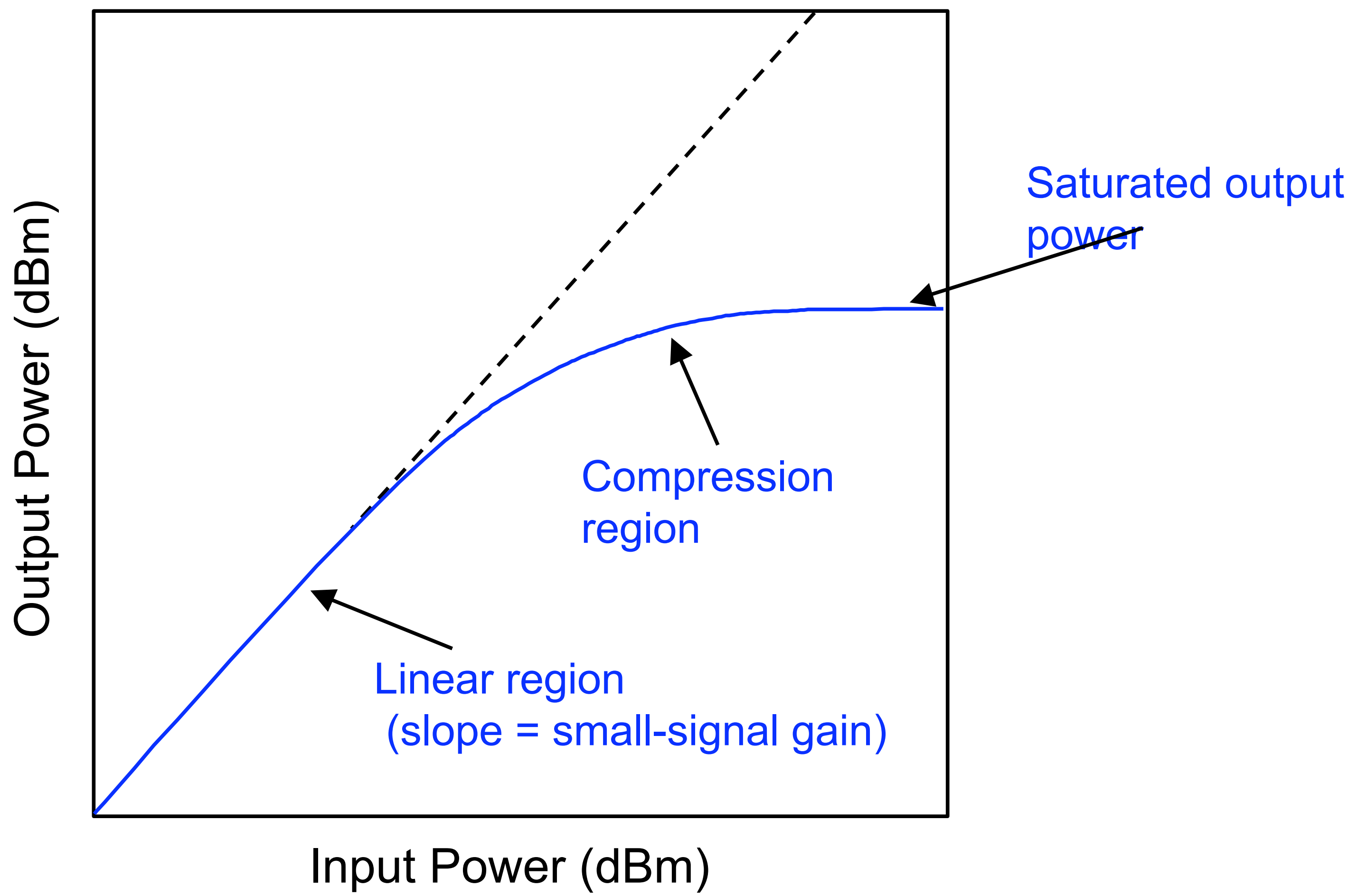
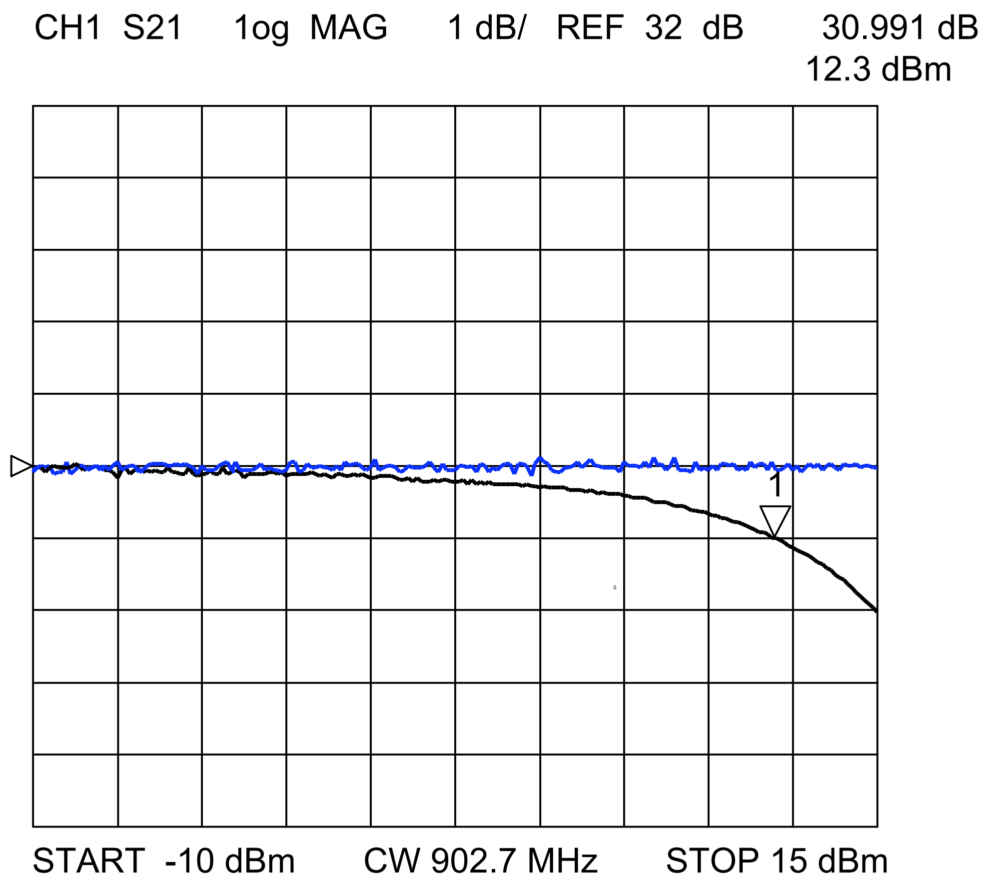

File number = 5
Core 2-4 GHz Vert. NB H=2705
07/01/97 2149
Current= 10.74 ma DT= 0 ps Atten 3
Amp (dB) Type=1 Amp Phase
Phase (deg)
0
360
-50
0
1700.821785 MHz
1701.828175 MHz
Console Location 43, Network Analyzer Measurement
27-OCT-1998 10:42
14:56


File number = 2
Core 2-4 GHz Vert. WB ATTEN = 3
07/01/97 2117
Current= 10.75 ma DT= 0 ps Atten 3
Amp (dB) Type=5 Amp LSB Phase LSB Amp USB Phase USB Phase (deg)
0
360
-50
0
999.7960051 MHz
5025.602475 MHz
Console Location 43,
Network Analyzer Measurement
27-OCT-1998 10:42
14.47

Power Sweeps - Compression



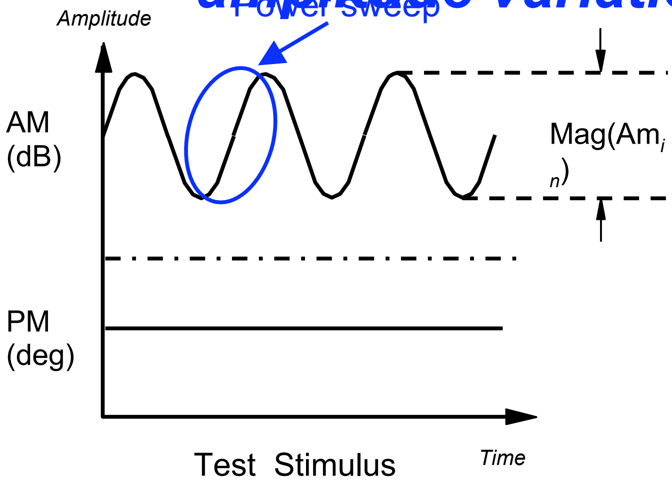
Power Sweep - Gain Compression

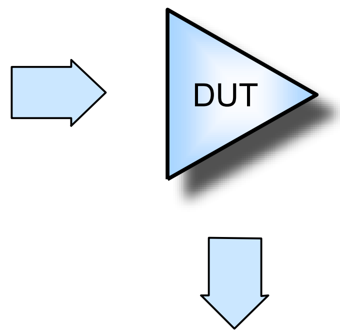


1 dB compression: input power resulting in 1 dB *drop* in gain

AM to PM Conversion

Measure of phase deviation caused by amplitude variations

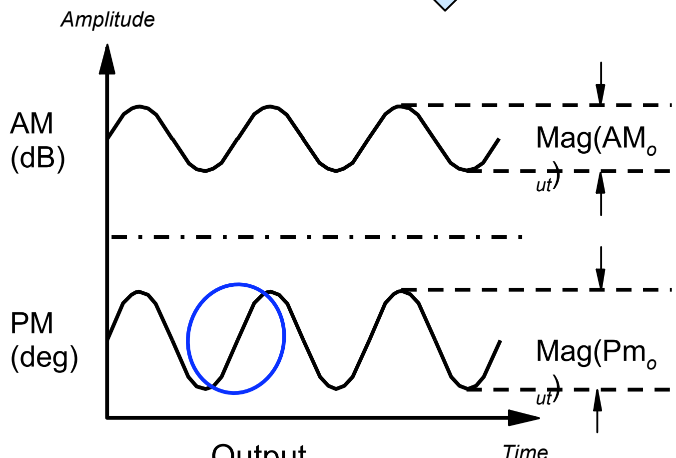


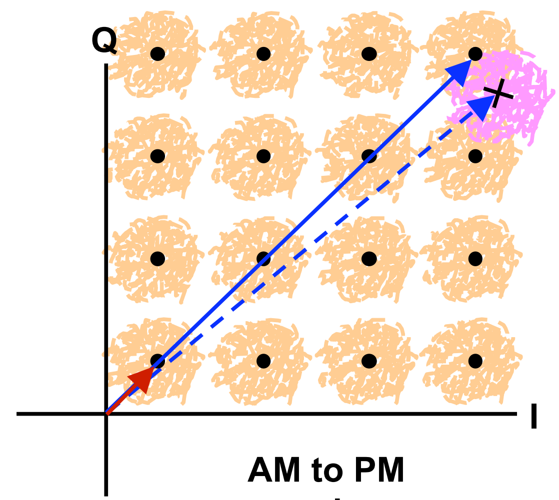


- AM can be undesired: supply ripple, fading, thermal
- AM can be desired: modulation (e.g. QAM)

AM - PM Conversion =

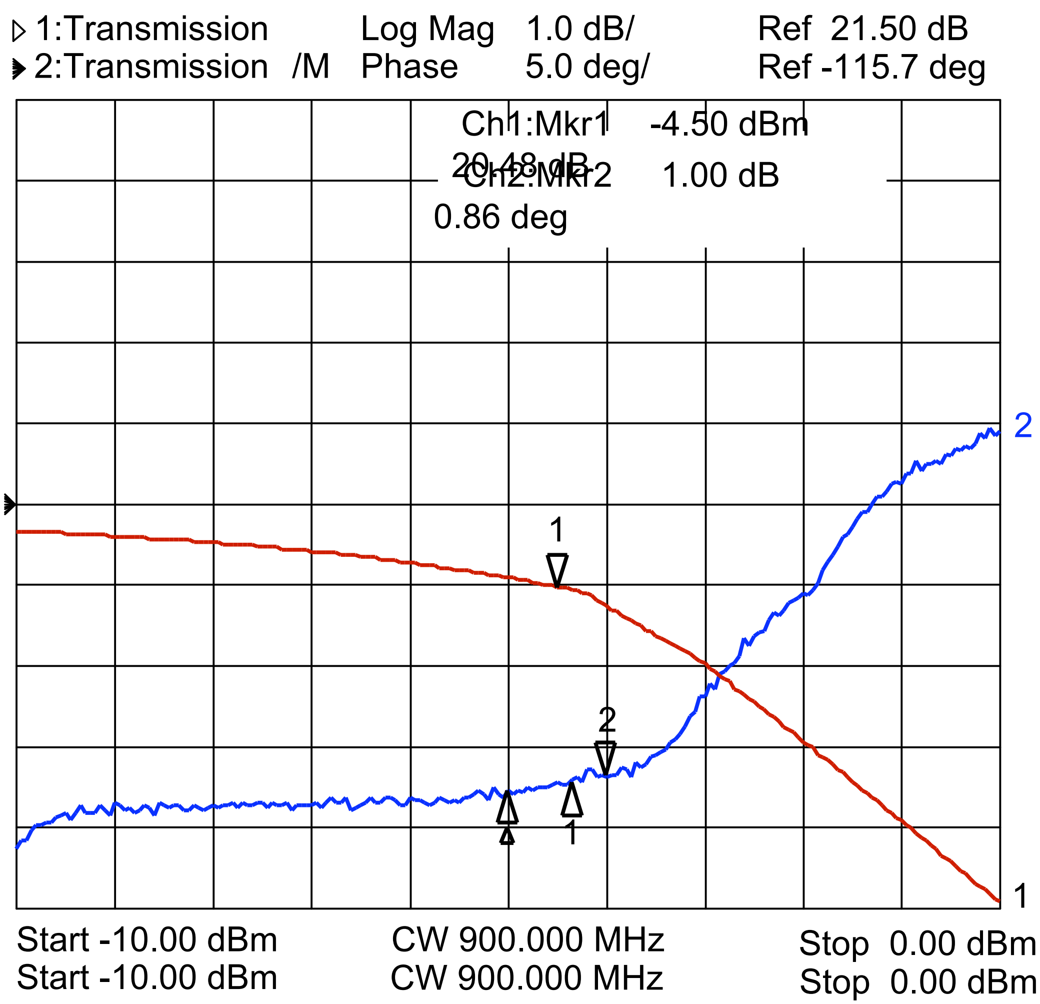
$$\frac{\text{Mag}(Pm_{out})}{\text{Mag}(Am_{in})} \quad (\text{deg/dB})$$





AM to PM conversion can cause bit errors

Measuring AM to PM Conversion



- Use transmission setup with a power sweep
- Display phase of S21
- AM - PM = 0.86 deg/dB

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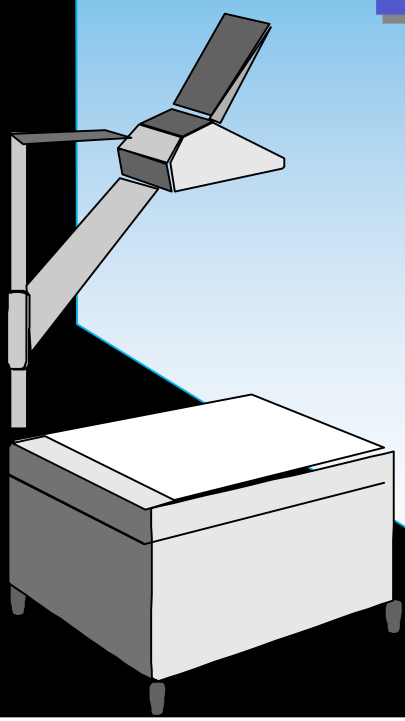
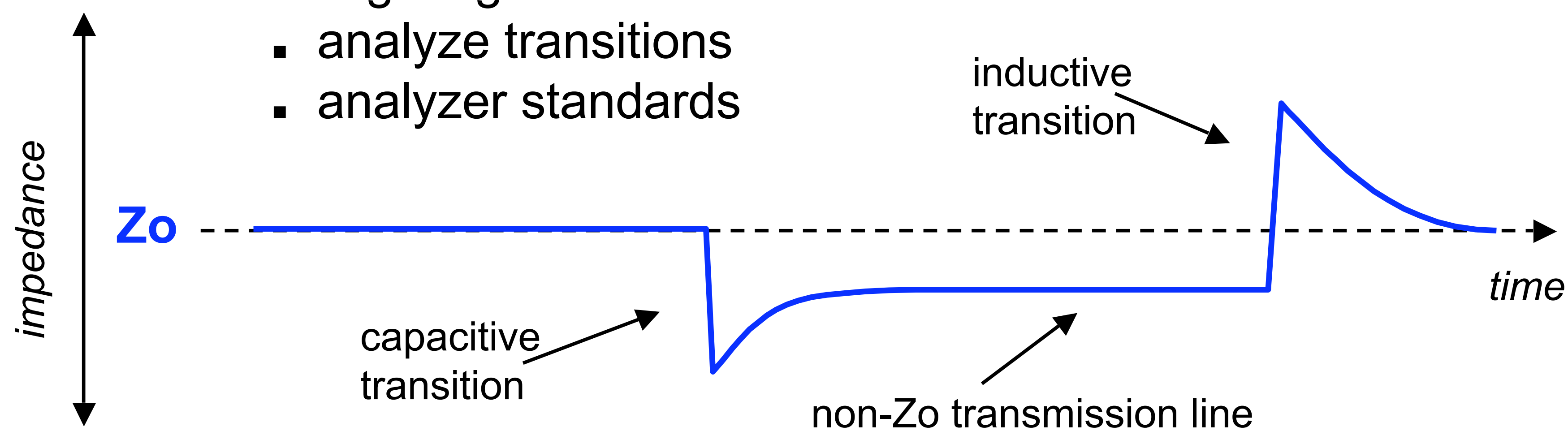
Agenda



- What measurements do we make?
- Network analyzer hardware
- Error models and calibration
- Example measurements
- Appendix
  - Advanced Topics
    - time domain
    - frequency-translating devices
    - high-power amplifiers
    - extended dynamic range
    - multiport devices
    - in-fixture measurements
    - crystal resonators
    - balanced/differential
  - Inside the network analyzer
  - Challenge quiz!

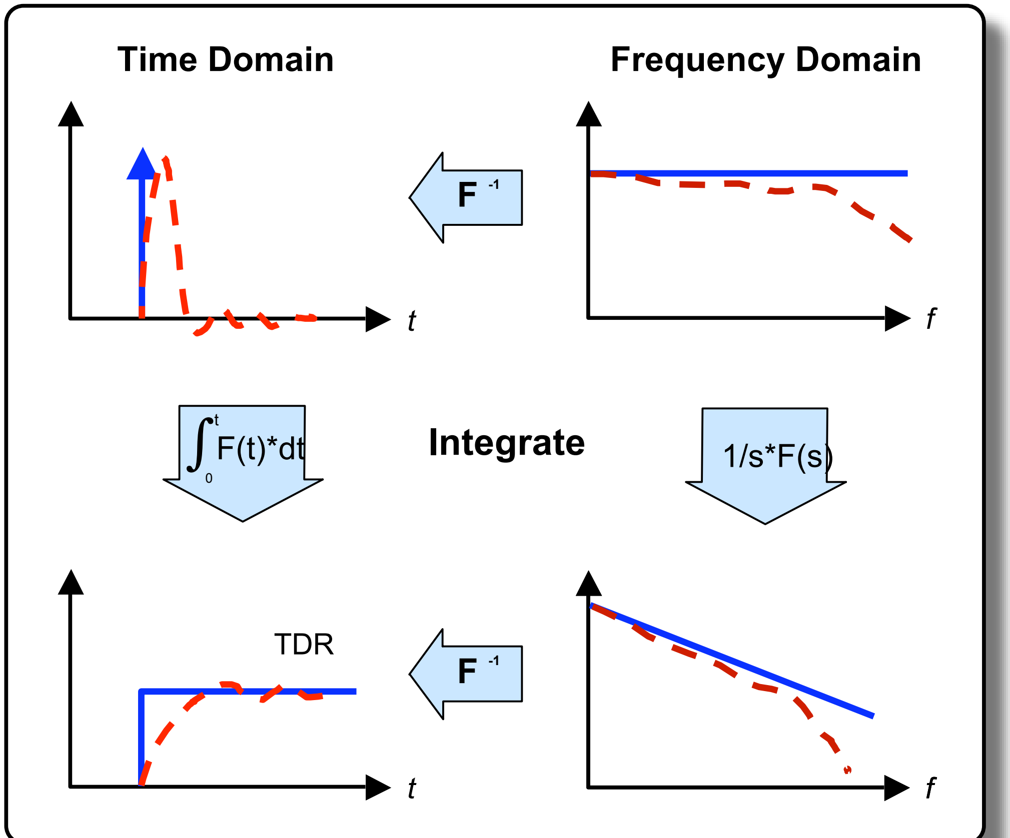
Time-Domain Reflectometry (TDR)

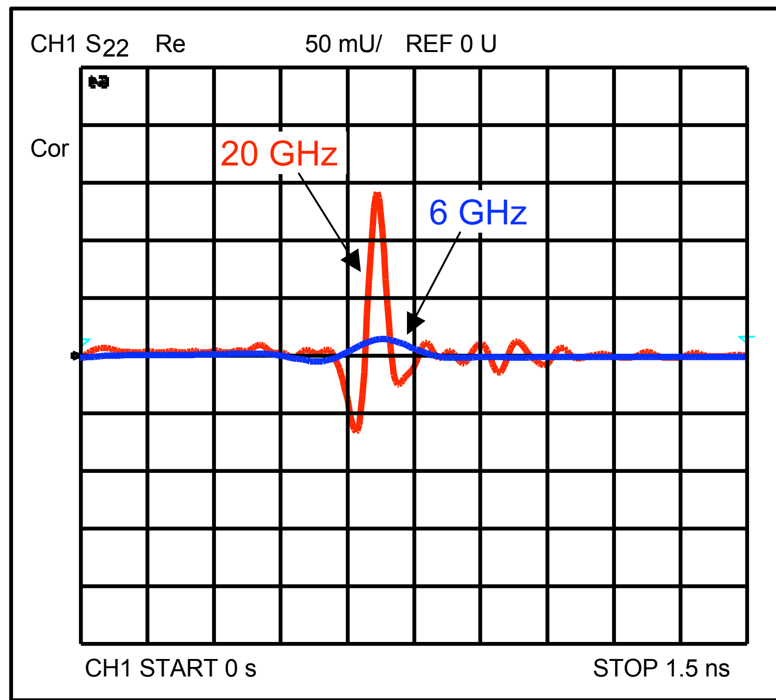
- What is TDR?
  - time-domain reflectometry
  - analyze impedance versus time
  - distinguish between inductive and capacitive transitions
- With gating:
  - analyze transitions
  - analyzer standards



TDR Basics Using a Network Analyzer

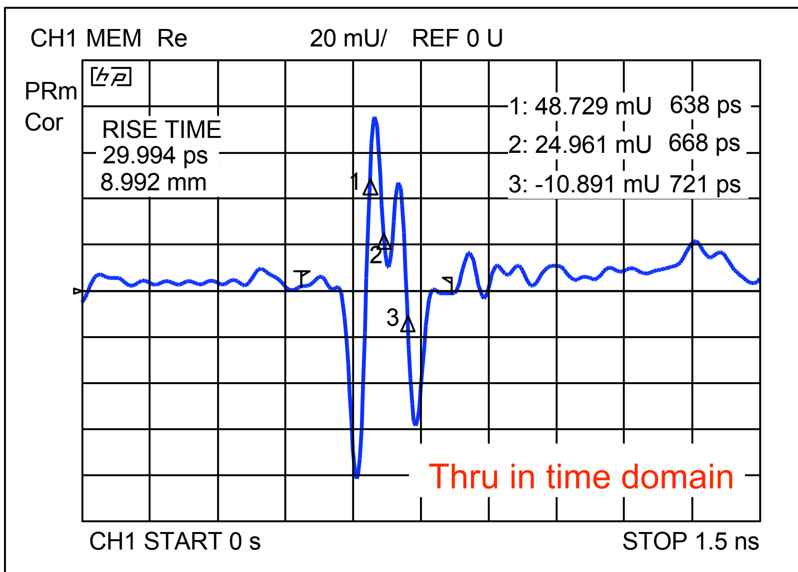
- start with broadband frequency sweep (often requires microwave VN/
- use inverse-Fourier transform to compute time-domain
- resolution inversely proportionate to frequency span

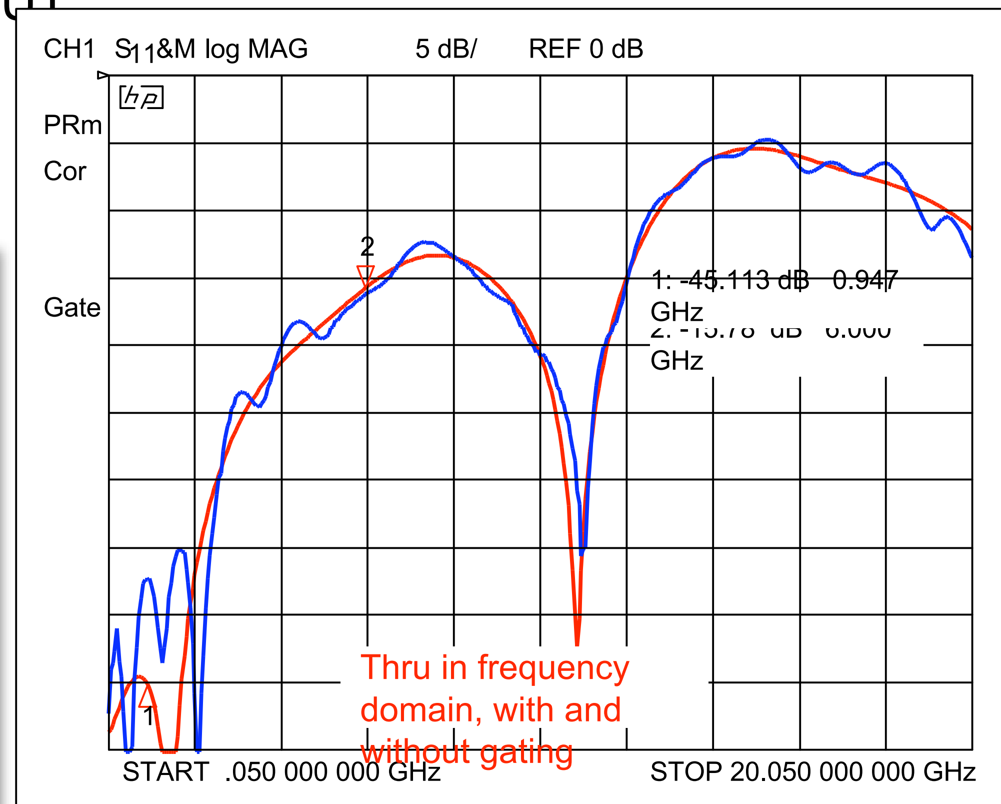




Time-Domain Gating

- TDR and gating can **remove** undesired reflections (a form of error **correction)**
- Only useful for **broadband** devices (a load or thru for example)
- Define **gate** to only include DUT
- Use two-port calibration





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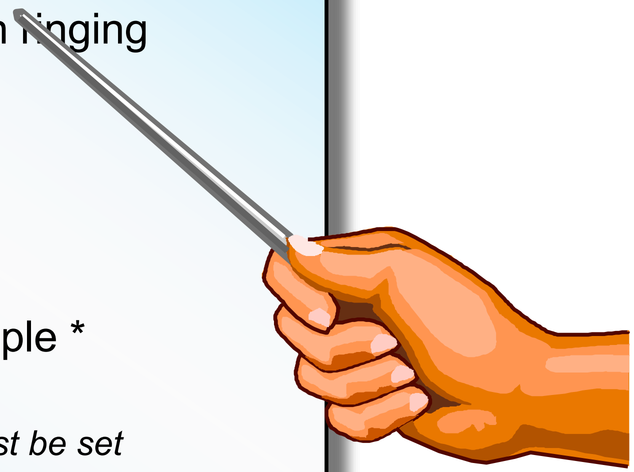
Ten Steps for Performing TDR

1. Set up desired frequency range (need wide span for good spatial resolution)
2. Under SYSTEM, transform menu, press "set freq low pass"
3. Perform one- or two-port calibration
4. Select S11 measurement *
5. Turn on transform (low pass step) *
6. Set format to real *
7. Adjust transform window to trade off rise time with ringing and overshoot *
8. Adjust start and stop times if desired
9. For gating:
   - set start and stop frequencies for gate
   - turn gating on *
   - adjust gate shape to trade off resolution with ripple *
10. To display gated response in frequency domain
   - turn transform off (leave gating on) *
   - change format to log-magnitude *



If using two channels (even if coupled), these parameters must be set independently for second channel

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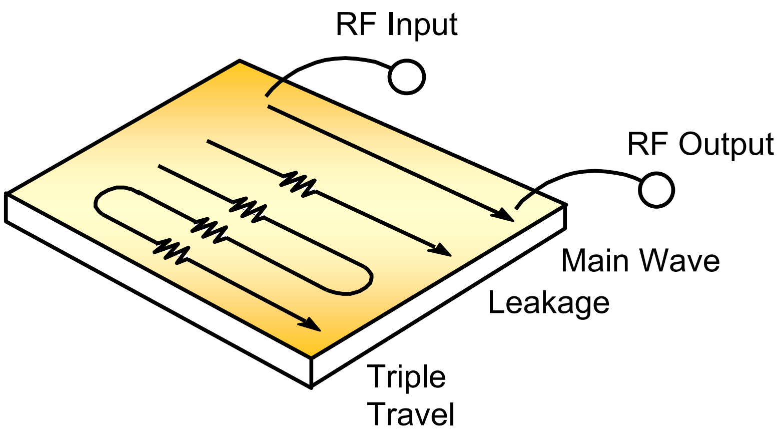
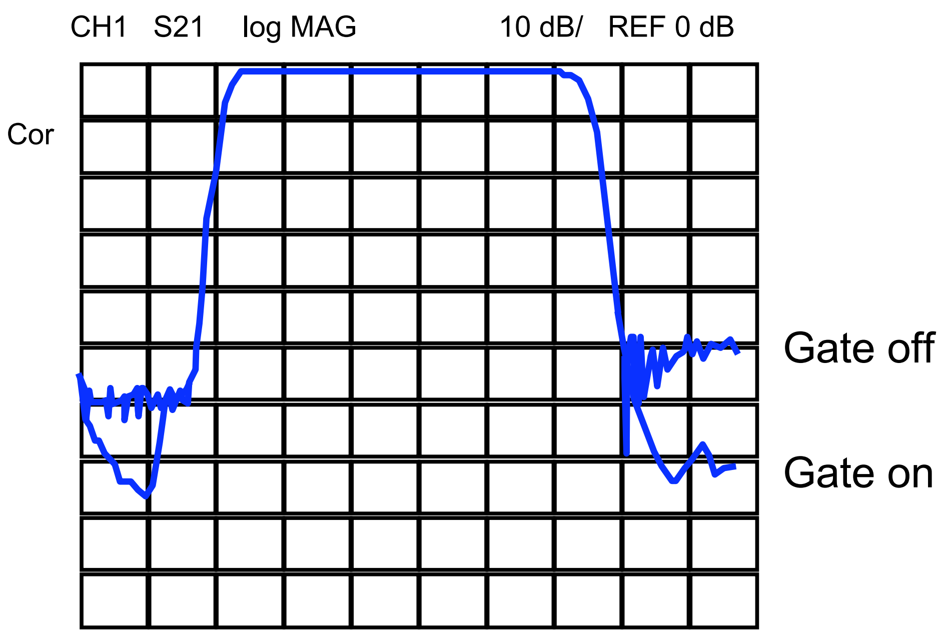
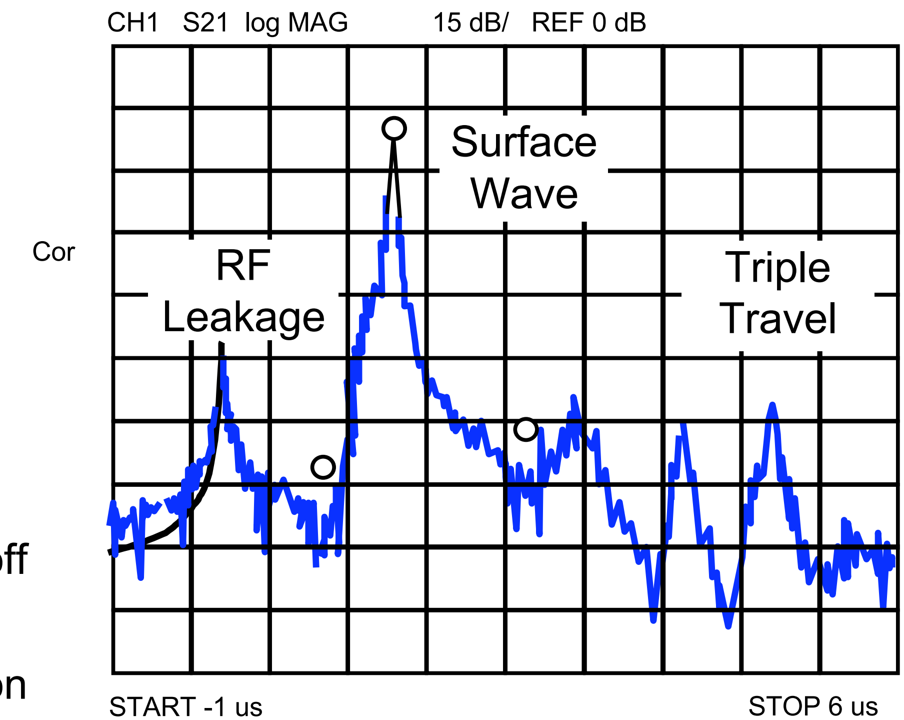
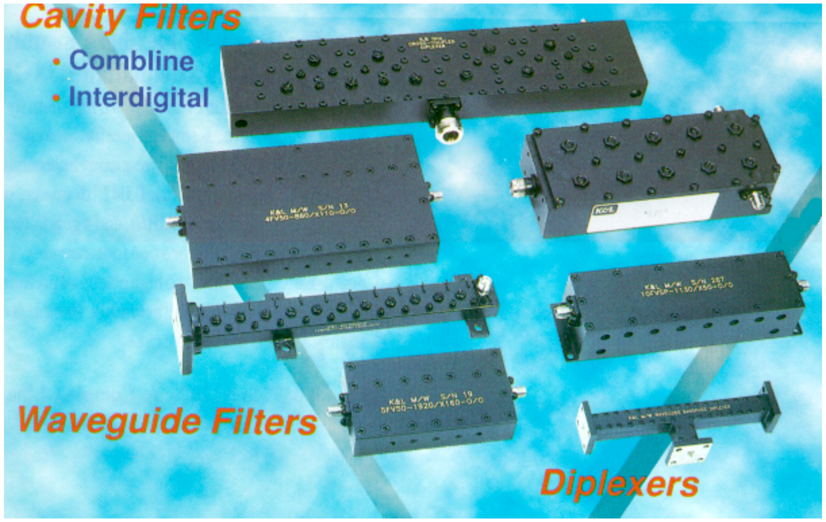
Time-Domain Transmission





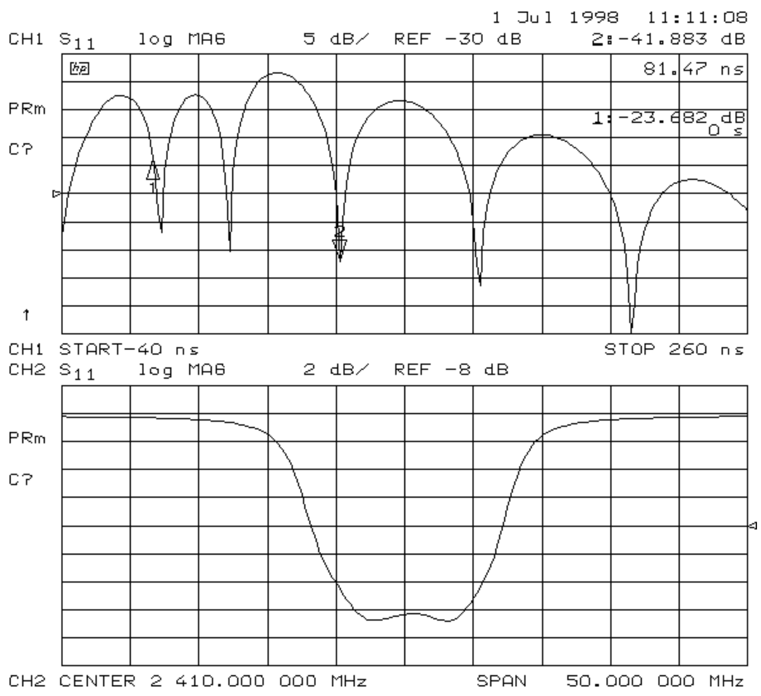


Time-Domain Filter Tuning



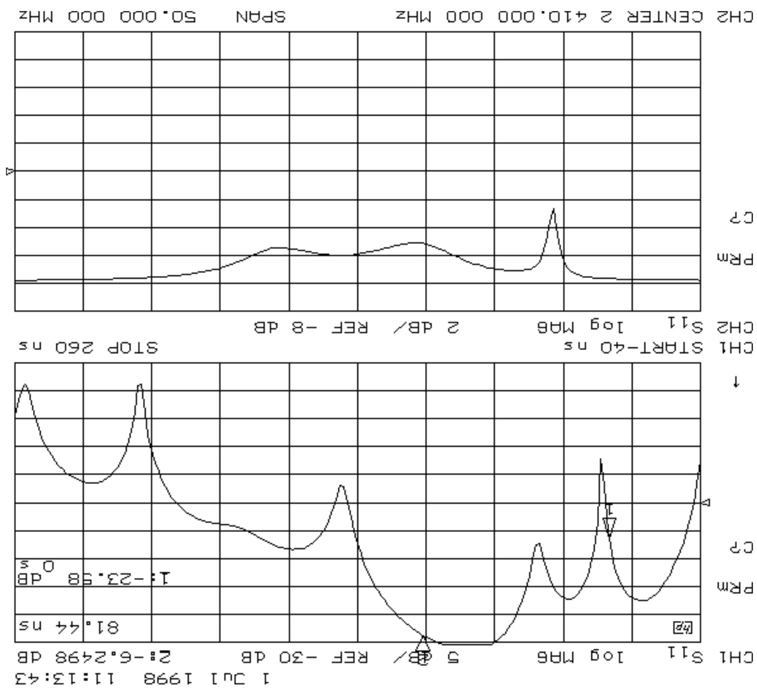
- Deterministic method used for tuning cavity-resonator filters
- Traditional frequency-domain tuning is very difficult:
  - lots of training needed
  - may take 20 to 90 minutes to tune a single filter
- Need VNA with fast sweep speeds and fast time-domain processing

Filter Reflection in Time Domain



- Set analyzer’s center frequency
  = center frequency of the filter
- Measure S_{11} or S_{22} in the time domain
- Nulls in the time-domain response correspond to individual resonators in filter

Tuning Resonator #3



- Easier to identify mistuned resonator in time-domain: null #3 is missing
- Hard to tell which resonator is mistuned from frequency-domain response
- Adjust resonators by minimizing null
- Adjust coupling apertures using the peaks in-between the dips

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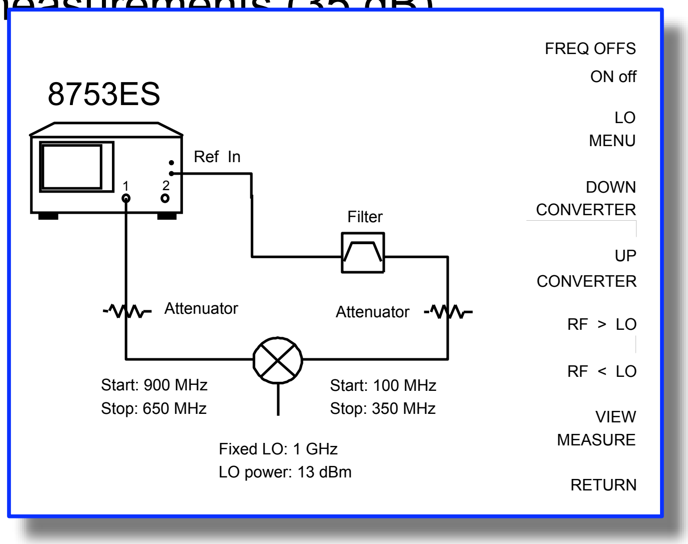
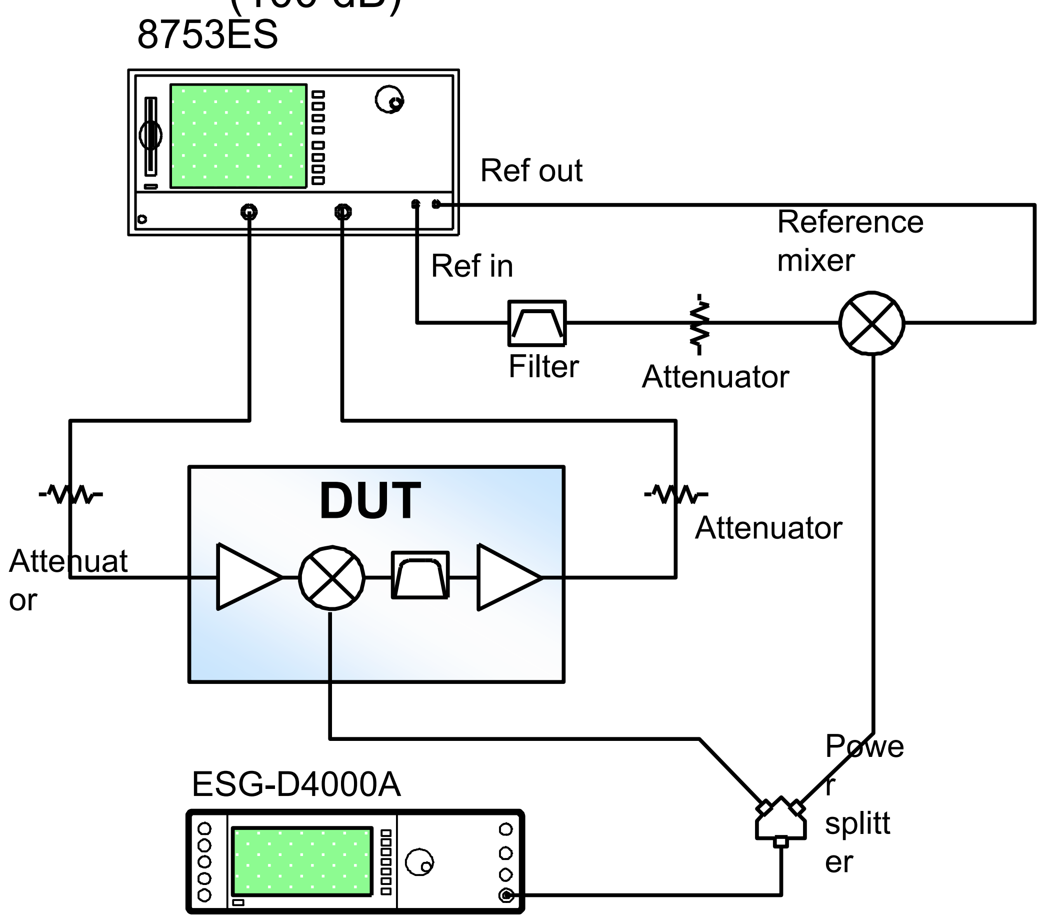
Frequency-Translating Devices

Medium-dynamic range measurements (35 dB)



High-dynamic range measurements (100 dB)

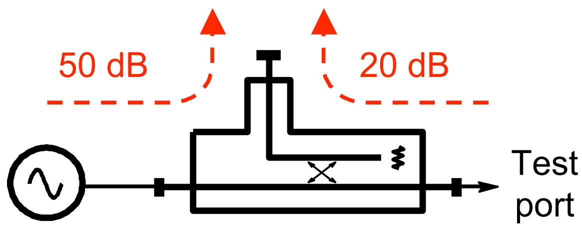


Directional Coupler *Directivity*

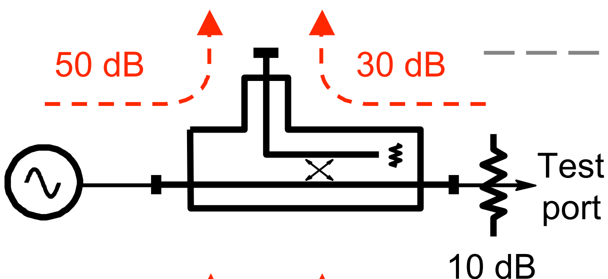
$$\text{Directivity} = \frac{\text{Coupling Factor}_{(fwd)} \times \text{Loss}_{(through\ arm)}}{\text{Isolation}_{(rev)}}$$

Directivity (dB) = Isolation (dB) - Coupling Factor (dB) - Loss (dB)

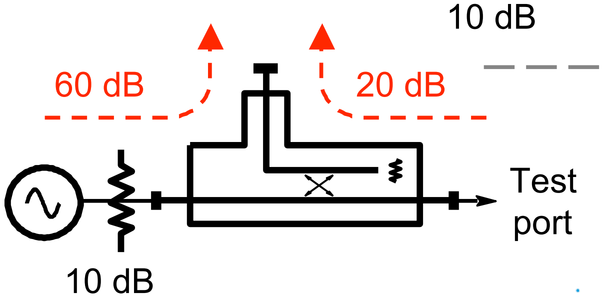
Examples:



Directivity = 50 dB - 20 dB = 30 dB

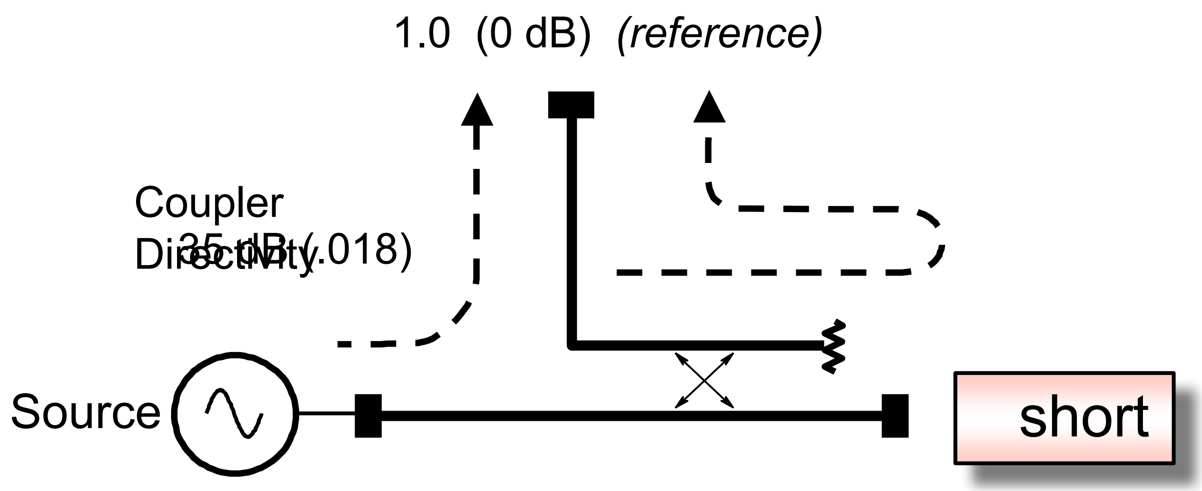


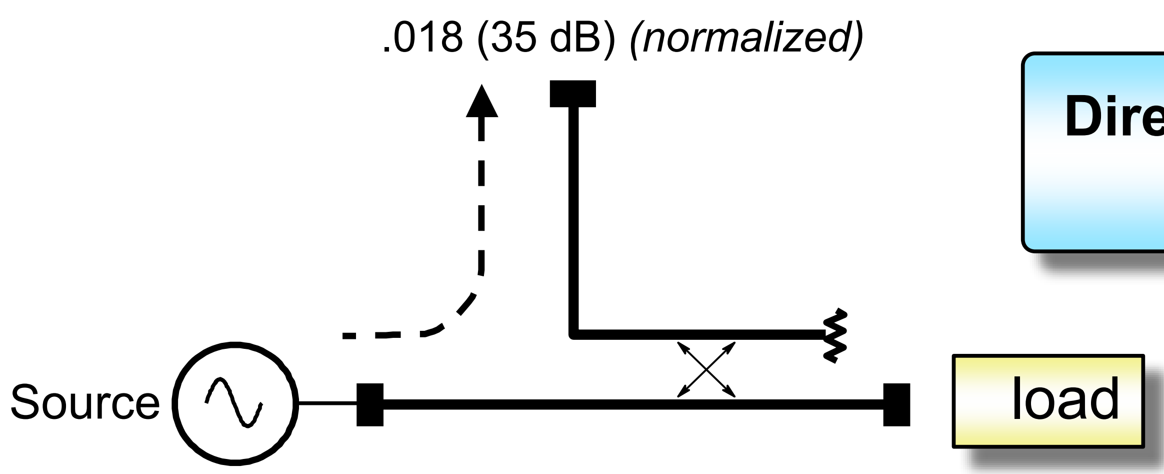
Directivity = 50 dB - 30 dB - 10 dB = 10 dB



Directivity = 60 dB - 20 dB - 10 dB = 30 dB

One Method of Measuring Coupler Directivity





Directivity = 35 dB - 0 dB

= 35 dB

Assume perfect load (no reflection)

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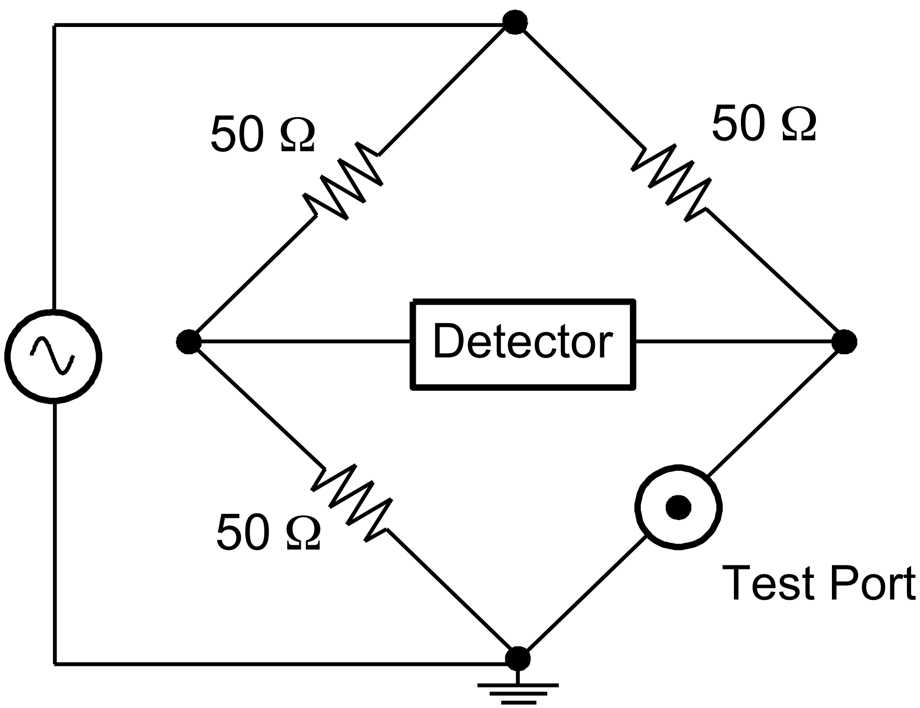
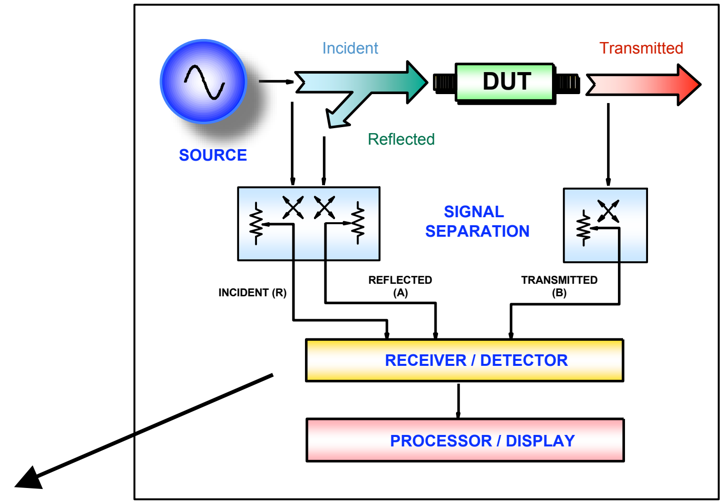
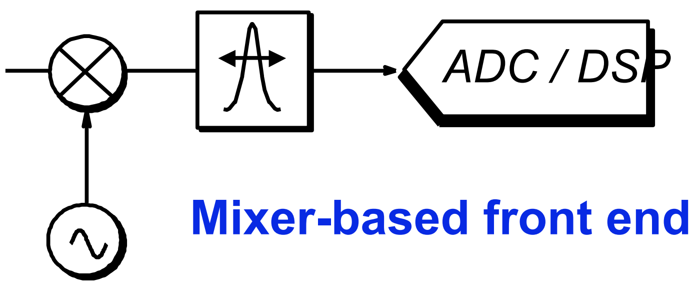
Directional Bridge



- 50-ohm load at test port balances
  the bridge -- detector reads zero
- Non-50-ohm load imbalances bridge
- Measuring magnitude and phase of imbalance gives complex impedance
- "Directivity" is difference between maximum and minimum balance

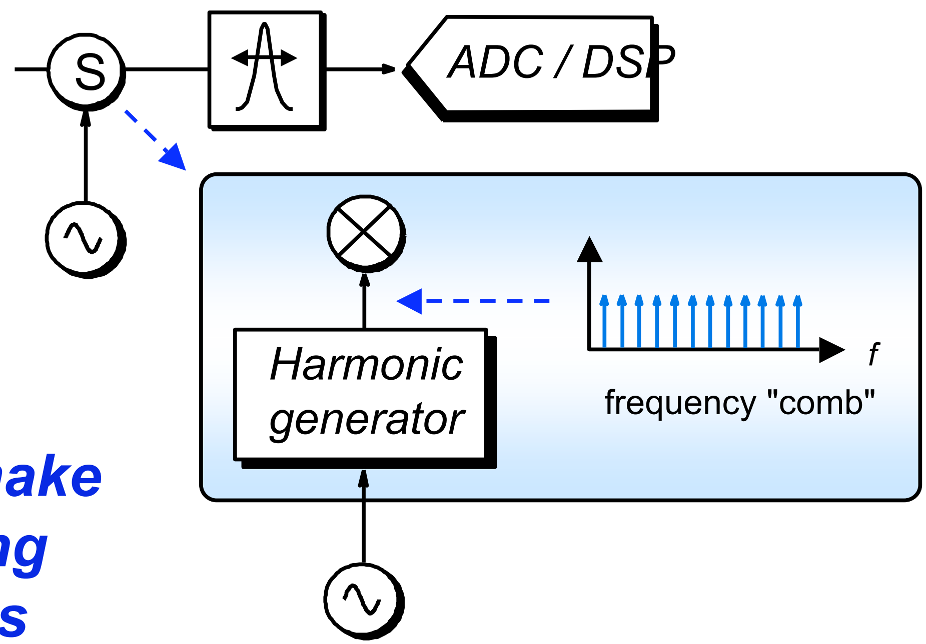
NA Hardware: Front Ends, Mixers Versus Samplers





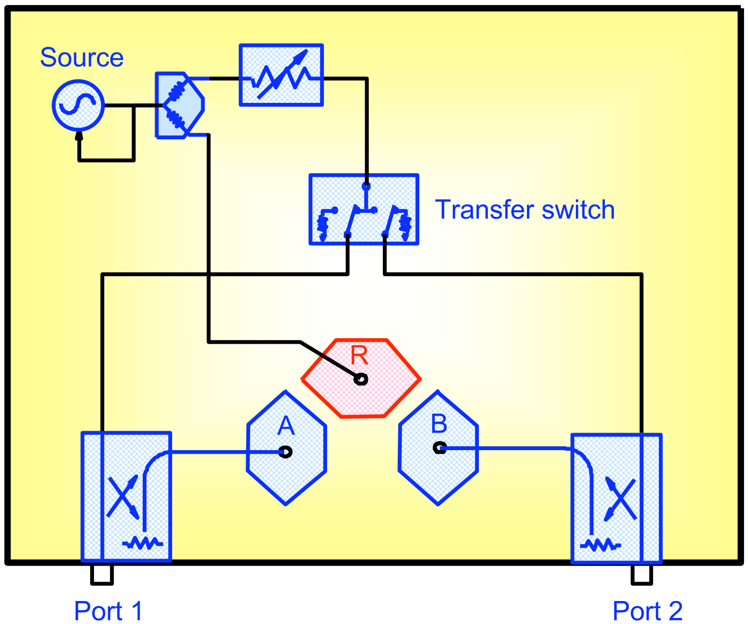
Mixer-based front end

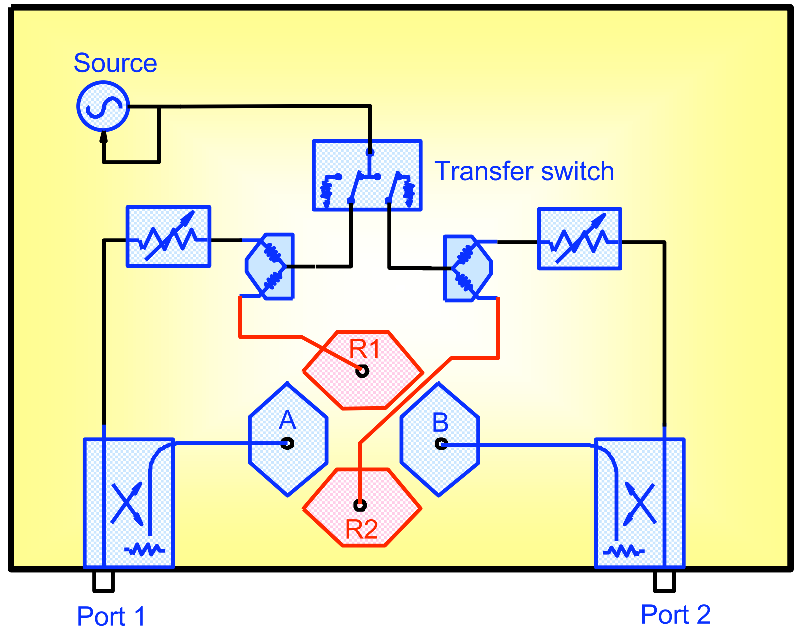
Sampler-based front end



It is cheaper and easier to make broadband front ends using samplers instead of mixers

Three Versus Four-Receiver Analyzers





3 receivers

- more economical
- TRL*, LRM* cals only
- includes:
  - 8753ES
  - 8720ES (standard)

4 receivers

- more expensive
- true TRL, LRM cals
- includes:
  - 8720ES (option 400)
  - 8510C

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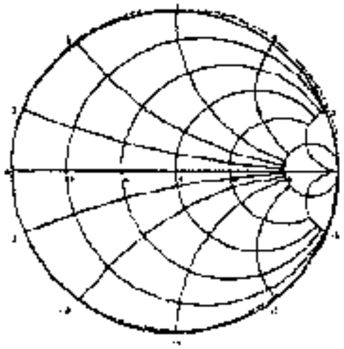
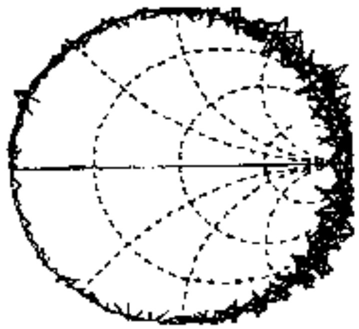
Why Are Four Receivers Better Than Three?

TRL





TRL*

8720ES Option 400 adds fourth sampler, allowing full TRL calibration

- **TRL***
  - assumes the source and load match of a test port are equal (port symmetry between forward and reverse measurements)
  - this is only a fair assumption for three-receiver network analyzers
- **TRL**
  - four receivers are necessary to make the required measurements
  - TRL and TRL* use identical calibration standards
- **In noncoaxial applications,** TRL achieves better source and load match correction than TRL*
- **What about coaxial applications?**
  - SOLT is usually the preferred calibration method
  - coaxial TRL can be more accurate than SOLT, but not commonly used

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Challenge Quiz

1. Can filters cause distortion in communications systems?
   A. Yes, due to impairment of phase and magnitude response
   B. Yes, due to nonlinear components such as ferrite inductors
   C. No, only active devices can cause distortion
   D. No, filters only cause linear phase shifts
   E. Both A and B above

2. Which statement about transmission lines is false?
   A. Useful for efficient transmission of RF power
   B. Requires termination in characteristic impedance for low VSWR
   C. Envelope voltage of RF signal is independent of position along line
   D. Used when wavelength of signal is small compared to length of line
   E. Can be realized in a variety of forms such as coaxial, waveguide, microstri

3. Which statement about narrowband detection is false?
   A. Is generally the cheapest way to detect microwave signals
   B. Provides much greater dynamic range than diode detection
   C. Uses variable-bandwidth IF filters to set analyzer noise floor
   D. Provides rejection of harmonic and spurious signals
   E. Uses mixers or samplers as downconverters

Challenge Quiz (continued)

4. Maximum dynamic range with narrowband detection is defined as:

A. Maximum receiver input power minus the stopband of the device under te

B. Maximum receiver input power minus the receiver's noise floor

C. Detector 1-dB-compression point minus the harmonic level of the source

D. Receiver damage level plus the maximum source output power

E. Maximum source output power minus the receiver's noise floor

5. With a T/R analyzer, the following error terms can be corrected:

A. Source match, load match, transmission tracking

B. Load match, reflection tracking, transmission tracking

C. Source match, reflection tracking, transmission tracking

D. Directivity, source match, load match

E. Directivity, reflection tracking, load match

6. Calibration(s) can remove which of the following types of measurement

A. Systematic and drift

B. Systematic and random

C. Random and drift

D. Repeatability and systematic

E. Repeatability and drift

Challenge Quiz (continued)

7. Which statement about TRL calibration is false?

A. Is a type of two-port error correction
B. Uses easily fabricated and characterized standards
C. Most commonly used in noncoaxial environments
D. Is not available on the 8720ES family of microwave network analyzers
E. Has a special version for three-sampler network analyzers

8. For which component is it hardest to get accurate transmission and reflection measurements when using a T/R network analyzer?

A. Amplifiers because output power causes receiver compression
B. Cables because load match cannot be corrected
C. Filter stopbands because of lack of dynamic range
D. Mixers because of lack of broadband detectors
E. Attenuators because source match cannot be corrected

9. Power sweeps are good for which measurements?

A. Gain compression
B. AM to PM conversion
C. Saturated output power

Answers to Challenge Quiz

1. E
2. C
3. A
4. B
5. C
6. A
7. D
8. B
9. E